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Dual-Band Transmitarray with Low Scan Loss for Satcom Applications

Kien T. Pham, Guang Liu, David González Ovejero, and Ronan Sauleau

Abstract— This paper presents the experimental validation of independent and wide beam scanning with a dual-band transmitarray antenna (TA) in Satcom up- and down-links at Ka-band. The TA consists of two sub-arrays, one operates in the down-link with central frequency at 19.5 GHz, while the other one operates in the up-link centered at 29 GHz. Both sub-arrays share a common radiating aperture to obtain compact configuration. The TA layout is made of 1-bit unit-cells and its design relies on the bifocal technique to extend the beam scanning capability. The proposed bifocal prototype includes 1500 up-link unit-cells in 30×50 matrix and 1581 down-link unit-cells arranged in 31×51 rectangular lattice. The 1D scanning is validated by displacing the feed horn along one direction. We show that the TA beam can be scanned in a $\pm 40^\circ$ and $\pm 30^\circ$ independently in each band while keeping a very low scan loss (< 2 dB).

Index Terms— Bifocal, Satcom, dual-band, dual-polarization.

I. INTRODUCTION

Transmitarray antennas (TAs) are a mature alternative technology with some key advantages with respect to more standard solutions based on reflectors, phased arrays and reflectarrays. As compared to reflectarray antennas (RAs), which work in reflection mode, TAs operate in transmission mode and do not suffer from blockage from the feeder. They can be also easily integrated on moving platforms, for example, high speed trains, vehicles, drones, etc., without significant impact on their aerodynamic properties. In particular, TAs are considered as very promising candidates for Satcom on the move (SOTM) and 5G applications. The frequency bands allocated in Europe for SOTM applications (both civil and military) are 27.5 GHz – 31 GHz and 17.7 GHz – 21.2 GHz for the up and down links, respectively [1]. The advantage of covering both bands with the same aperture is, hence, obvious.

Recent studies on TAs have demonstrated their performance at various frequency bands, e.g. [2]-[5], including also dual-polarization and dual-band capabilities, e.g. [6], [7]. Metal-only prototypes have been also introduced as lower cost solutions compared to their dielectric-based counterparts [8], [9]. Reconfigurable TAs (RTAs) with electronically steerable beams are also of strong interest owing to their 2D scanning capabilities over a wide angular field of view, typically beyond $\pm 50^\circ$ [10], [11]. However, RTAs or reconfigurable RAs require a significant number of solid state components to control their phase distribution on the radiating aperture, and their unit-cells architectures may become quite complex to route DC biasing lines [10]-[14]. Purely passive TAs can also be used to steer the beam in any arbitrary direction by mechanically displacing a feed horn in the TA focal plane [3] or by switching focal arrays [15]. The later architecture exhibits a limited field of view, while the feed in [3] is displaced over longer distances to reach a wider maximum scan angle, but at the expense of a quite high scan loss (around 5 dB at $\pm 30^\circ$) due

to the higher spill-over radiation and phase aberration [3]. Recently, a 1D TA in parallel plate waveguide provided $\pm 42^\circ$ beam-scanning in the H-plane by switching the focal source. In this configuration, the number of beams equals the number of ports [16]. Therefore, significant efforts are being devoted to obtaining wide angle scanning and low scan loss simultaneously.

The design procedure of RAs and TAs is similar, except for operation in reflection or transmission. Hence, we provide next an overview on RA and TA structures with an improved scan range. One possibility consists in introducing a bifocal architecture to expand the scanning range of RAs [17]-[18] and TAs [19]. The designs in [17]-[18] obtain the phase distribution on the RA aperture as the average phase of two foci associated to two beam directions; optimization algorithms are also applied to overcome the limitations of unifocal and bifocal techniques. On the other hand, the weighted average approach is used in [19]. This technique takes into account a Gaussian weight function on the aperture in order to obtain low aberration in both phase and illumination level. The scanning loss is reported to be less than 1-dB for a scanning range of $\pm 30^\circ$ in [18] and around 2.8 dB for a 0° to 50° scanning in [19]. A recent dual-band TA in circular polarization with wide beam scanning (up to 50° with scan loss below 3.6 dB) is reported in [7] for Ka-band Satcom. The TA structure consists of 6 substrates and 7 layers.

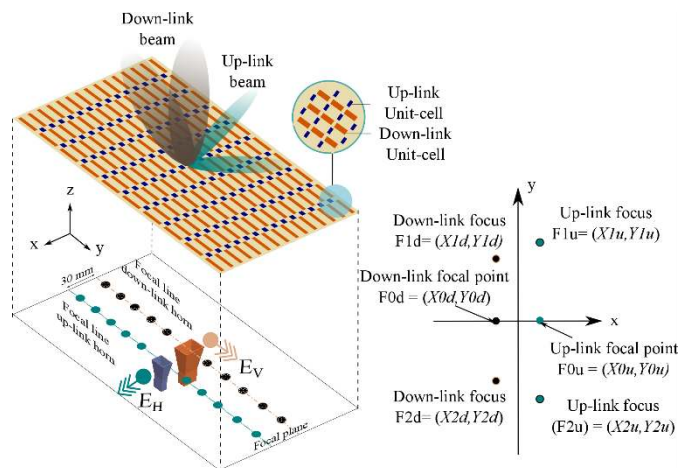


Fig. 1. Architecture of dual-band dual-linearly polarized bifocal TA with independent beam scanning, and its four focal points (right figure). The radiating aperture contains two independent sub-arrays operating in the down link (in orange) and in the up-link (in blue). Green and dark dots illustrate the positions of the up- and down-link horns displaced in the focal plane to steer the beam.

The main objective of this paper is to present an experimental demonstration on scanning loss reduction for dual-band TA, as alternative to the work reported in [6], and to extend scanning range in comparison with [18]-[20] with the additional freedom of tilting the beam in either up- or down-link for arbitrary directions. The simplified design procedure presented in this work for dual-band operation is an advantage with respect to [20] for light-weight TA.

The antenna architecture and main design rules are described in Section II. The fabricated prototypes and measurement results are presented in Section III to validate the proposed concept. Conclusions are drawn in Section IV.

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II. BIFOCAL TRANSMITARRAY IN DUAL-BAND OPERATION

The purpose of the proposed TA configuration is to provide independently two arbitrary beams pointing to any direction while each beam operates in either up- or down-link. These beams are able to operate simultaneously or alternatively. The detailed architecture of the proposed antenna is illustrated in Fig. 1. This schematic includes a dual-band TA, which layout is calculated to provide two independent linearly-polarized (LP) pencil beams. The TA is illuminated with two separate feeding sources (the pyramidal horns shown in Fig. 1), which are displaced individually in the focal plane to steer the beams individually in each band.

The concept used here for dual-band operation is based on the interleaving technique already introduced by the authors in [6]. This technique consists in interleaving two independent LP TA sub-arrays in the same radiating aperture. Each sub-array operates in orthogonal polarization and in a different frequency band. The use of LP unit-cells strongly-decoupled in the down- and up-link leads to a very simple design procedure, as described in [6]: both down- and up-link sub-transmitarrays are designed individually and their layout are superimposed to form the dual-band radiating aperture. We introduce here an improved design by combining the interleaving technique [6] with the bifocal one [17], [18] to further improve the TA beam scanning performance.

More precisely, the up-link and down-link arrays are made of 30-by-50 and 31-by-51 elements arranged in a rectangular lattice, as illustrated in Fig. 1. The unit-cells are square with periodicity of 6 mm to be compatible with array interleaving [6]. The unit-cells include two narrow radiating patches connected by a via-hole structure and separated by a ground. These three metal layers are printed on two identical 0.762-mm thick substrates (Roger Duroid RT6002). The detailed dimensions, characteristics of the up- and down-link unit-cells are reported in Section III in [6] and not mentioned here for the sake of brevity.

In contrast to [6], the TA is extended along y -axis (corresponding to E-plane in the up-link and H-plane in the down-link) to reduce spill-over loss for extreme tilt angles. The focal distance is set to 110 mm to maximize the antenna gain. The 10-dBi gain standard horns, similar to the ones in [6], are used to illuminate the TA aperture; they are offset by +15 mm and -15 mm along x -axis for up-link and down-link respectively. Such an inter-horn spacing (30 mm) has been selected to ease their accommodation in the focal plane.

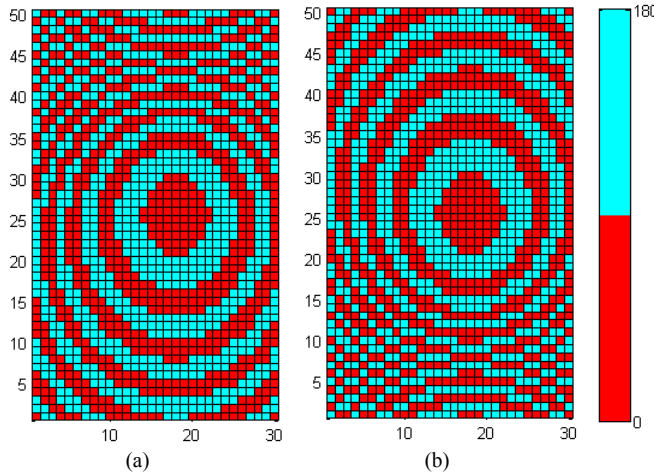


Fig. 2. Computed phase distribution (in deg.) on the TA aperture at 29 GHz for up-link horn located at (a) 63.5 mm and (b) -63.5 mm along y -axis, in order to radiate at -30° and $+30^\circ$ in E-plane, respectively.

The bifocal technique has been implemented here following the design procedure reported in [19], [20], in order to design the two desired interleaved bifocal sub-arrays in the up- and down links. The technique implemented here is modified to apply this dual-band TA (see Eq. (1) and Eq. (2) below). The initial parameters are taken from [6] for $D_{Au} = 180$ mm, $F_u = 110$ mm and $\tau_u = 0.6$ for edge illumination of -12 dB. The maximum gain is obtained at broadside or $\alpha_{0,u}(a_0=0)=0^\circ$. The two focal points $F1u$ and $F2u$ of the up-link sub-array are located along its own focal line (Fig. 1), parallel to y -axis, symmetrically at $y = -63.5$ mm and $y = +63.5$ mm; their coordinates are thus the following: $F1u = (15$ mm, 63.5 mm) and $F2u = (15$ mm, -63.5 mm); their positions, defined in Fig. 1, lead to two beams pointing at $\pm 30^\circ$. The phase and amplitude distributions on the sub-array radiating aperture are plotted in Figs. 2 and 3, respectively, for each beam. As described in [17], these phase layouts have been averaged and combined to produce the final TA layout at 29 GHz (Fig. 4a), with the corresponding parameters $y_{i,u} = 63.5$ mm and $\alpha_{i,u} = 30^\circ$ [17].

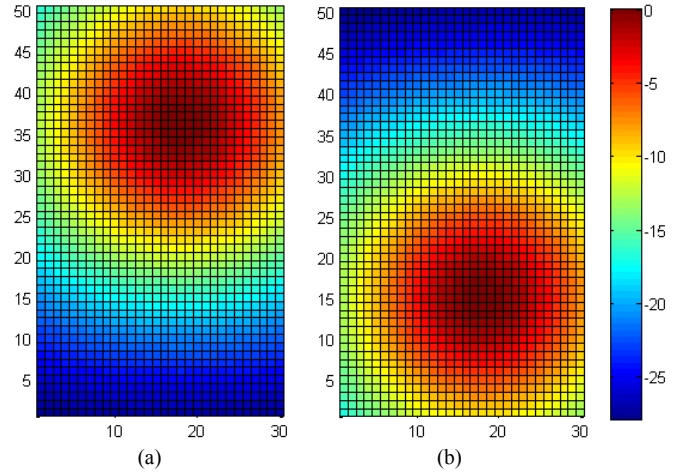


Fig. 3. Normalized illumination level (in dB) on the TA aperture at 29 GHz for up-link horn located at (a) 63.5 mm and (b) -63.5 mm along y -axis, in order to radiate at -30° and $+30^\circ$ in E-plane respectively.

Here, the phase is optimized by averaging the phase aberration due to feed horn displacement. The bifocal phase distribution is calculated as follows [19]-[20]

$$\varphi_{TA}^{bif} = \frac{A_1 \varphi_1^{uif} + A_2 \varphi_2^{uif}}{A_1 + A_2}, \quad (1)$$

where A_1 and A_2 are the illumination levels of the incident wave and are used as weight coefficients for the corresponding unifocal phase layouts φ_1^{uif} and φ_2^{uif} .

In turn, the unifocal phase layouts above are computed as follows

$$\varphi_i^{uif} = k_0 \left(y \sin \alpha_i - \sqrt{(x - x_0^{u/d})^2 + (y - y_i^{u/d})^2 + F^2} \right) \quad (2)$$

where u/d stands for uplink/downlink array respectively

The same procedure has been applied in the down link, assuming that both focal points are located at $F1d = (-15$ mm, 51.5 mm) and $F2d = (-15$ mm, -51.5 mm) and generate two beams pointing at $\pm 25^\circ$ in elevation. The corresponding parameters of [17] are $y_{i,d} = 51.5$ mm and $\alpha_{i,d} = 25^\circ$. The final layout at 19.5 GHz is provided in Fig. 4b.

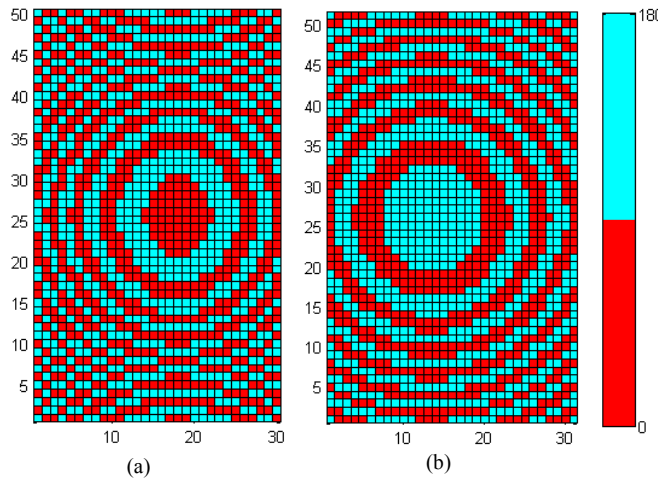


Fig. 4. Bifocal layouts of the dual-band TA at (a) 29 GHz and (b) 19.5 GHz respectively.

The parameters used for the design proposed here are summarized in Table I.

TABLE I
MAIN DESIGN PARAMETERS USING THE PARAMETERS DEFINED IN [19],[20]

Parameters	Down-link @ 19.5 GHz	Up-link @ 29 GHz
D_A	186 mm	180 mm
y_1/y_2	-51.5mm / 51.5mm	-63.5mm / 63.5mm
α_1/α_2	$25^\circ / -25^\circ$	$30^\circ / -30^\circ$

One can notice that the unifocal phase layouts for the up- and downlink are computed separately since they are independent and the feed-horns positions for the up- and down-links are also different ($x_0^u = +15\text{mm}$ and $x_0^d = -15\text{mm}$), as shown in Fig. 1.

III. EXPERIMENTAL RESULTS

To better demonstrate the enhanced performance of the bifocal prototype, a unifocal dual-band TA has been also designed, with the same aperture size, unit-cell type and F/D ratio as the bifocal TA described in Section II. Fig. 5a and Fig. 5b show the down- and up-link layouts computed at 19.5 GHz and 29 GHz, respectively.

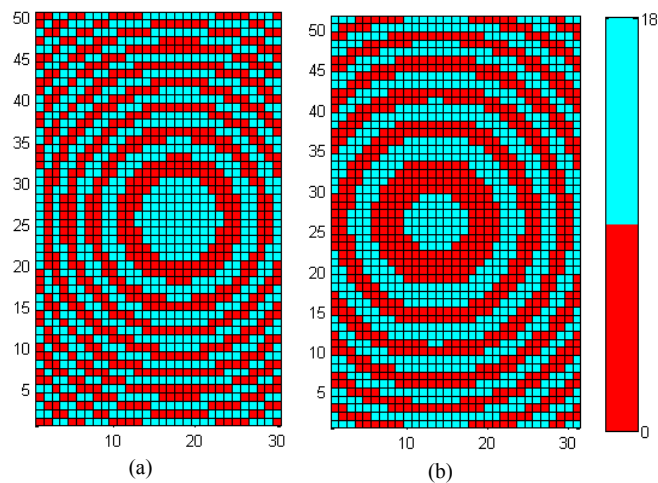


Fig. 5. Unifocal layouts of dual-band TA computed at (a) 29 GHz and (b) 19.5 GHz respectively. The unit-cell is the same as for the bifocal TA.

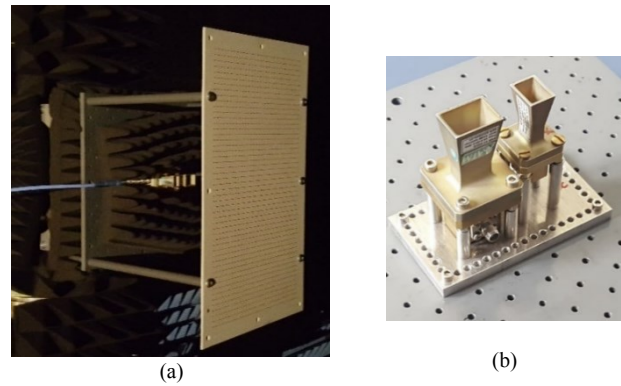


Fig. 6. Bifocal dual-band TA antenna mounted in IETR anechoic chamber. (a) TA panel. (b) Dual-feed horn focal array.

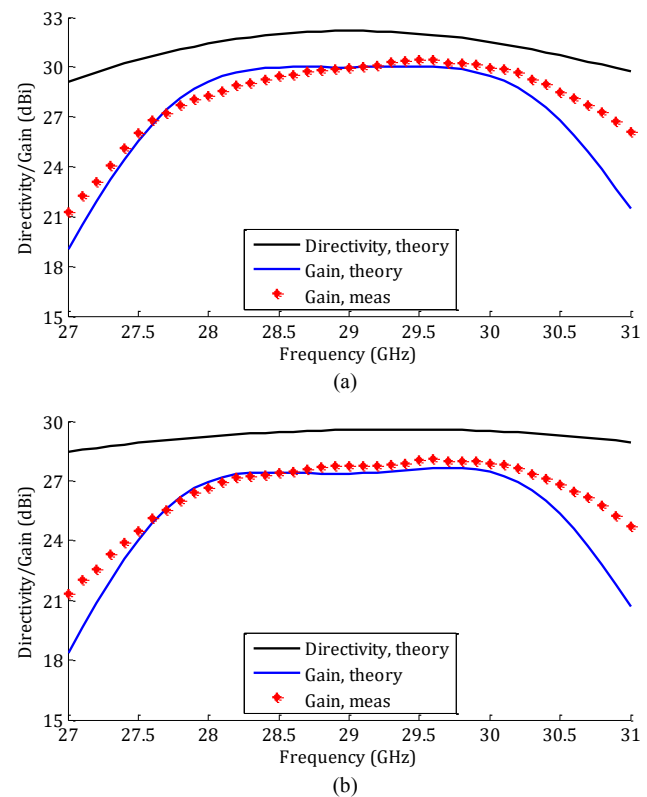


Fig. 7. Directivity and gain as a function of frequency: (a) unifocal and (b) bifocal TAs in up-link.

Both prototypes have been fabricated and measured in the millimeter-wave far-field anechoic chamber at IETR. The bifocal prototype mounted on the receiving mast is shown in Fig. 6a. They have been measured individually, using in both cases exactly the same feeding system with sliding horns (Fig. 6b). In the following results, as the TA prototypes are too large to be modeled using commercial electromagnetic solvers (like Ansys HFSS or CST) in affordable simulation times, all theoretical data have been obtained with our in-house CAD tool, previously validated successfully in a number of publications, e.g. [4], [11], [12].

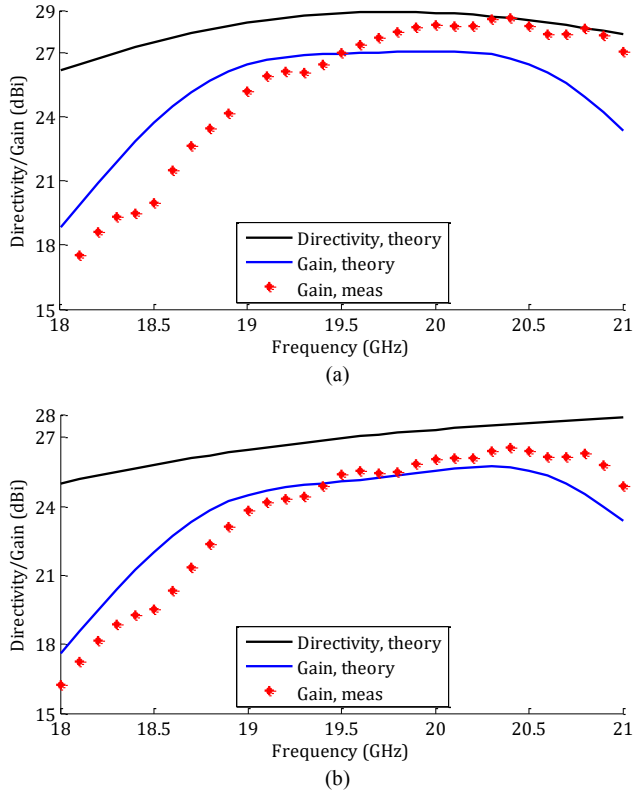


Fig. 8. Directivity and gain as a function of frequency: (a) unifocal and (b) bifocal TAs in down-link.

A. Frequency Response and Patterns at Broadside

Fig. 7 and Fig. 8 show the directivity and gain of the unifocal and bifocal TAs in up- and down-links, respectively. A good agreement between theoretical and measured gain values is observed in both bands.

In the up-link band, the measured -1-dB and -3-dB bandwidth (BW) of the bifocal prototype equal 7.6 % (28.2 GHz - 30.4 GHz) and 11.7% (27.6 GHz - 31 GHz), respectively. In the unifocal case, the -1 and -3-dB BWs are slightly smaller, namely, 6% (28.6 GHz - 30.3 GHz) and 10% (27.8 GHz - 30.7 GHz), respectively. Similar conclusions can be drawn for the down link: the -1-dB and -3-dB measured gain BWs of unifocal TA span from 19.7 GHz to 20.9 GHz and 19.1 GHz to 21.2 GHz (10.8% around 19.5 GHz) respectively, whereas the -3-dB bandwidth of the bifocal TA spans between 18.9 GHz and 21.2 GHz (11.8%).

Due to the extension of the array dimension along the y-axis, the gain values at boresight of the up- and down-link unifocal TAs presented here (30 dBi at 29 GHz and 27 dBi at 19.5 GHz, respectively) are larger than the gains reported in [6] by about 1.2 dB.

The normalized calculated radiation patterns are almost superimposed with the measured ones. For brevity purposes, we only provide the results in the scan plane at the center frequency in each case (H-plane at 29 GHz in Fig. 9a, and E-plane at 19.5 GHz in Fig. 9b). In both cases, the measured side-lobe level (SLL) is in very good agreement with the simulated one.

The simulated results have been obtained using array theory, e.g. [11]; in particular, this simplified model uses the unit-cell characteristics computed in a purely periodic environment (Floquet mode analysis) as input data; moreover, it does not account for

truncation and illumination effects. Despite these approximations, the agreement between the simulated and measured gains is very satisfactory (Fig. 7 and Fig. 8).

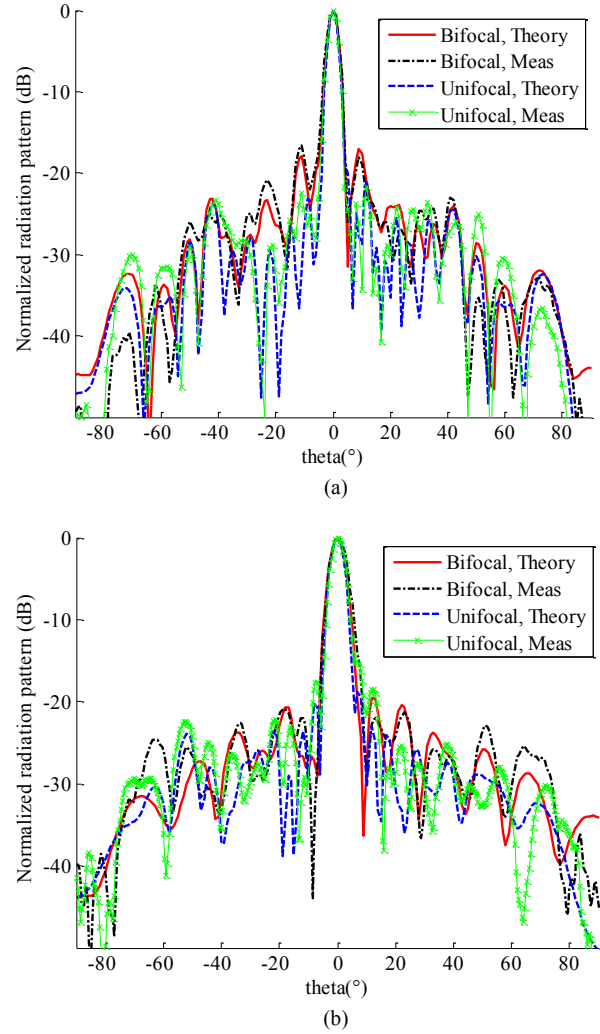


Fig. 9. Computed and measured radiation patterns (a) in H-plane at 29 GHz and (b) in E-plane at 19.5 GHz.

B. Performance in Scanning

The performance in scanning of both prototypes has been measured by translating the feed horn base along focal lines in either down- or up-link, as schematized in Fig. 1. In practice, two successive feed positions are separated by 10 mm, and they vary up to 80 mm from the center position (Fig. 6b) in both directions to check beam symmetry.

The collection of beam patterns measured for various horn positions is shown in Fig. 10 (up-link) and Fig. 11 (down-link) for the bifocal prototype. In all figures, the tilted beams are normalized to the maximum gain value measured at boresight. At 29.5 GHz, when the feed horn is moved from -70mm to +70mm, the main beam is tilted from -32° to 33° with a scan loss lower than 2 dB. The total scan range reaches 60° for a scan loss better than 1 dB (Fig. 10b). The SLL is less than -11 dB for all beams in this range (Fig. 10a). Theoretical calculations are in very good accordance with measurement results, except for some beams at wide angle (see Fig. 10a); this is possibly due to the horn fixture, effect of oblique incidence and the edge

diffraction that are not taken into account when computing the radiation patterns.

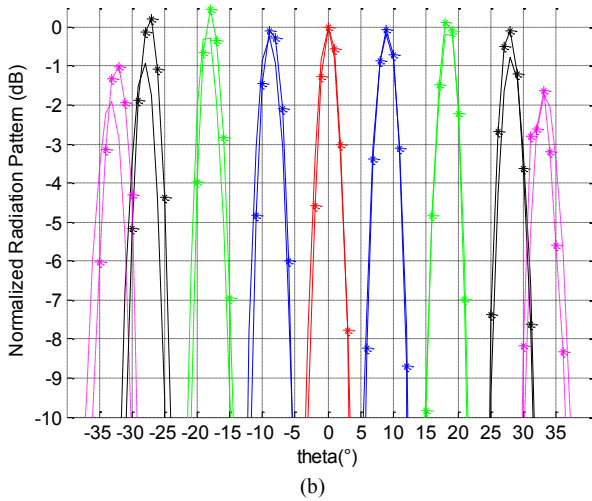
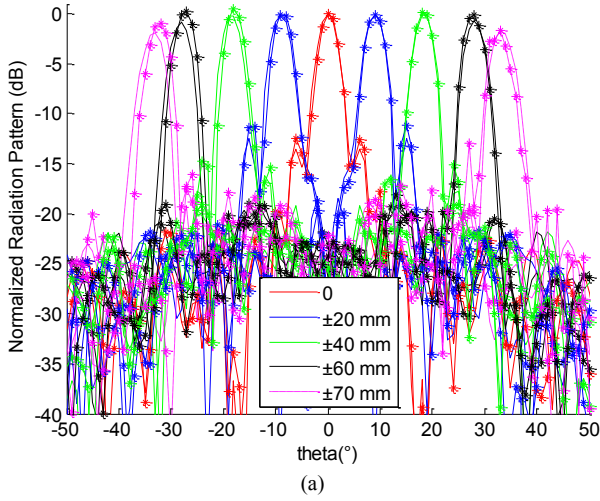


Fig. 10. Computed and measured radiation patterns of bifocal TA, for different beam pointing directions, at 29 GHz in E-plane. (a) Results obtained for a wide range of elevation angle, (b) zoom close to the main beams. Curves with markers correspond to experimental results. All curves are normalized to the maximum gain at boresight.

Similar results have been obtained in the down link at 19.5 GHz as shown in Figs. 11a and 11b. As the unit-cell is electrically smaller in this band, the scan range is slightly improved and reaches 80° (horn displacement of 80 mm) with a maximum gain drop of only 2 dB at $\pm 40^\circ$ (see Fig. 11b). The scan loss remains smaller than 1 dB loss for a field of view of $\pm 30^\circ$. Although not reported for brevity purposes, a very good agreement between measured and simulated patterns has been obtained for all beam positions across the 3dB bandwidth.

As shown in Fig. 4b, the scanning performance obtained by translating the feed-horn in the bifocal down-link TA is better than the scanning obtained by the methods described in [6] (Section IV.C, Fig.19).

The unifocal dual-band TA has been also fully characterized for various horn positions, using the same experimental setup. As expected, our results indicate that the performance in scanning suffers from much larger scan loss (Fig. 12). A detailed analysis shows that the scan loss reaches 3.7-dB at $\pm 18^\circ$, and that it drops sharply beyond

(5-dB at $\pm 25^\circ$), thereby confirming the considerable improvement in scanning of the bifocal approach.

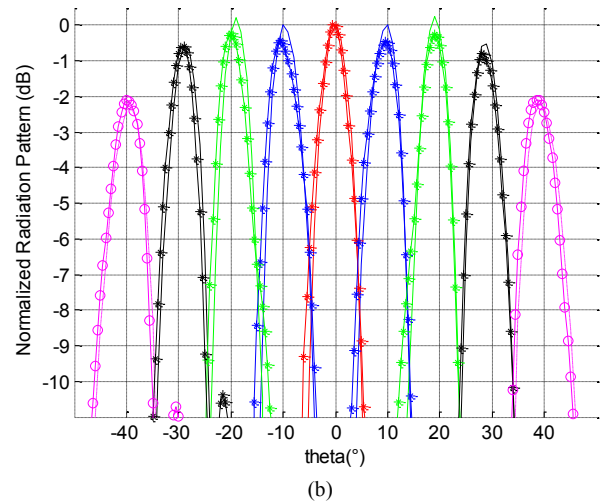
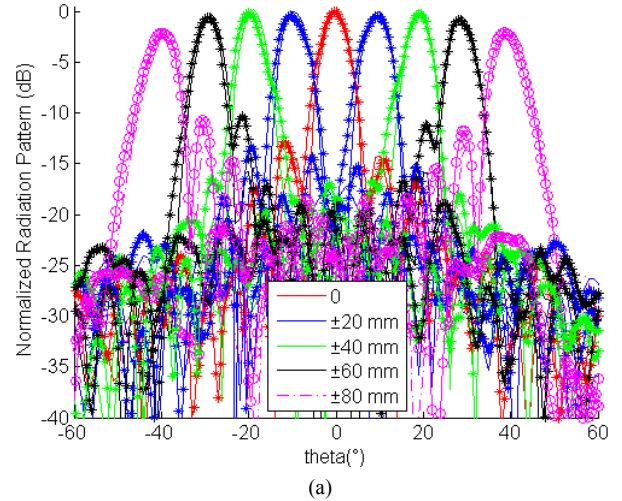


Fig. 11. Computed and measured radiation patterns of bifocal TA, for different beam pointing directions, at 19.5 GHz in H-plane. (a) Results obtained for a wide range of elevation angle, (b) zoom close to the main beams. Curves with markers correspond to experimental results. All curves are normalized to the maximum gain at boresight.

A summary of recent results obtained at Ka-band with beam steerable transmitarray and reflectarray antennas is provided in Table II. It is obvious that this work provides a very wide field of view for both up- and down-link Ka-band with independent radiations.

TABLE II
PERFORMANCE IN SCANNING FOR VARIOUS BIFOCAL REFLECTARRAY AND TRANSMITARRAY PROTOTYPES AT KA-BAND.

Ref. type	Frequency (GHz)	Scan. Range (deg.)	Loss (dB)
This work TA	29	65° (-32°-35°)	2.0
	19.5	80° ($\pm 40^\circ$)	2.0
[7], TA	30	50° (0°-50°)	3.3
	20	50° (0°-50°)	3.6
[19], TA	30	50° (0°-50°)	2.8
[20], TA	30	40.4° (16.1°-56.5°)	2.4
[18], RA	32	60° ($\pm 30^\circ$)	0.75

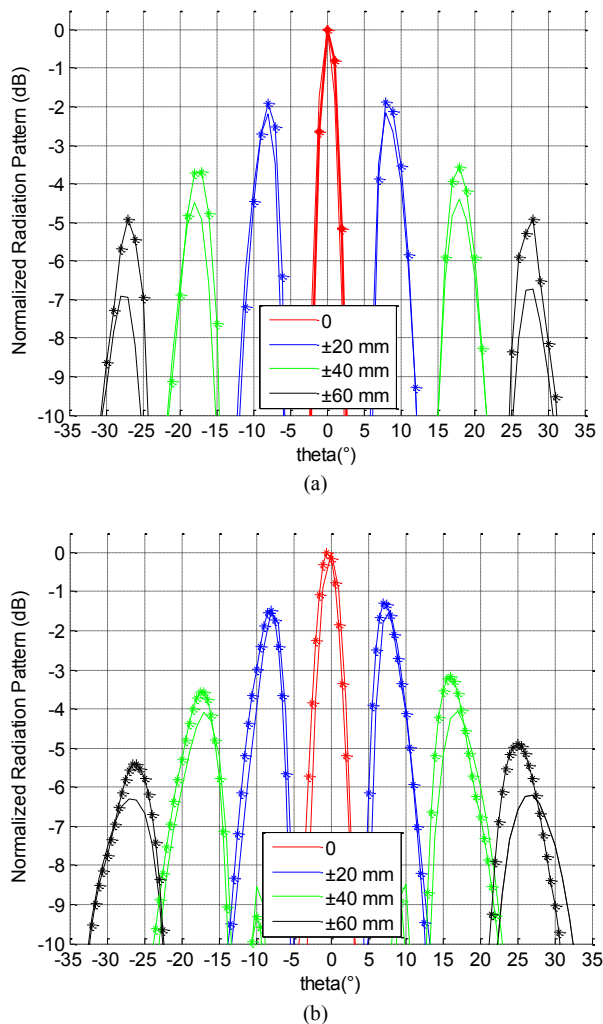


Fig. 12. Computed and measured radiation patterns of unifocal TA, for different beam pointing directions, (a) at 29 GHz in E-plane and (b) at 19.5 GHz in the H-plane. Curves with markers correspond to experimental results. All curves are normalized to the maximum gain at boresight. The reported results are zoomed close to the main beam to better appreciate the scan loss level, as compared to bifocal designs (Figs. 10 and 11).

IV. CONCLUSION

The paper has demonstrated experimentally independent scanning of transmitarray antennas in up- and down-links at Ka-band. Two prototypes have been fully characterized to validate their scanning capabilities. Both operate in dual-band (their design relies on the interleaving technique), and one of them exhibits two focal points in each band to extend its maximum scanning range. Our results show that it is possible to scan the TA beam over 80° and 60° in elevation, with only 2-dB of loss at 19.5 GHz and 29 GHz respectively. Indeed, the wide beam scanning provided by this architecture, with two independent beams operating in different frequency bands, makes it an excellent candidate for SOTM applications or for 5G applications.

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