

DOA Estimation and Achievable Rate Analysis for 3D Massive MIMO in Aeronautical Communication Systems

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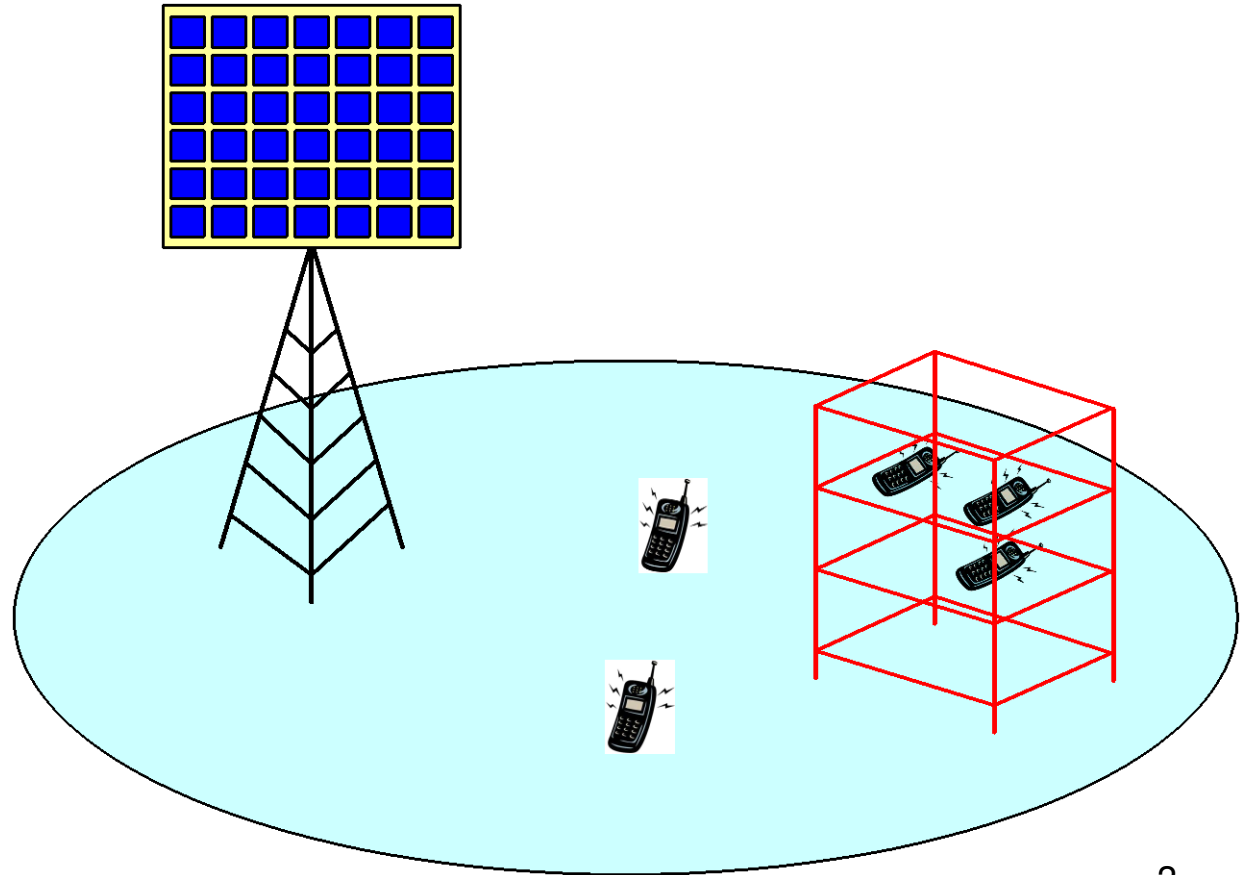
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Outline

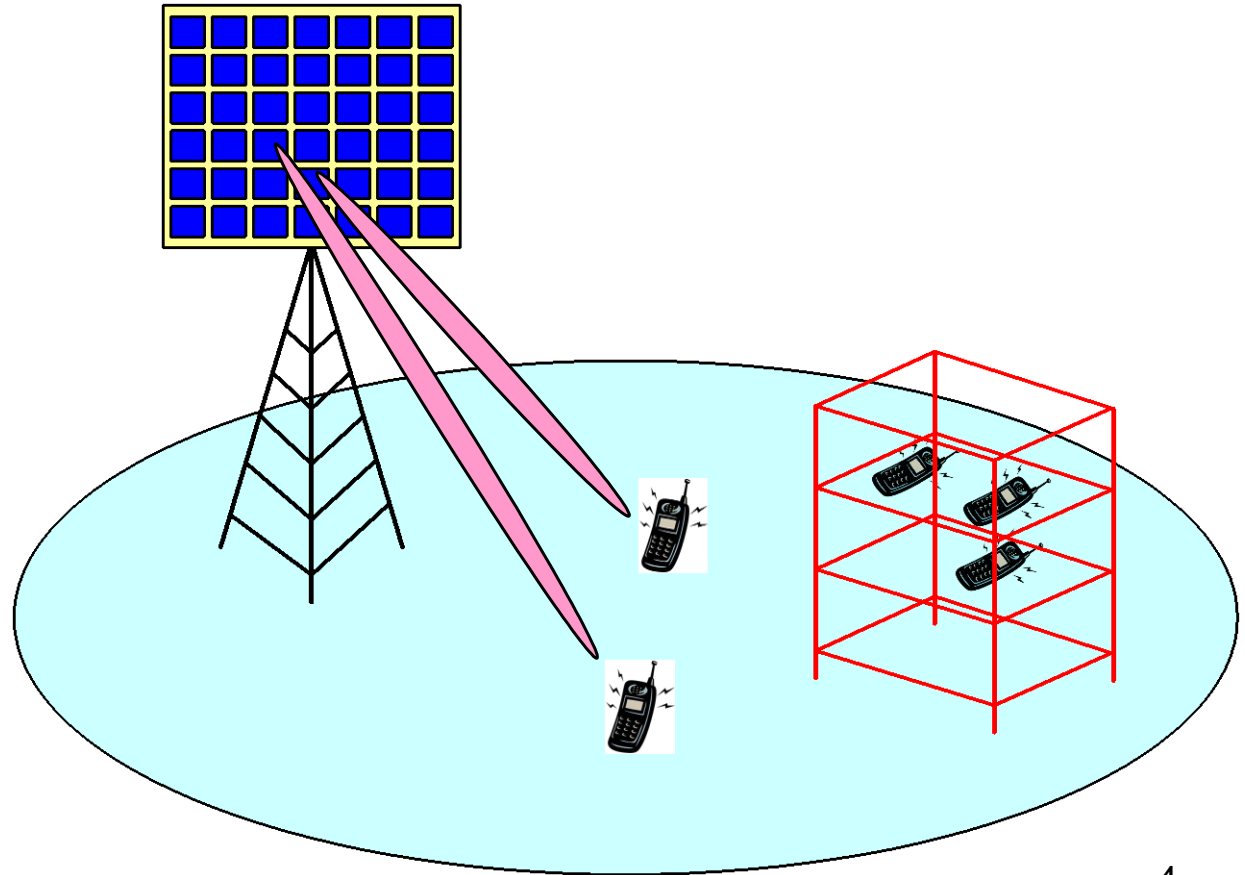
- Motivation
- DOA estimation algorithm
- Channel model
- Contribution:
 - MSE characterization.
 - Rate analysis.



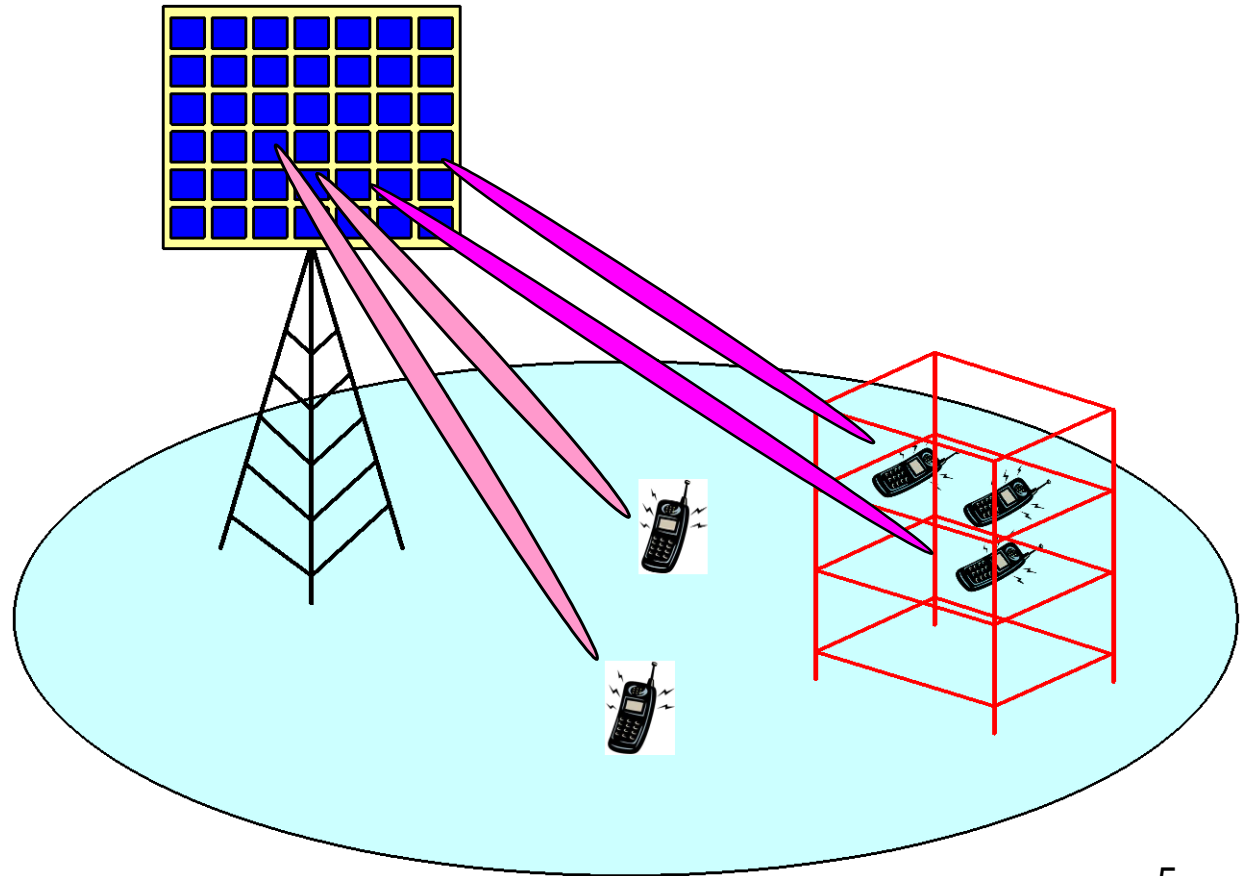
3D massive MIMO systems



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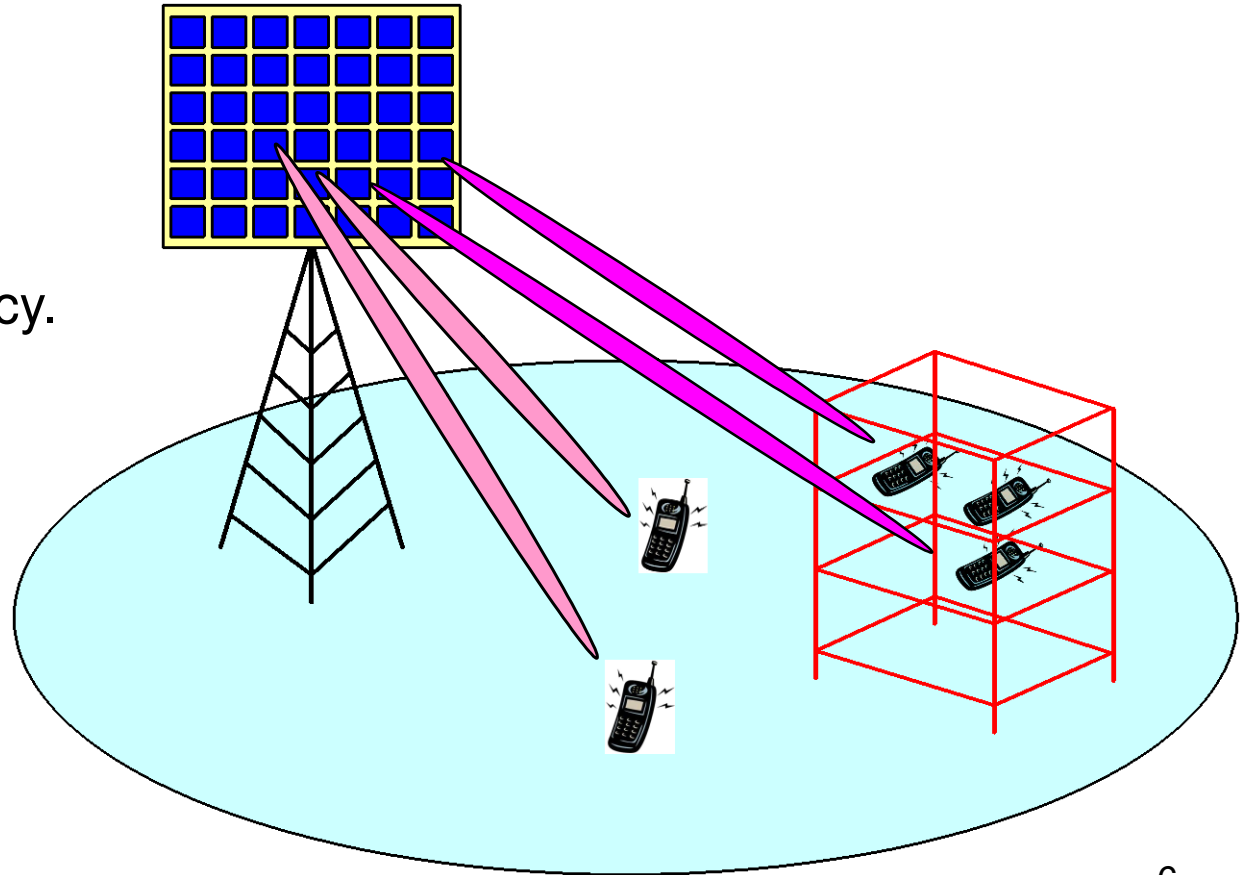


3D massive MIMO systems



3D massive MIMO systems

- Spectral efficiency.
- Spatial diversity.

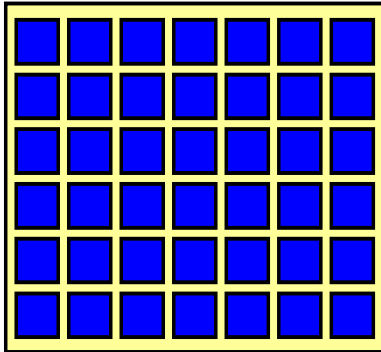


Why DOA estimation is important in massive MIMO systems?



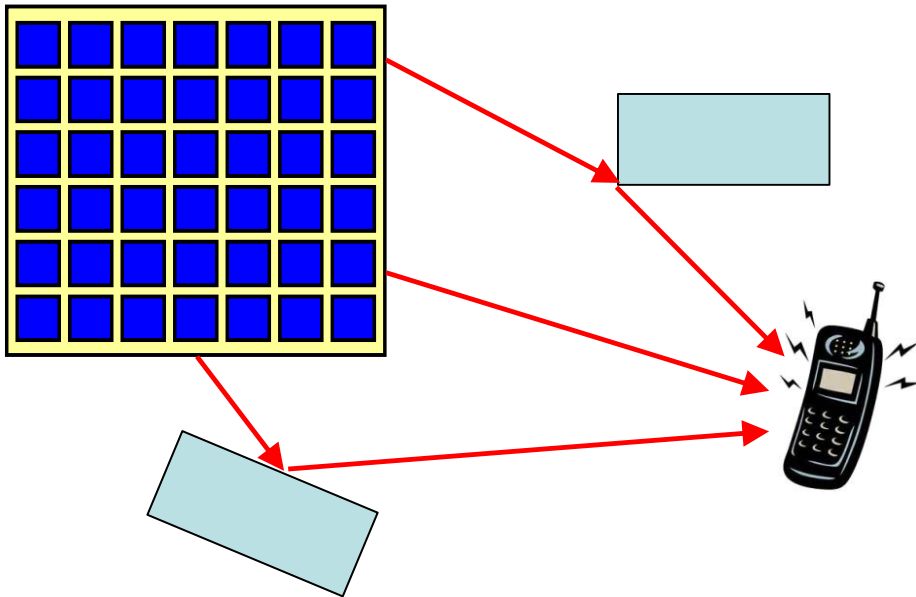
Why DOA estimation is important in massive MIMO systems?

- Wireless communications channel



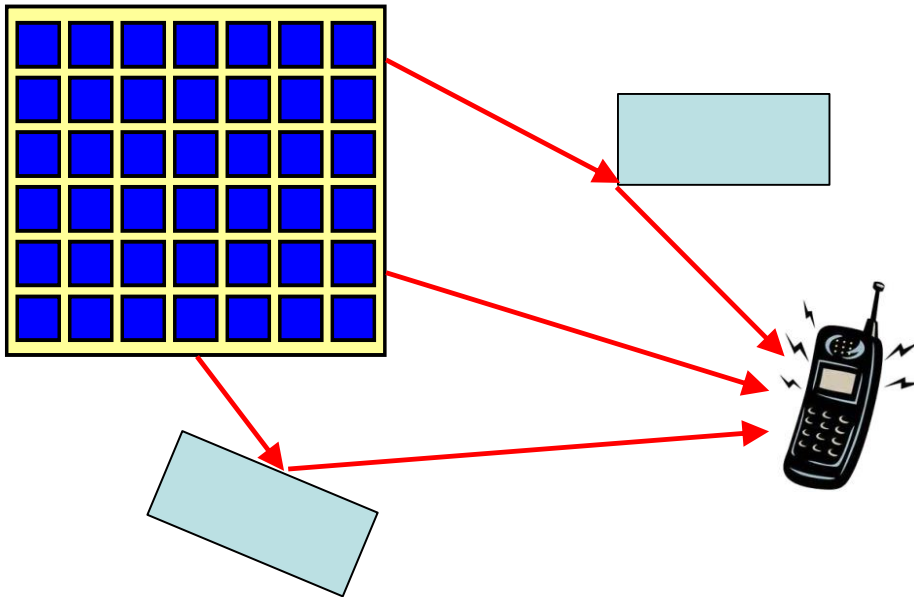
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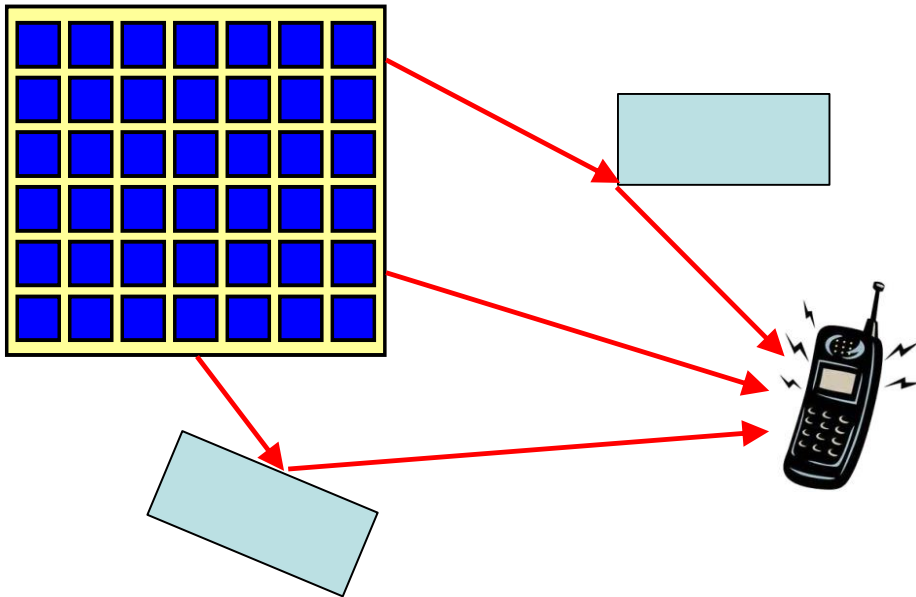
➤ Wireless communications channel



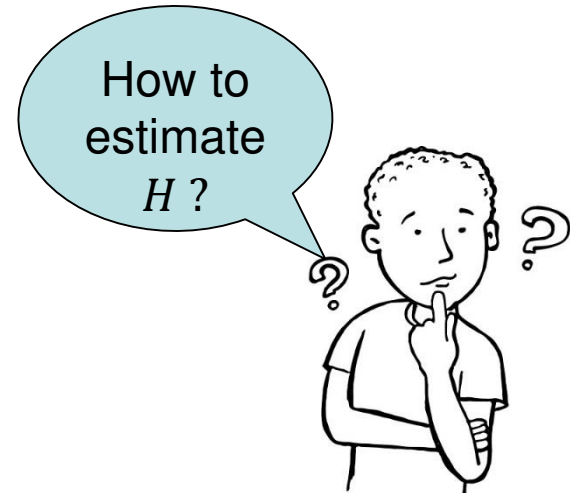
$$H = \begin{bmatrix} H(1,1) & \cdots & H(1,N) \\ \vdots & \ddots & \vdots \\ H(M,1) & \cdots & H(M,N) \end{bmatrix}$$

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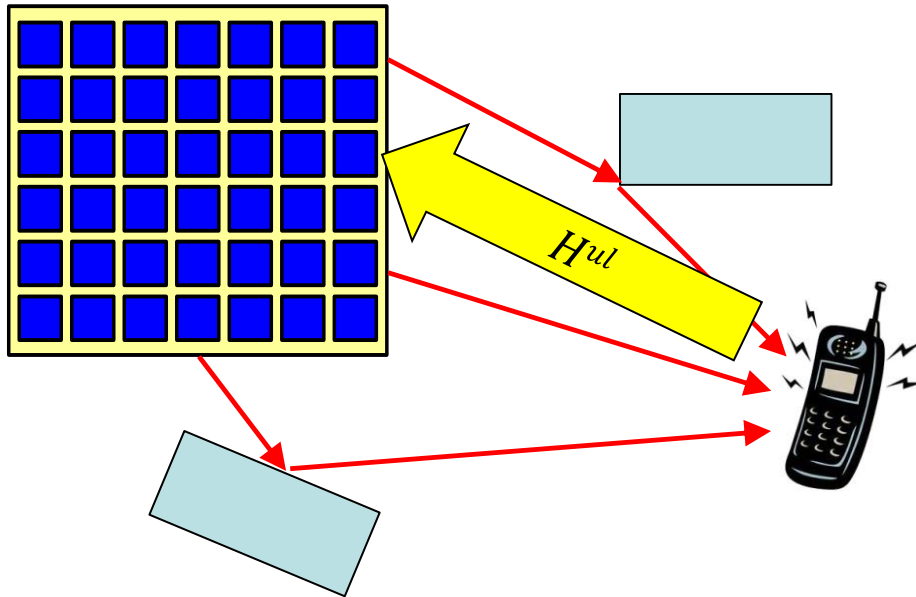


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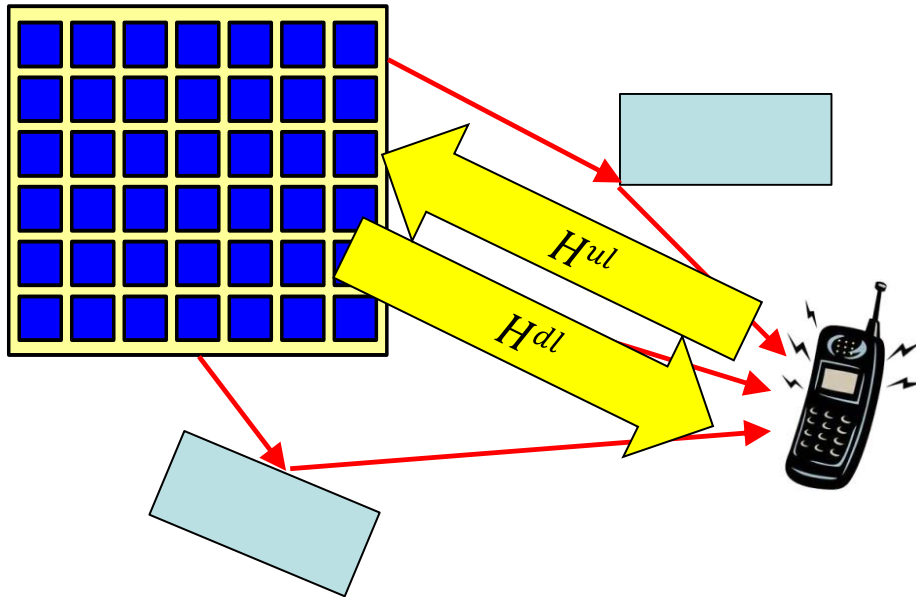
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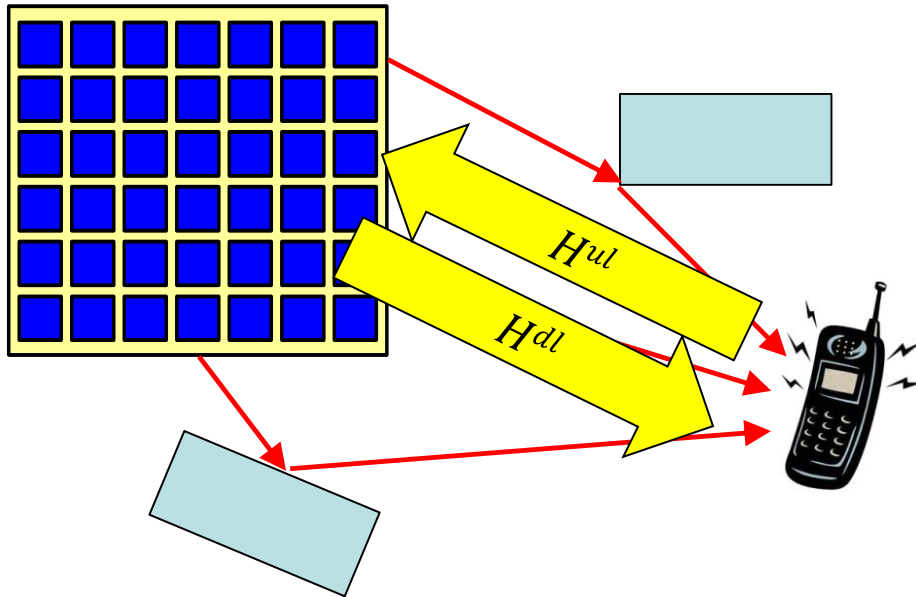
➤ Traditional and alternative ways



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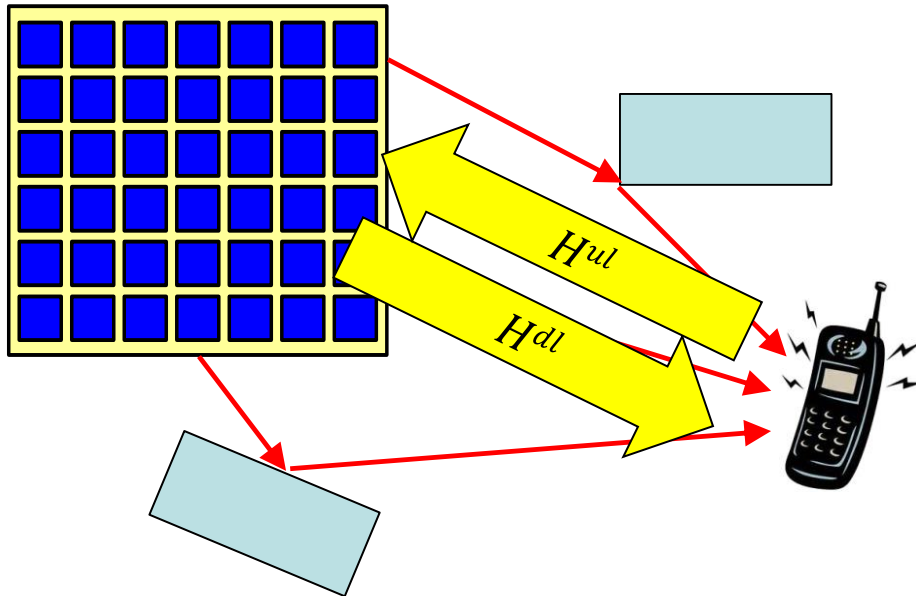


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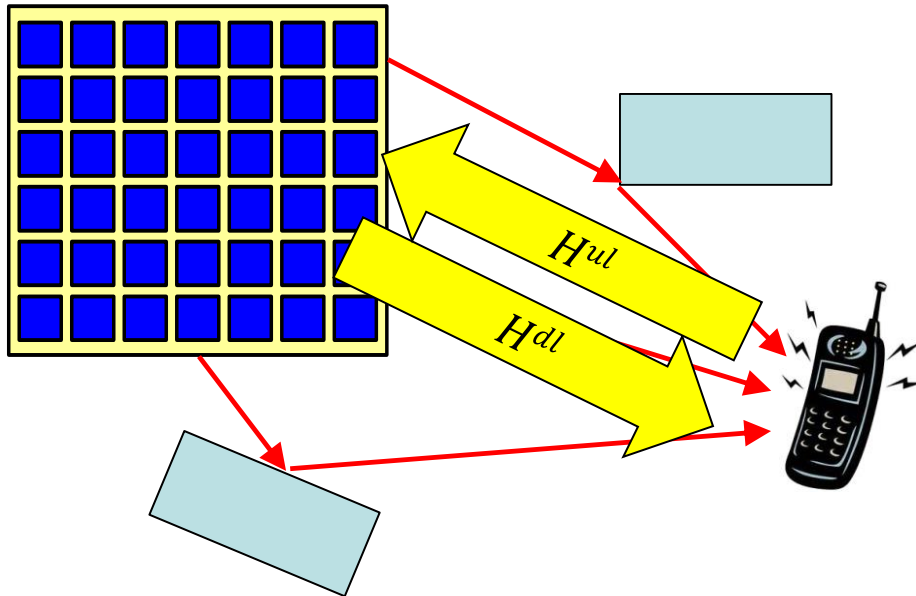
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Traditionally: Completely rely on the channel feedback

Alternatively: Due to the limited number of paths,

$$H = f(\theta, \varphi)$$

DOA estimation algorithm



DOA estimation algorithm

- Unitary **E**stimation of **S**ignal **P**arameters via **R**otational **I**nvariance **T**echniques (***ESPRIT***).



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 - Other algorithms are either highly computationally intensive, such as Multiple Signal Classification (MUSIC), or not accurate, such as DFT-based approaches.
 - Compared to ESPRIT, unitary ESPRIT processes real-value data from start to end.



Unitary ESPRIT algorithm



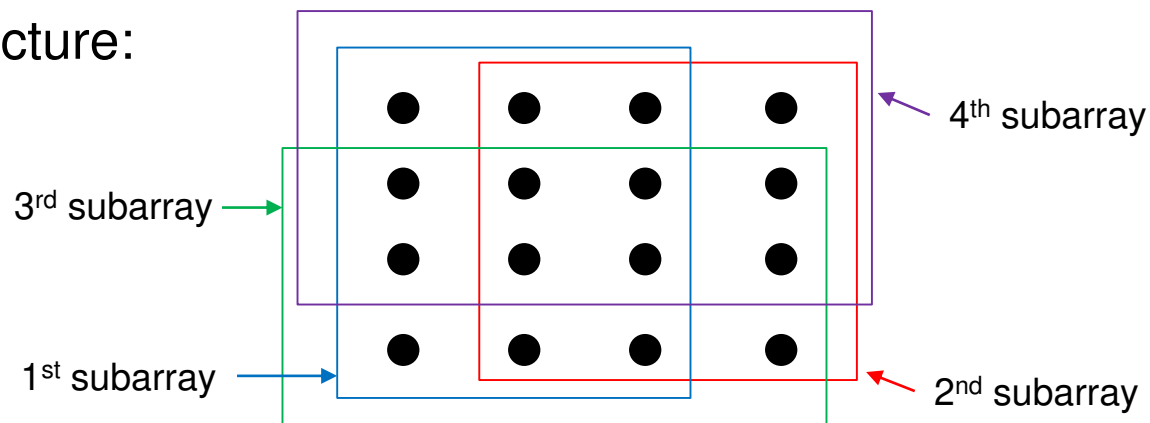
Unitary ESPRIT algorithm

- Array structure:



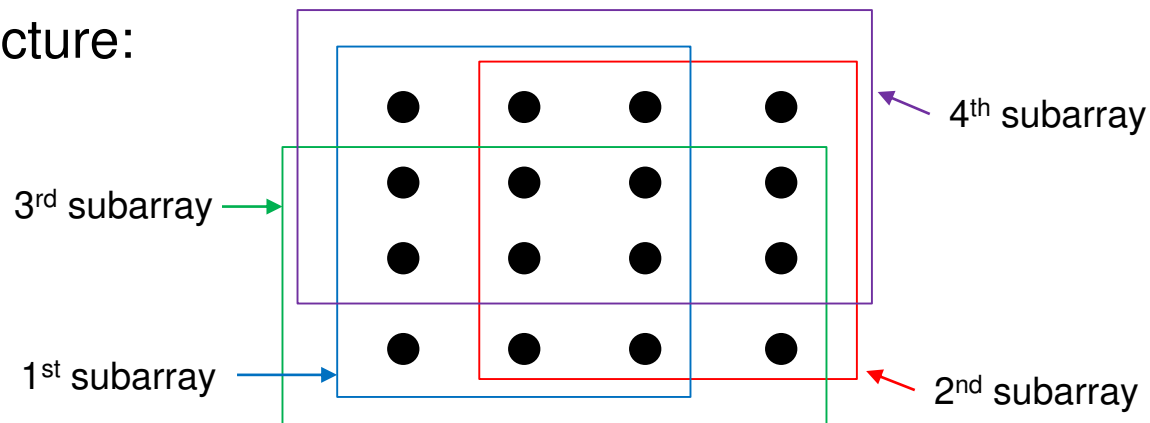
Unitary ESPRIT algorithm

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Unitary ESPRIT algorithm

➤ Array structure:



- This property leads to the rotational invariance of signal subspaces spanned by the data vectors associated with the spatially displaced subarrays [1].

[1] "Introduction to direction of arrival estimation" by Z.Chen , G.Gokeda, and Y.Yu



Unitary ESPRIT algorithm steps



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1. Received data: forward-backward averaging, then transform to real-valued.



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Unitary ESPRIT algorithm steps

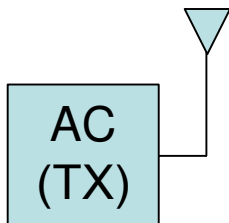
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4. From the eigenvalues of the real-valued matrix obtained in step 3, extract the DOA information.



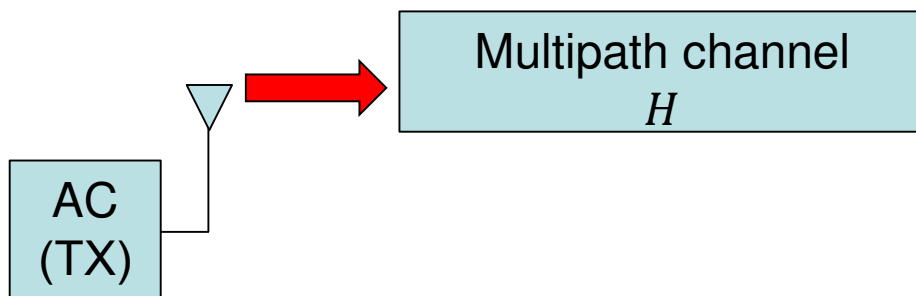
Channel model



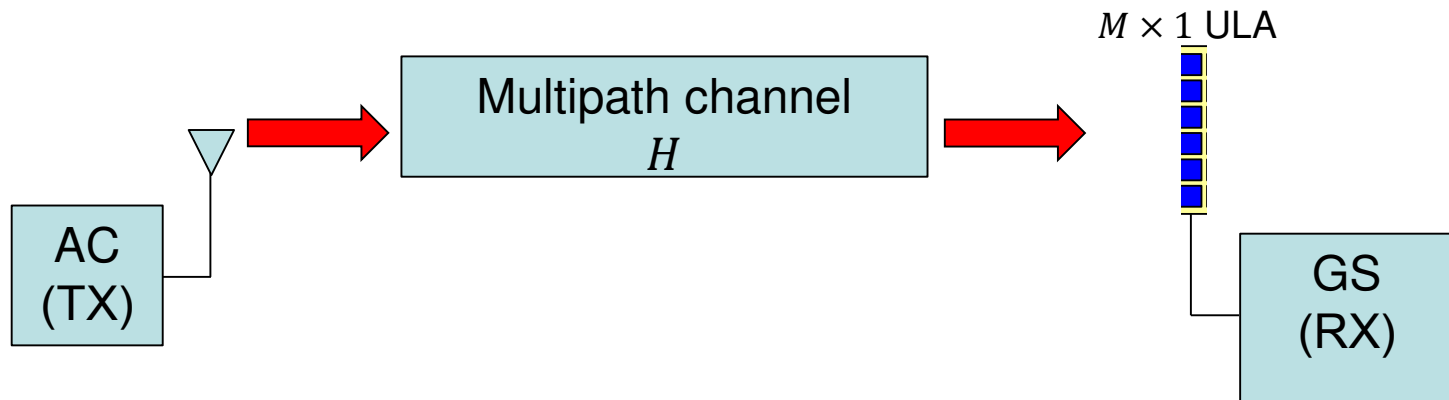
Channel model



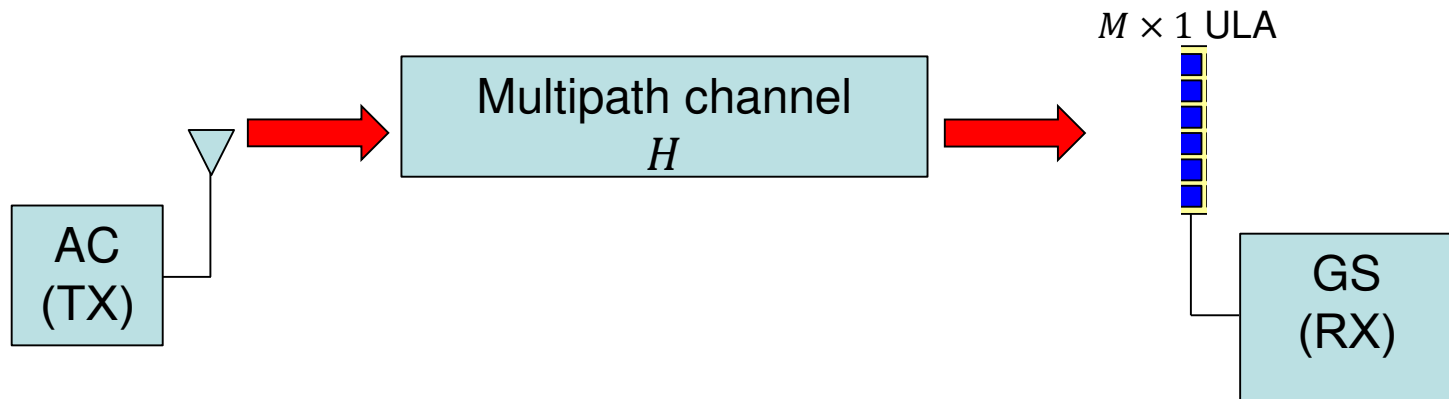
Channel model



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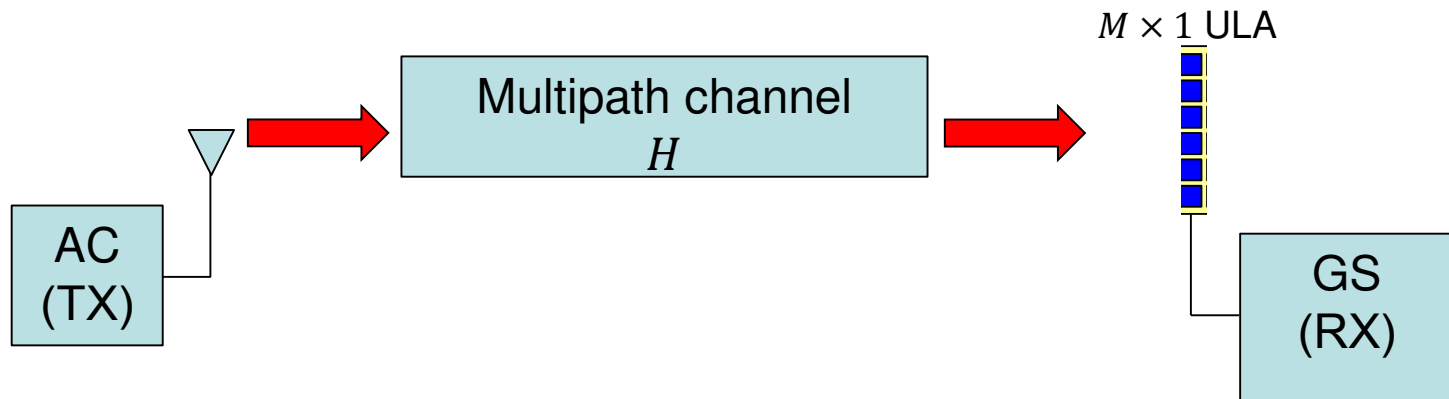
Channel model



$$h(t) = \sum_{l=1}^P \alpha_l(t) a_l g_l(t - \tau_l)$$



Channel model

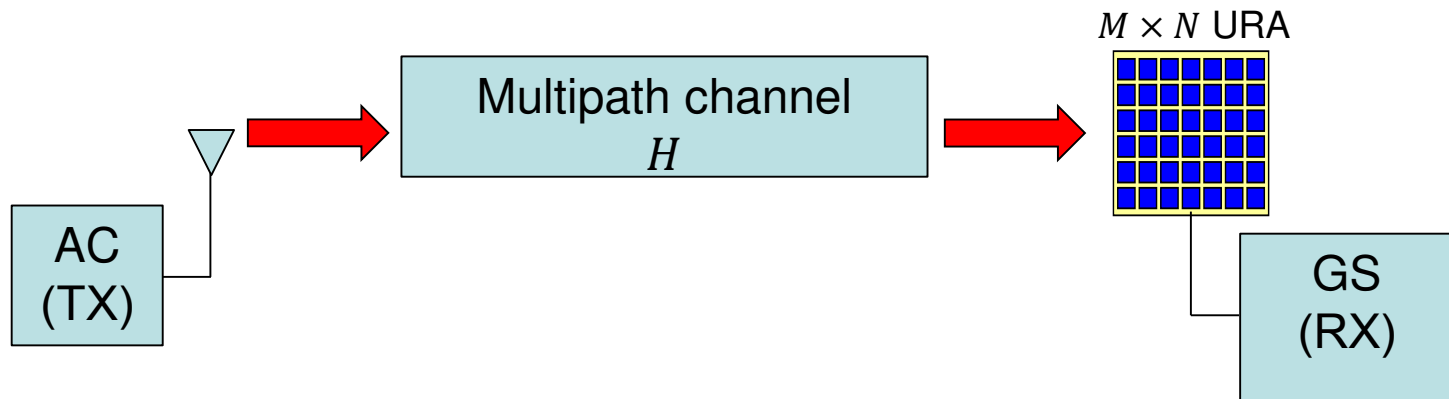


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$$a_l = a(v_l) = [1, e^{jv_l} \quad \dots \quad e^{j(N-1)v_l}]^T$$

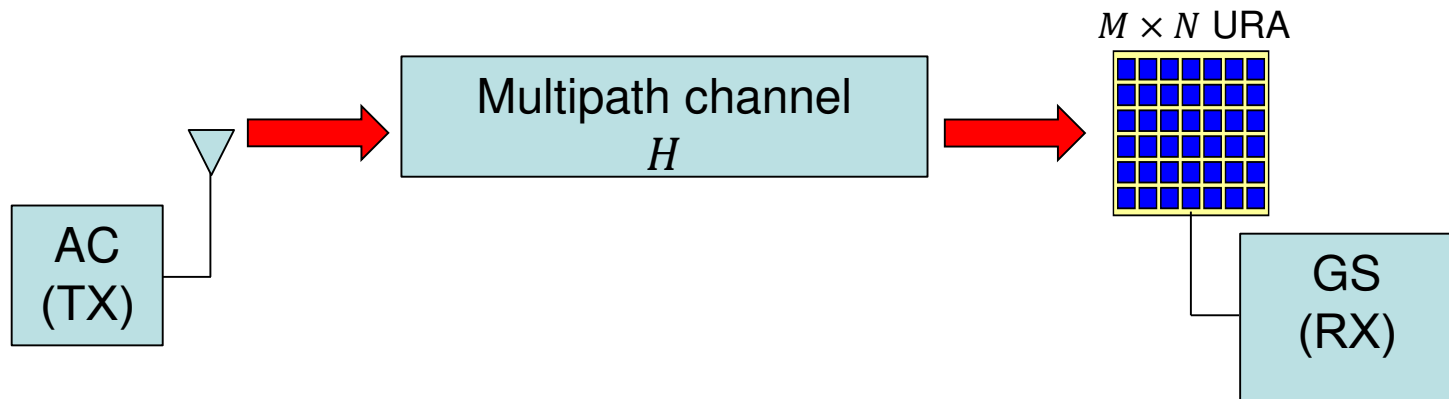


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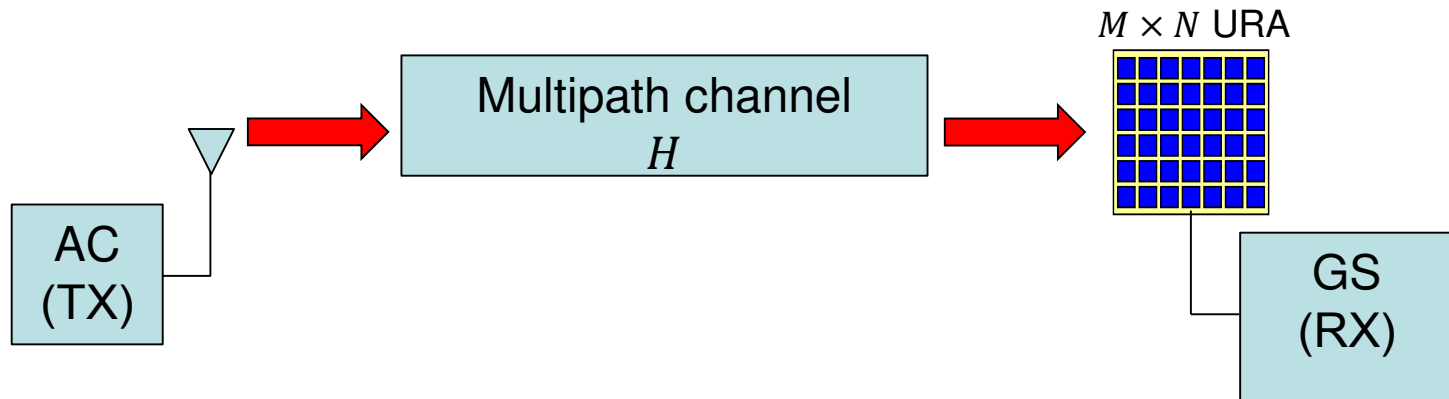


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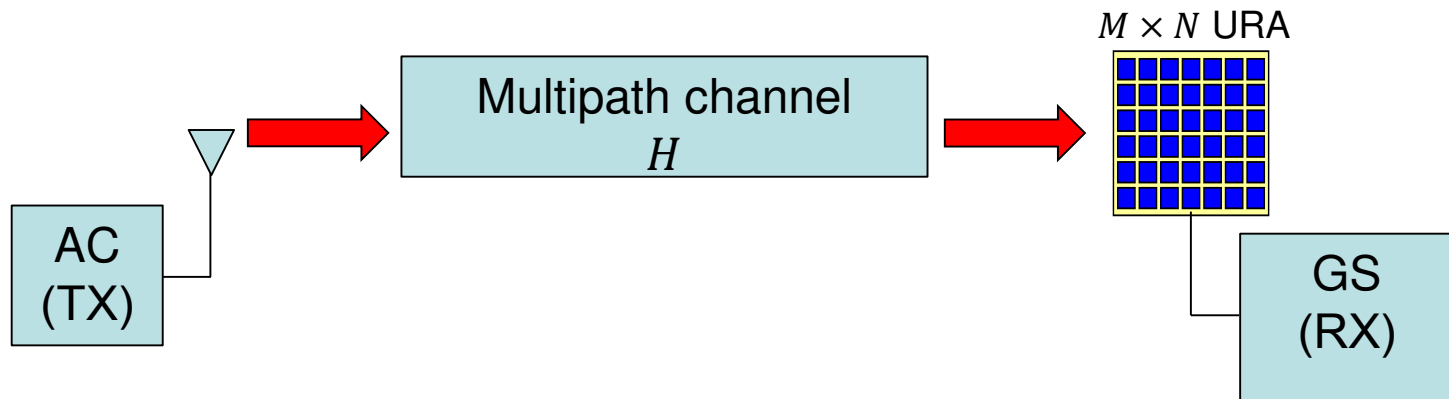
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$$\mu_l = \frac{2\pi}{\lambda} \cos \theta_l \quad v_l = \frac{2\pi}{\lambda} \sin \theta_l \cos \phi_l$$

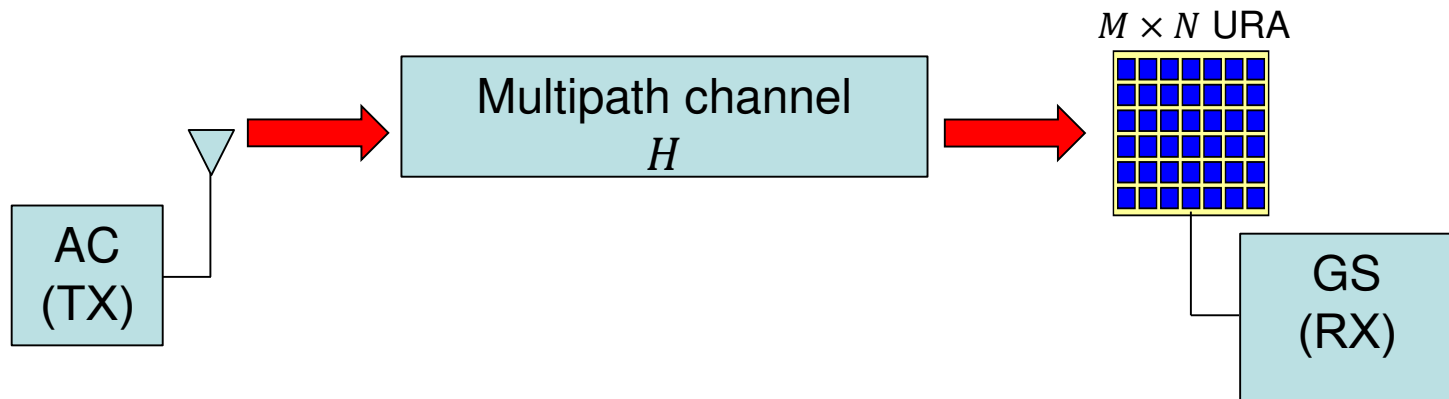


Channel model



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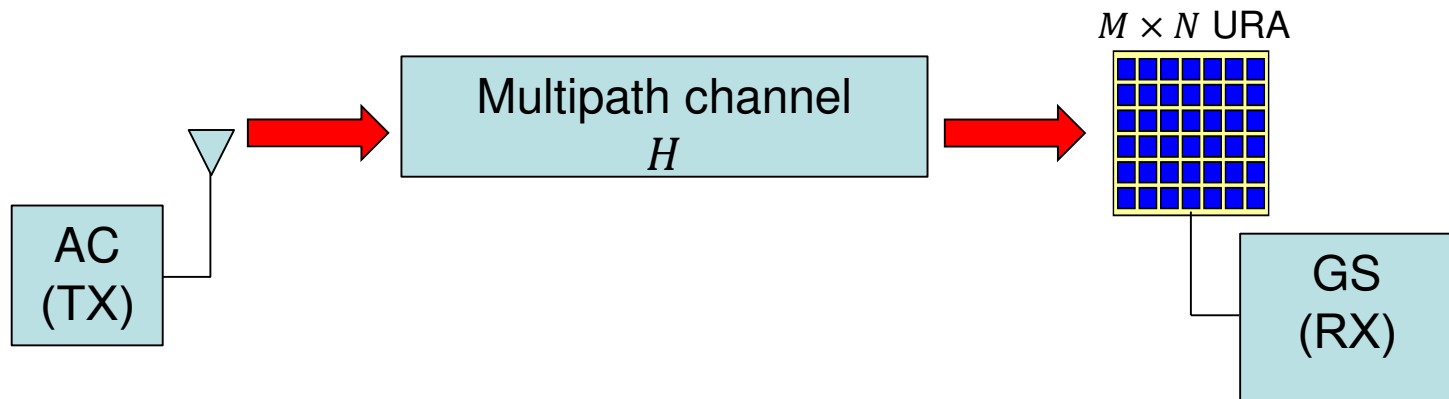


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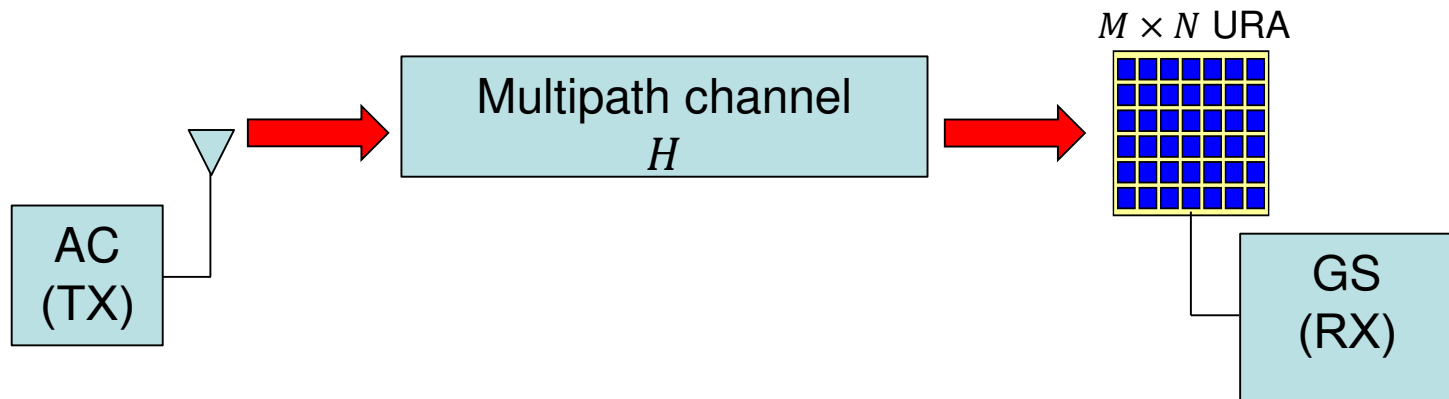


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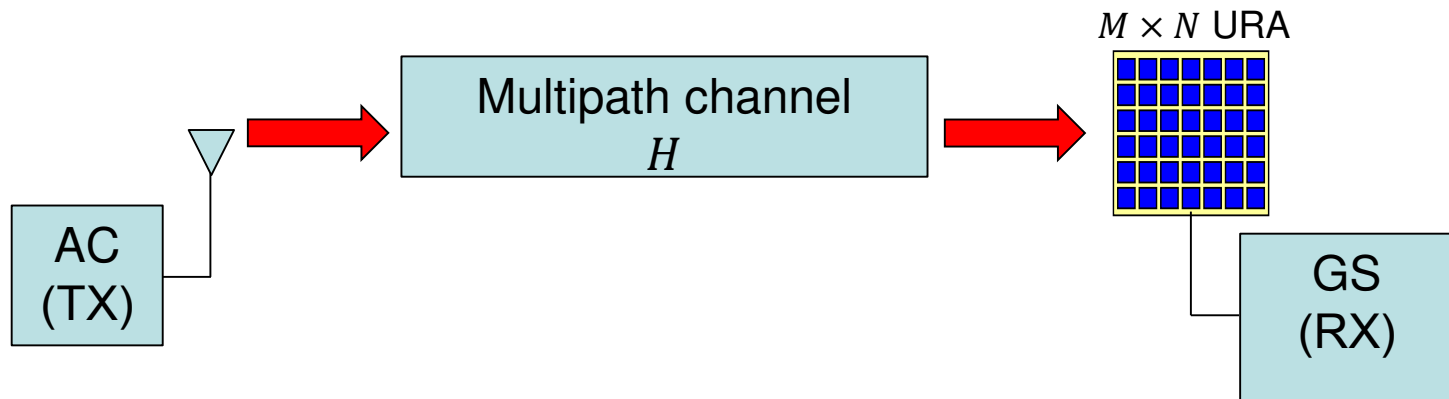
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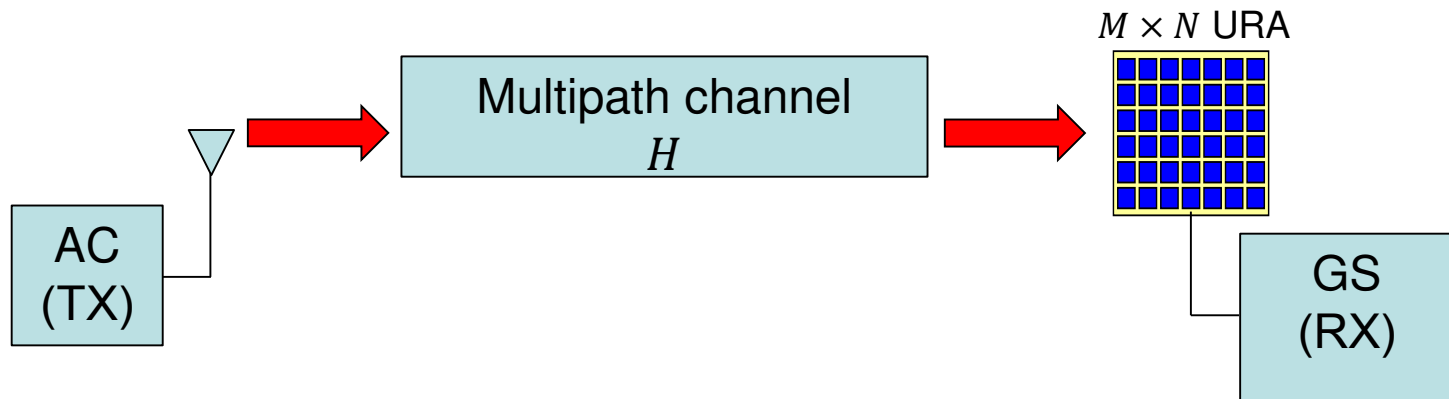
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D is the complex channel gain matrix (diagonal $P \times P$).

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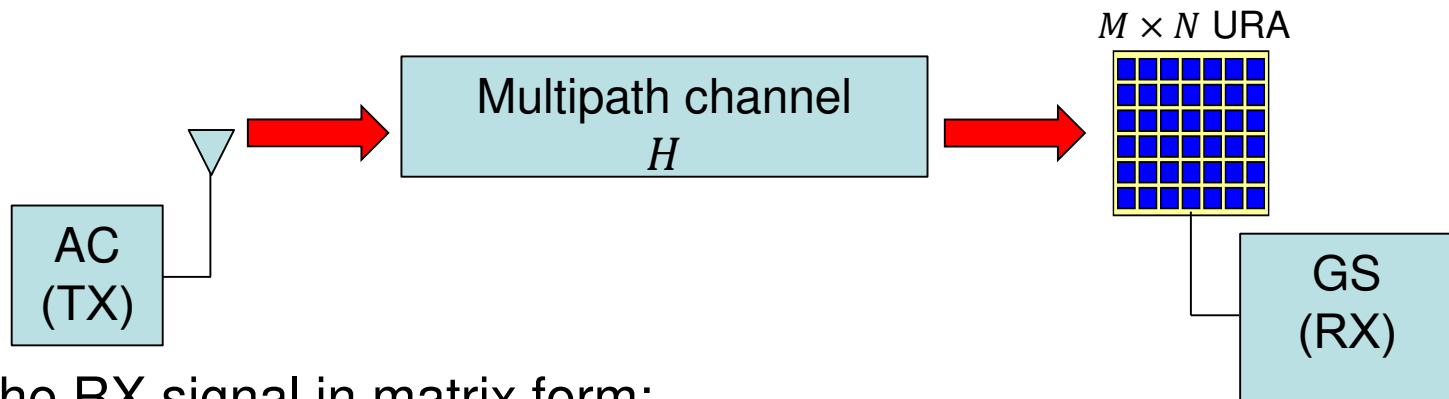
A is the array response matrix ($MN \times P$).

D is the complex channel gain matrix (diagonal $P \times P$).

G is the time-delay matrix ($P \times LV$).



Channel model

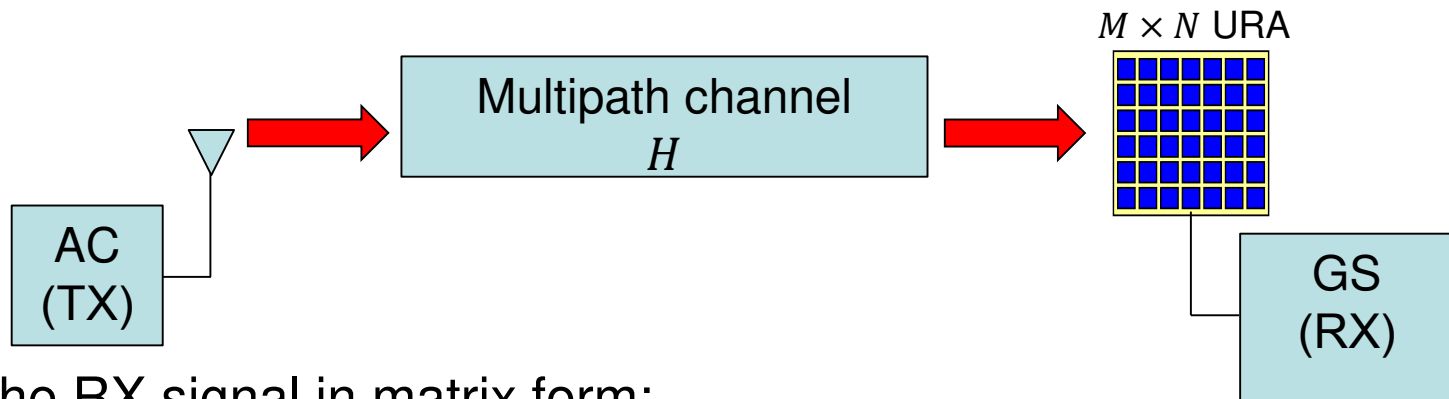


- The RX signal in matrix form:

$$Y = HS + W$$



Channel model

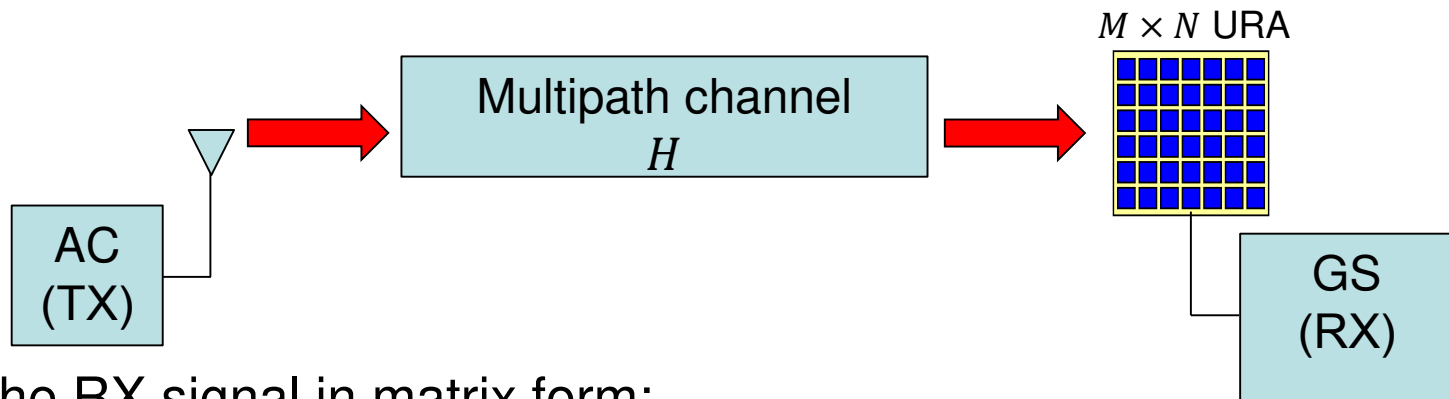


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- By extending to Q symbol periods, re-arranging the dimensions of the channel matrix H to be $MN \times VQ$, and taking the DFT, we have the uplink channel matrix :

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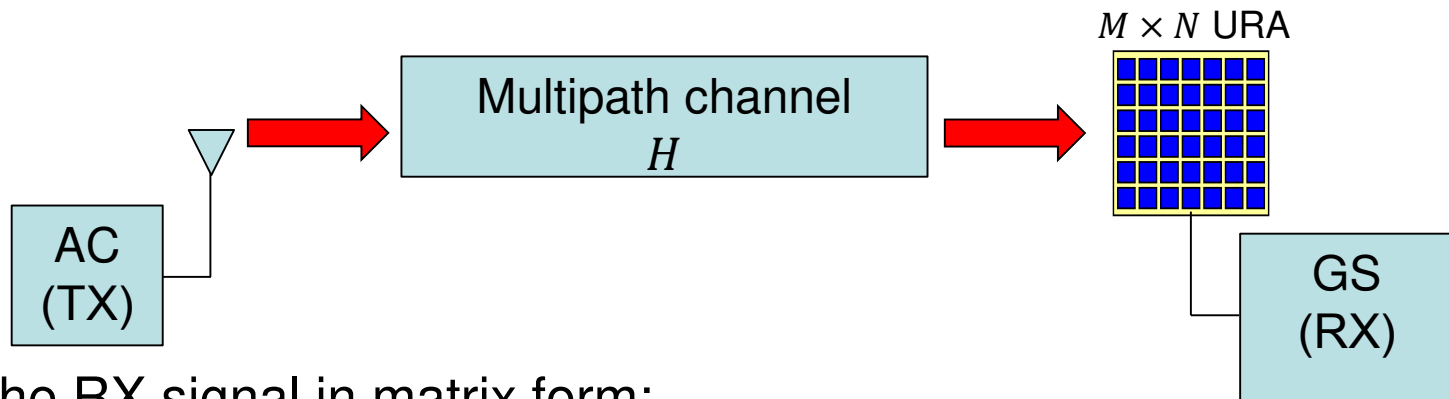
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F_{ψ} is the phase shift matrix ($P \times LB$, $B < V$)

MSE characterization



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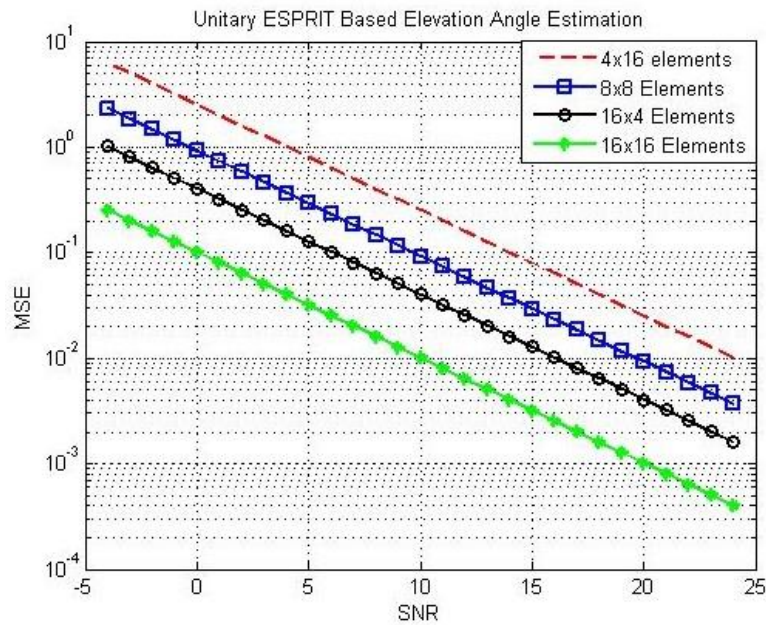
$$g_F = DFT(g) \in C^{LV \times 1}$$



Simulation results:



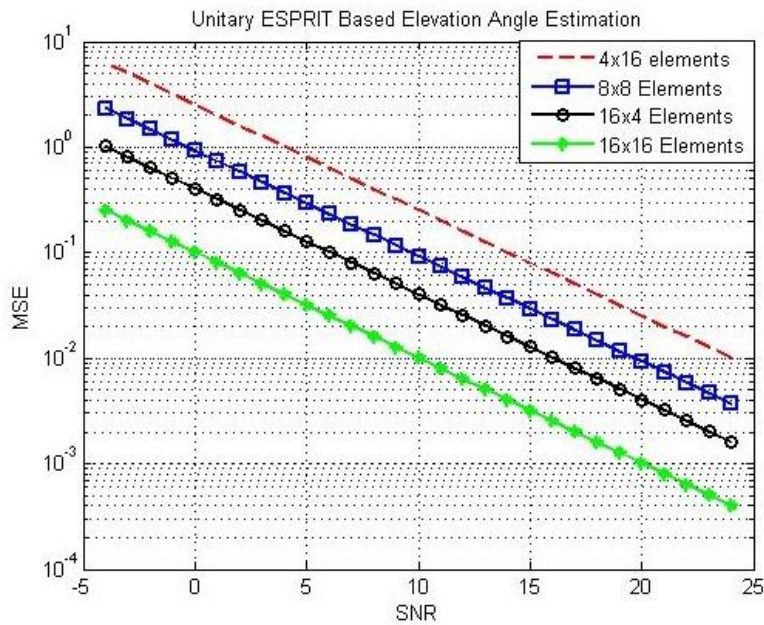
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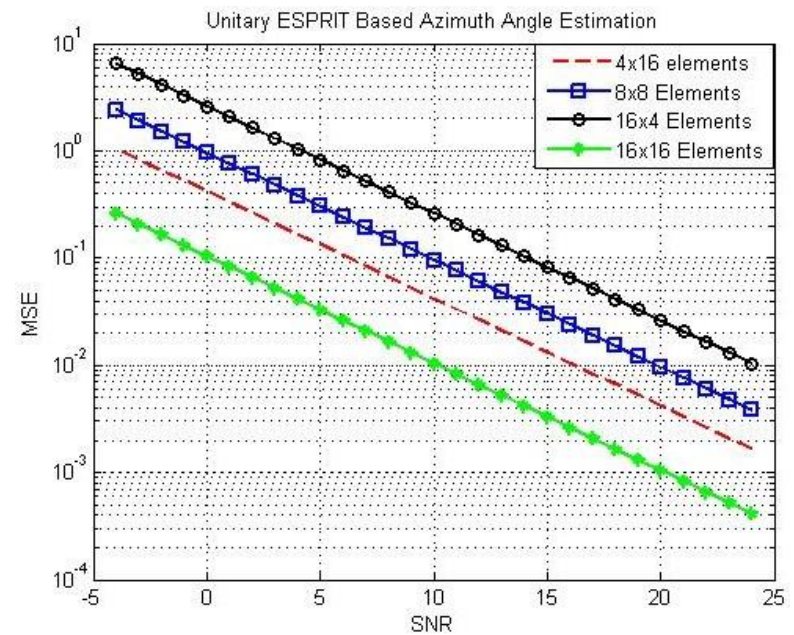
Elevation



Simulation results:



Elevation



Azimuth



Achievable rate analysis



Achievable rate analysis

- The achievable rate can be written as:

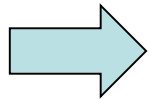
$$R = \sum_{l=1}^P \log_2 \left(1 + \frac{MN |\alpha_l|^2 |a_l^T f_l|^2 p_l}{\sigma^2} \right)$$



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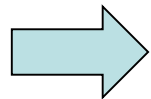
No DOA estimation error: $f_l = (a(v_l) \otimes a(\mu_l))^*$



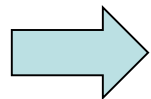
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DOA estimation error: $f_l = (a(v_l + \Delta v_l) \otimes a(\mu_l + \Delta \mu_l))^*$



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$$[x]^+ = \max(x, 0) \quad \text{and} \quad \gamma_l = \frac{MN |\alpha_l|^2}{\sigma^2}$$



Power allocation

- The optimal power allocation strategy that maximizes R :

$$\max R \quad \text{subject to} \quad \sum_{l=1}^P p_l \leq p_{tot}$$

- Thus, the expected TX power for the l^{th} path is

$$E[p_l] = \left[\eta - \frac{1}{\gamma_l} \left(1 + \frac{M^2-1}{12} E[(\Delta\mu_l)^2] \right) \left(1 + \frac{N^2-1}{12} E[(\Delta v_l)^2] \right) \right]^+$$

$$[x]^+ = \max(x, 0) \quad \text{and} \quad \gamma_l = \frac{MN |\alpha_l|^2}{\sigma^2}$$

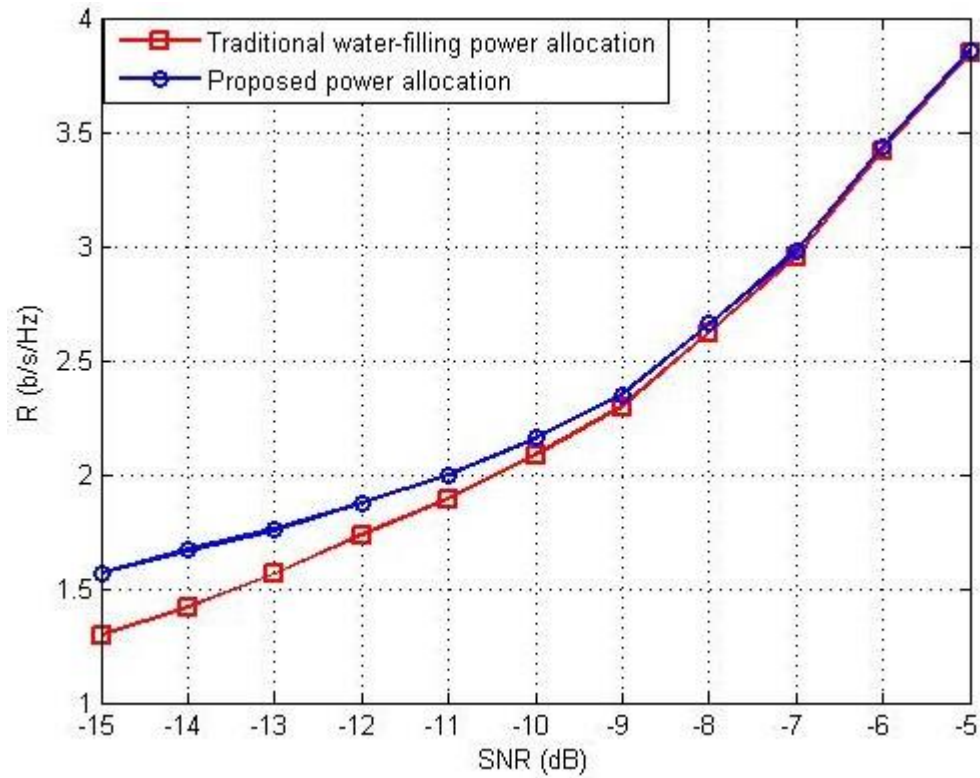
- If $\Delta v_l = 0$ and $\Delta\mu_l = 0$, the power allocation becomes the traditional water-filling solution.



Results



Results



Future work



Future work

- Extend the results to MU-MIMO systems.



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- Joint angle-delay estimation (JADE) using tensor algebra.



Future work

- Extend the results to MU-MIMO systems.
- Joint angle-delay estimation (JADE) using tensor algebra.
- JADE for multi-cell MIMO systems.



Questions?

