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# Mutual-Coupling Isolation Using Embedded Metamaterial EM Bandgap Decoupling Slab for Densely Packed Array Antennas

MOHAMMAD ALIBAKHSHIKENARI<sup>1</sup>, (Student Member, IEEE),  
MOHSEN KHALILY<sup>2</sup>, (Senior Member, IEEE),  
BAL SINGH VIRDEE<sup>3</sup>, (Senior Member, IEEE),  
CHAN HWANG SEE<sup>4,5</sup>, (Senior Member, IEEE),  
RAED A. ABD-ALHAMEED<sup>6,7</sup>, (Senior Member, IEEE),  
AND ERNESTO LIMITI<sup>1</sup>, (Senior Member, IEEE)

<sup>1</sup>Electronic Engineering Department, University of Rome "Tor Vergata", via del politecnico 1, 00133 Rome, Italy

<sup>2</sup>Institute for Communication Systems, Home of the 5G Innovation Center, University of Surrey, Guildford GU2 7XH, U.K.

<sup>3</sup>Center for Communications Technology and Mathematics, School of Computing and Digital Media, London Metropolitan University, London N7 8DB, U.K.

<sup>4</sup>School of Engineering and the Built Environment, Edinburgh Napier University, Edinburgh EH10 5DT, U.K.

<sup>5</sup>School of Engineering, University of Bolton, Bolton BL3 5AB, U.K.

<sup>6</sup>Faculty of Engineering and Informatics, University of Bradford, Bradford BD7 1DP, U.K.

<sup>7</sup>Department of Communication and Informatics Engineering, College of Science and Technology, Basra University, Basra 61004, Iraq

Corresponding author: Mohsen Khalily (m.khalily@surrey.ac.uk)

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**ABSTRACT** This paper presents a unique technique to enhance isolation between transmit/receive radiating elements in densely packed array antenna by embedding a metamaterial (MTM) electromagnetic bandgap (EMBG) structure in the space between the radiating elements to suppress surface currents that would otherwise contribute towards mutual coupling between the array elements. The proposed MTM-EMBG structure is a cross-shaped microstrip transmission line on which are imprinted two outward facing E-shaped slits. Unlike other MTM structures, there is no short-circuit grounding using via-holes. With this approach, the maximum measured mutual coupling achieved is  $-60$  dB @ 9.18 GHz between the transmit patches (#1 & #2) and receive patches (#3 & #4) in a four-element array antenna. Across the antenna's measured operating frequency range of 9.12–9.96 GHz, the minimum measured isolation between each element of the array is 34.2 dB @ 9.48 GHz, and there is no degradation in radiation patterns. The average measured isolation over this frequency range is 47 dB. The results presented confirm the proposed technique is suitable in applications such as synthetic aperture radar and multiple-input multiple-output systems.

**INDEX TERMS** Metamaterial, electromagnetic bandgap, array antennas, decoupling slab, mutual coupling, synthetic aperture radar, multiple-input multiple-output.

## I. INTRODUCTION

In recent years, it has become a necessity to reduce the size of wireless communications systems. However, the size of certain components such as antennas is governed by the wavelength of the signal. Hence, reducing the size of radiating elements in wireless systems has become an area of intense investigation. Antennas are also employed in arrays

for applications like multiple-input multiple-output systems where they are prone to detrimental effects of surface waves and near-field, which cause adverse mutual coupling between adjacent  $E$ -plane coupled microstrip radiating elements. The effect of surface waves becomes especially dominant when the gap between the elements is greater than  $0.3\lambda_0$  [1]. Mutual coupling can severely degrade the antenna's radiation characteristics (pattern and efficiency). In addition, mutual coupling can cause correlation between the transmitted and received signals when the antennas are in close-proximity

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to each other that can result is diminution of system performance [2].

Numerous approaches have been investigated to reduce the mutual coupling between closely located antennas. Examples include using: (i) shorting patches to prevent the excitations of the surface waves [3]; (ii) cavity-backed slots [4]; (iii) partial substrate removal [5]; (iv) planar soft surfaces [6]; (v) parasitic element isolators [7]; (vi) metamaterial insulators for small-size antennas [8], [9]; and (vii) reversal of current through the metamaterial radiators [10].

EM bandgap structures have also been used in planar antennas to improve the antenna's performance [11], [12]. EM bandgap structures consist of periodic structures with half-wavelength periodicity separation of dielectric or metal elements that function to prevent propagation of surface waves within its bandgap [13]. The accommodation of half-wavelength periodicity separation in array antennas is physically challenging. Hence, various attempts have been carried out to reduce the size of EM bandgap structures [14]–[16]. Properties of EM bandgap have been exploited to reduce mutual coupling between antenna elements [17]–[24].

Wireless transceivers employing full-duplex (i.e. simultaneous transmit/receive) currently employ distinct frequencies for transmit and receive channels. Studies show that by using a single frequency for the full-duplex operation can substantially increase throughput as well as simplify the front-end architecture of a transceiver [25]. Various other approaches for full-duplex communication have also been investigated previously including optimising the antenna geometry [26]–[28], using various polarization diversity techniques [29]–[31], exploiting digital beamforming [32], near-field filtering [33], [34], RF-canceller [35], combined mechanical/EBG structures [36] and sharing single antenna [37]. However, there is still a need for small-size antenna configurations with high-isolation between adjacent radiating elements.

In this paper, a technique is described to realise high isolation between antenna elements suitable for array antennas or full-duplex high-speed target radars. The array antenna used to demonstrate this technique consists of four-element patch radiators implemented on the same substrate. The array antenna is designed to operate over 9.12 to 9.96 GHz with bandwidth of 840 MHz, which is extensive band for MIMO and SAR applications. Mutual coupling reduction is achieved by employing a unique metamaterial EM bandgap decoupling slab. Unlike conventional mutual coupling reduction approaches, the proposed technique provides high isolation between radiating elements and the size of the array antenna remains unchanged. The antenna performance and mutual coupling were analysed using standard full-wave EM simulation tools and then were validated by the measurements. In addition, to more validity of the proposed method the results extracted from the full wave EM simulator have compared with the circuit model, which show an excellent agreement with each other proving the precisely of the proposed approach.

## II. MUTUAL COUPLING REDUCTION BETWEEN ARRAY ELEMENTS

This section first discusses the basic array antenna used in this study as a reference that is constituted from four square patches with no decoupling slab. Reflection and transmission coefficient response of the array is presented without and with loading of a cross-shaped simple decoupling slab (SDS), which is located between the four radiators, to show the degree of mutual coupling suppression between array's elements. Enhanced suppression is demonstrated in section III by employing MTM electromagnetic bandgap (EMBG) decoupling structure.

### A. ARRAY ANTENNA STRUCTURE

The reference array antenna, depicted in Fig. 1, is constructed with four identical square microstrip patches, where each patch is excited individually. Dielectric substrate used is a lossy FR-4 with dielectric constant  $\epsilon_r = 4.3$ , thickness  $h = 1.6$  mm and loss-tangent  $\tan\delta = 0.025$ . The configuration of the array antenna is symmetrical.

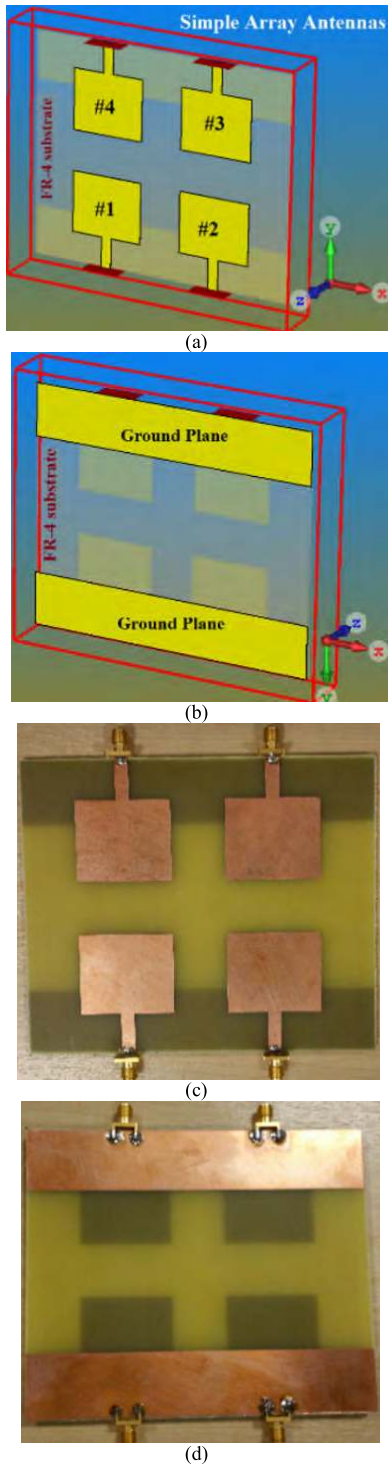
TABLE 1. Isolation between array antenna's elements.

S-parameters	$S_{12}$	$S_{13}$	$S_{14}$
Minimum	16.95dB @9.42GHz	34.0dB @9.12GHz	18.0dB @9.42GHz
Average	19.5 dB	35.75 dB	20.0dB
Maximum	21.85dB @9.96GHz	37.5dB @9.60GHz	22.0dB @9.96GHz

Measured S-parameter responses (reflection coefficient ( $S_{11} < -10$ dB) and transmission coefficients ( $S_{12}$ ,  $S_{13}$ , &  $S_{14}$ ) of each radiating element (#1 to #4) of the reference array antenna are shown in Fig. 2. The patch antennas operate from 9.12 GHz to 9.60 GHz with frequency bandwidth, maximum impedance matching and fractional bandwidth of 480 MHz,  $-40$  dB at 9.36 GHz (resonance frequency), and 5.13%, respectively. The isolation (minimum, average, and maximum) between elements: #1 & #2; #1 & #3; and #1 & #4, are given in Table 1. Due to symmetrical configuration of the proposed array antenna, the isolation between other adjacent elements are identical.

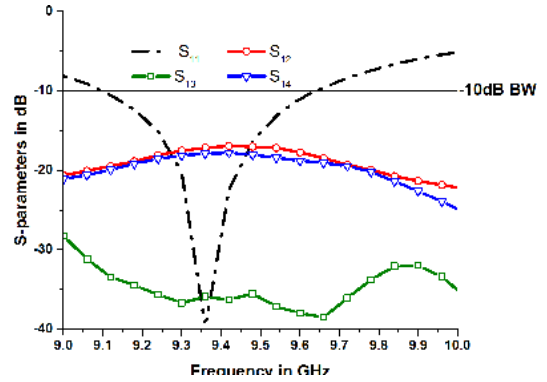
### B. ARRAY ANTENNA WITH SIMPLE DECOUPLING SLAB

The main challenge is to achieve high isolation between the antenna elements while keeping them as close possible to each other to realize a compact array. A simple cross-shaped decoupling slab, shown in Fig. 3, was used to improve the isolation between the radiating elements of the array antenna in Fig. 1. The decoupling slab was inserted between the array's elements, as shown in Fig. 4. In the array antenna, patch #1 & #2 is used for transmission, and #3 & #4 for reception. Ground-plane of the array antenna is truncated as shown in Figs. 4 (b) and 4(d).



**FIGURE 1.** Reference array antenna configuration using four identical square patches, (a) top view of array antenna comprising four microstrip patches, (b) ground plane of array antenna, (c) fabricated prototype of the antenna, and (d) ground plane view of the fabricated antenna prototype.

The S-parameter performance of the array antenna with the decoupling slab in Fig. 5 shows the array has an impedance bandwidth of 720 MHz from 9.12 to 9.84 GHz, which is corresponds to fractional bandwidth of 7.6%. Comparing Figs. 2 and 5, it is evident by inserting SDS the antenna's

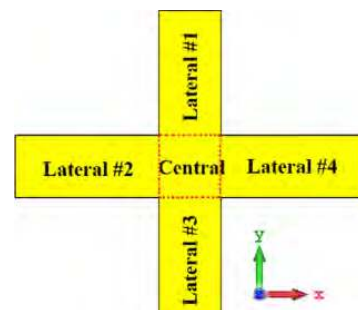


**FIGURE 2.** Measured reflection coefficient ( $S_{11} < -10\text{dB}$ ) and transmission coefficients ( $S_{12}$ ,  $S_{13}$ , &  $S_{14}$ ) of the reference array antenna.

bandwidth is extended by 240 MHz. This shows the decoupling slab does not degrade the impedance bandwidth of the array antenna. Optimum impedance match of  $-25\text{ dB}$  is observed at resonance frequency of 9.37 GHz. By applying the simple decoupling slab, the measured isolation of greater than 10 dB is achieved between the transmit patches (#1 & #2) and receive patches (#3 & #4). The minimum, average, and maximum transition coefficients ( $S_{12}$ ,  $S_{13}$ , and  $S_{14}$ ) are given in Table 2. Due to symmetrical configuration of the proposed array antenna, the isolation between other adjacent elements is identical.

**TABLE 2.** Isolation between array antenna's elements.

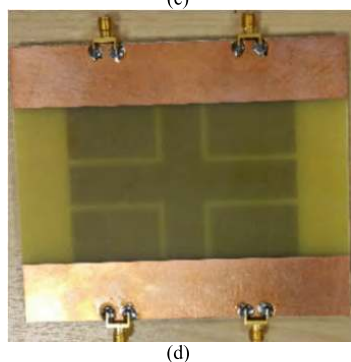
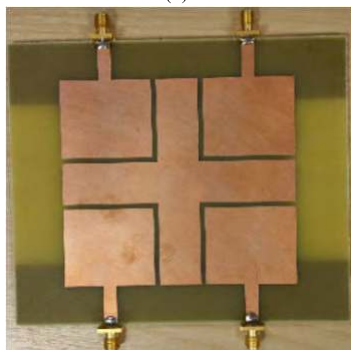
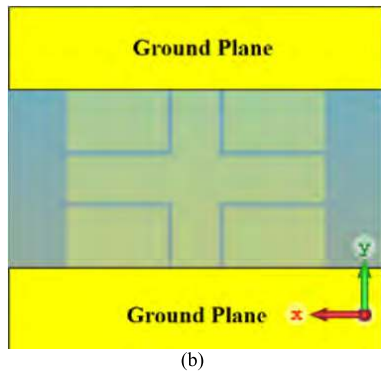
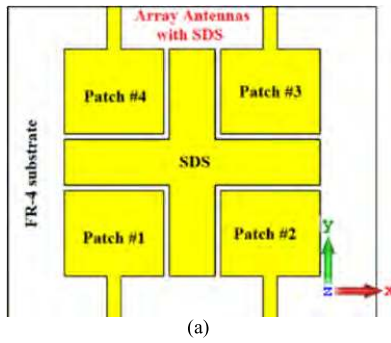
S-parameters	$S_{12}$	$S_{13}$	$S_{14}$
Minimum	22.0dB @9.84GHz	30.66dB @9.12GHz	19.13dB @9.48GHz
Average	27.0dB	34.52dB	24.0dB
Maximum	32.0dB @9.12GHz	38.9dB @9.54GHz	27.5dB @9.84GHz



**FIGURE 3.** Simple decoupling slab structure (SDS).

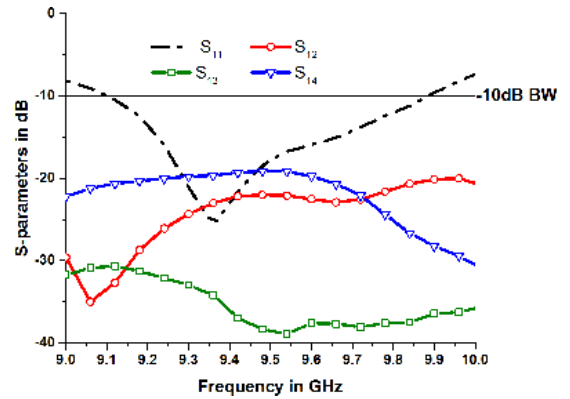
### III. DECOUPLING SLAB WITH EMBEDDED EM BANDGAP

Conventional microstrip antenna are built on dielectric substrates that comprise conductive tracks implemented on the top surface with a conductive ground-plane on the bottom surface of the substrate. It is shown in [38] that only

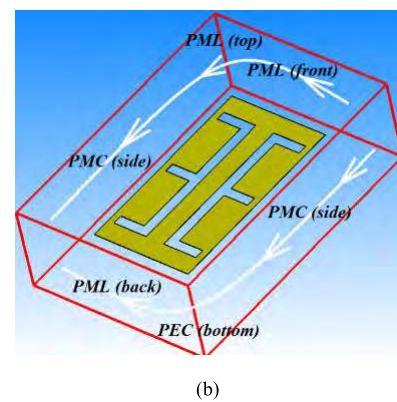
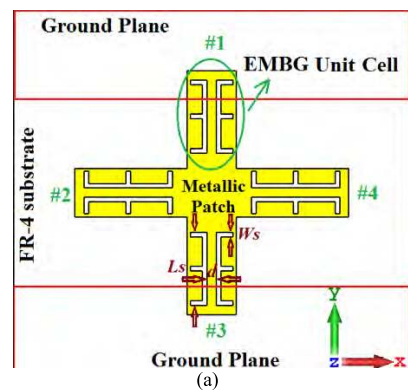


**FIGURE 4.** Array antenna configuration with embedded SDS, (a) simulated top view, (b) simulated back view of ground-plane, (c) fabricated prototype of the array, and (d) fabricated prototype of the ground plane.

$TM^{odd}$  and  $TE^{even}$  modes propagate in a microstrip structure, and the cut-off frequency of  $TM^{odd}$  is independent of substrate thickness. It is this mode that propagates through a thin substrate, and along with surface currents contribute towards mutual coupling. The suppression of surface currents between adjacent radiating elements in an array antenna and



**FIGURE 5.** Measured S-parameters performances of the array antenna with simple decoupling slab.



**FIGURE 6.** (a) Proposed MTM based EMBG decoupling slab embedded with four unit-cells of double E-shaped slits, and (b) EM bandgap unit-cell boundary conditions for full-wave simulation using finite element method solver.

$TM^{odd}$  mode is therefore necessary to prevent degradation of the radiation pattern in array antennas. EMBG structure shown in Fig. 6 is used here to minimize mutual coupling between neighbouring antennas in the array.

The proposed MTM-EMBG structure consists of resonant elements that are magnetically coupled to the dominant substrate mode, as shown in Fig. 6. Construction of the EM bandgap isolator involves embedding two identical E-shaped slits in each arm of the conductive decoupling slab of Fig. 3.

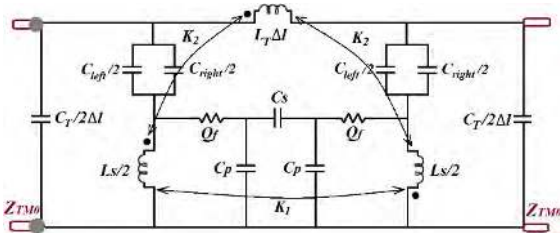


FIGURE 7. Transmission-line model of the EM bandgap unit-cell.

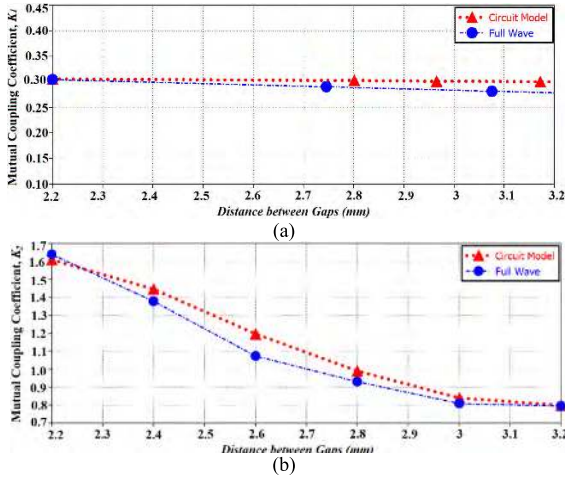


FIGURE 8. Comparison between full-wave and circuit model of coupling coefficients ( $K_1$  and  $K_2$ ) as a function of gap between the E-shaped slits, (a)  $K_1$ , and (b)  $K_2$ .

The slab essentially acts like a shunt inductance, and the two outwards facing E-shaped slits act as a series capacitor. Horizontally polarized magnetic-field coupling the slits induce electric currents on the MTM-EMBG decoupling slab that generate a magnetic-field in the opposite direction. When the E-shaped slits are in close-proximity, the inductance of the slab increases. At resonant frequency, the MTM-EMBG decoupling slab becomes essentially a perfect magnetic conductor that thwarts propagation of the substrate mode. Self-inductance resulting from mutual coupling interaction can be characterised by [39]

$$L_T = \frac{\mu_r \mu_0 A_{strip}}{d} \quad (1)$$

where  $A_{strip}$  is the surface area region bounding the E-shaped slits, and  $d$  is the gap between the slits. Horizontal magnetic-fields induce current in the conducting track that generates perpendicular electric-fields at the edges of the slits, and the corresponding capacitance can be calculated using [40]

$$C_T = \epsilon_r \epsilon_0 \frac{K(k_T)}{K(\sqrt{1-k_T^2})} \quad (2a)$$

$$k_T = \sin\left(\frac{\pi}{2}\eta\right) + 2\frac{\sqrt{\eta}}{1+\eta} \quad (2b)$$

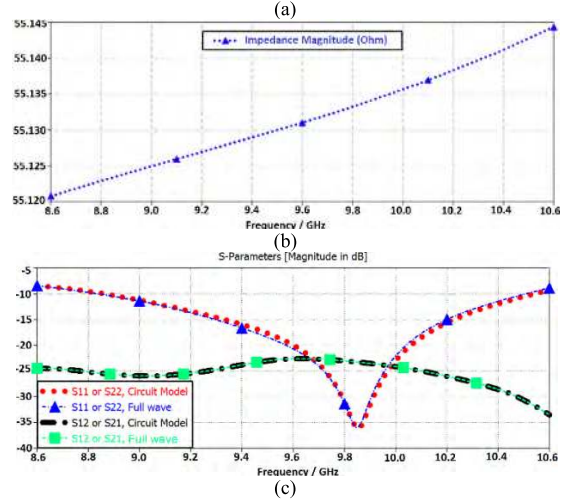
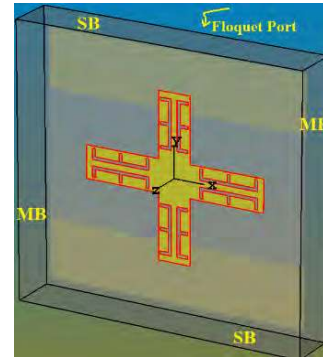


FIGURE 9. The proposed MTM EM bandgap decoupling structure etched on the top side of the substrate and excited by 50Ω microstrip transmission line on the bottom of the substrate: (a) Simulation model for determining the characteristics of the MTM-EMBG decoupling structure with slot width and length of  $W_s = 1.5\text{mm}$  and  $L_s = 24\text{mm}$ , respectively; Note, MB and SB represent the master and slave boundaries, respectively; (b) Simulated surface impedance of the MTM-EMBG decoupling structure; and (c) Simulated and circuit model reflection and transmission coefficients of the MTM-EMBG decoupling structure.

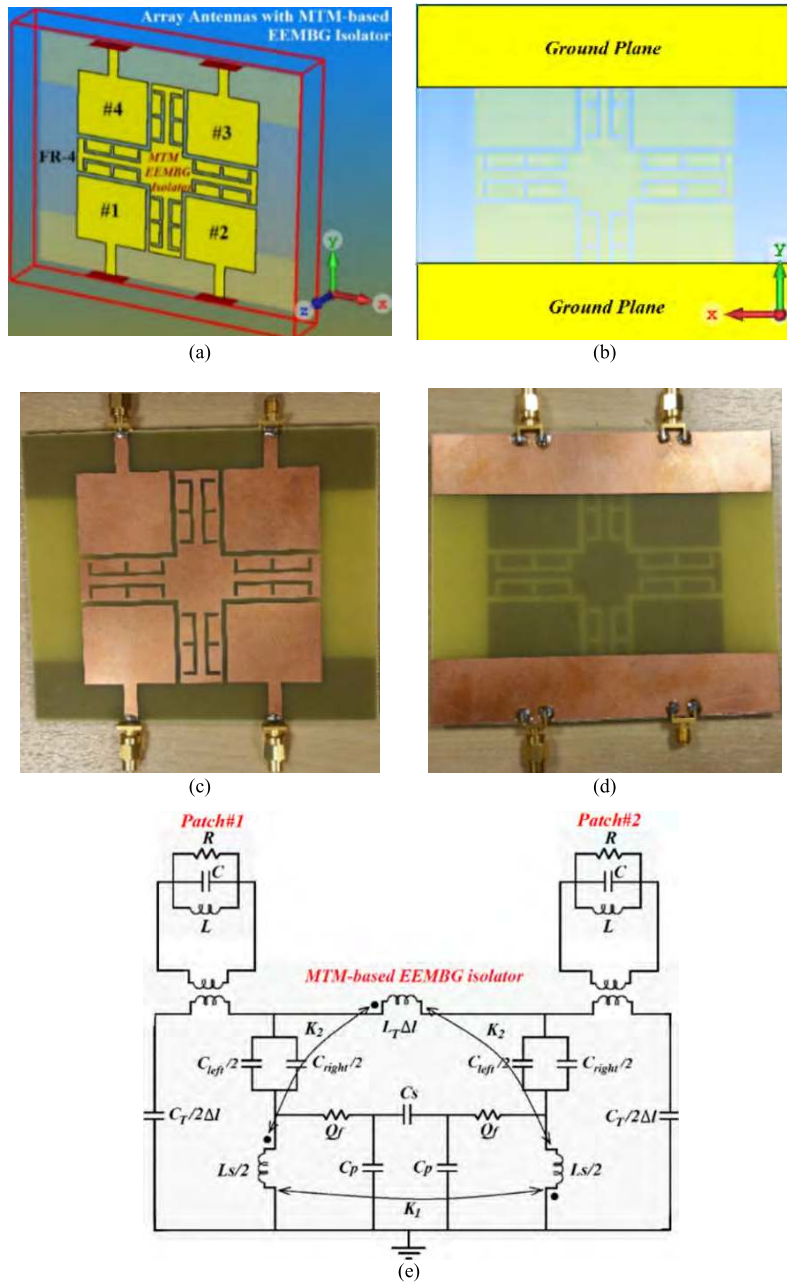
where  $\eta$  is the metallization ratio, and  $K(k)$  is the complete elliptic integral of first kind defined by [40]

$$\eta = \frac{w_s}{w_s + d} \quad (2c)$$

$$K(k) = \int_0^{\frac{\pi}{2}} \frac{d\theta}{\sqrt{1-k^2 \sin^2\theta}} \quad (2d)$$

where  $w_s$  is width of slits, and  $d$  represents gap between them (see Fig. 6). The inductance and capacitance of the EMBG unit-cell at 9.4 GHz is determined to be  $L_T = 12.8nH$  and  $C_S = 3.5pF$ , respectively.

From [39], [40] the transmission-line model for the MTM-EMBG structure is shown in Fig. 7. Inductance of the EM bandgap unit-cell can be represented with an inductive mutual coupling  $K_1$ . The mutual coupling between two horizontal E-shaped slits is represented by  $K_2$ . Mutual coupling between the equivalent transmission-line and the E-shaped slits is expressed by capacitive coupling  $C_{right}$  and  $C_{left}$  corresponding to the right and left slits, respectively.  $Q_f$  and  $C_p$  represent the quality-factor of the MTM-EMBG structure and



**FIGURE 10.** Geometry of the array antenna with MTM-EM bandgap decoupling slab, (a) simulated top view, (b) simulated bottom view of ground-plane, (c) fabricated prototype of the array, (d) fabricated prototype of the ground plane, and (e) the equivalent circuit model of the vertical unit-cell interfaced with patch antennas #1 and #2.

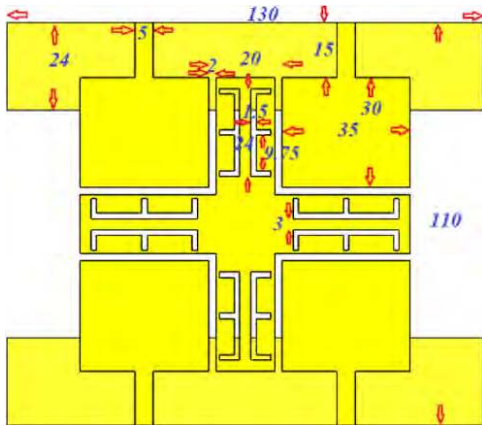
the parasitic capacitance between the slab and ground plane, respectively.

To confirm the accuracy of the MTM-EMBG structure model, a 3D EM full-wave solver (CST Microwave Studio ver. 2016) was employed. As shown in Fig. 6(b), the perfect magnetic conductor (PMC) walls impose the boundary conditions around the unit-cells. Perfectly matched layers (PMLs) are assigned to eliminate nonphysical reflections at the boundary of the upper free-space and the front and back sides. Perfect electric conductor (PEC) is assigned at

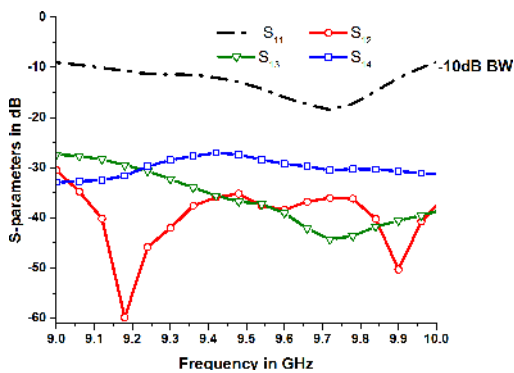
the bottom as ground plane. Equivalent circuit parameters of the MTM-EMBG unit-cell from the 3D EM full-wave solver is given in Table 3. This information was then used to determine the equivalent electrical circuit model, shown in Fig. 7, which was verified using Keysight’s ADS (RF circuit solver). Fig. 8 shows how the mutual coupling coefficient  $K_1$  and  $K_2$  are affected with variation in the gap between the E-shaped slits using circuit model and 3D EM full-wave solver. The proposed equivalent circuit model correlates well with the 3D EM full-wave solver results.

**TABLE 3.** Extracted circuit elements of the MTM-EMBG unit-cell equivalent circuit model.

$C_S$	3.5 pF
$L_S$	12.8 nH
$K_1$	0.28
$K_2$	0.8
$C_p$	4.36 pF
$C_{right}$	7.95 pF
$C_{left}$	7.95 pF
$Q_f$	2.1 $\Omega$
$\Delta l$	3 mm
$Z_{TMO}$	50 $\Omega$

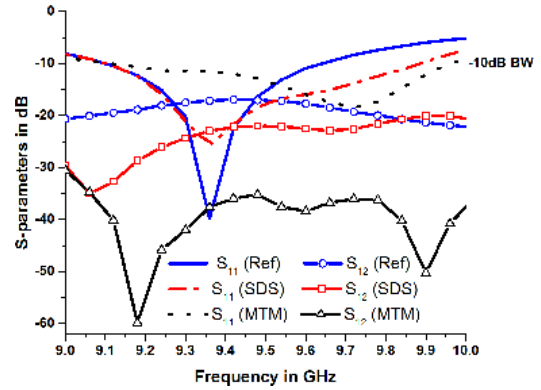


**FIGURE 11.** Dimensions (in millimetre) of the proposed antenna array with MTM EM bandgap isolator.

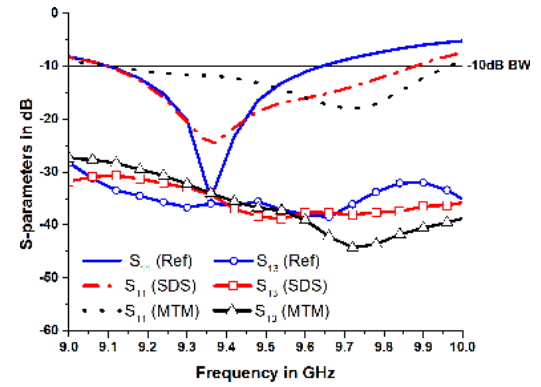


**FIGURE 12.** Measured S-parameters of the array antenna with MTM bandgap decoupling slab.

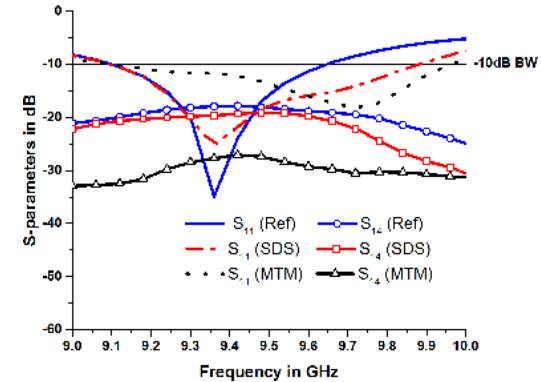
Mutual coupling coefficients  $K_1$  and  $K_2$  describe the magnetic-field linkage between the substrate mode and the EM bandgap isolator, and are dependent on the physical dimensions of the EM bandgap isolator. Fig. 8 shows that as the gap between the unit-cell becomes larger, the mutual coupling between the two E-shaped gaps ( $K_2$ ) becomes weaker; however, the inductive coupling between the substrate mode



(a)



(b)

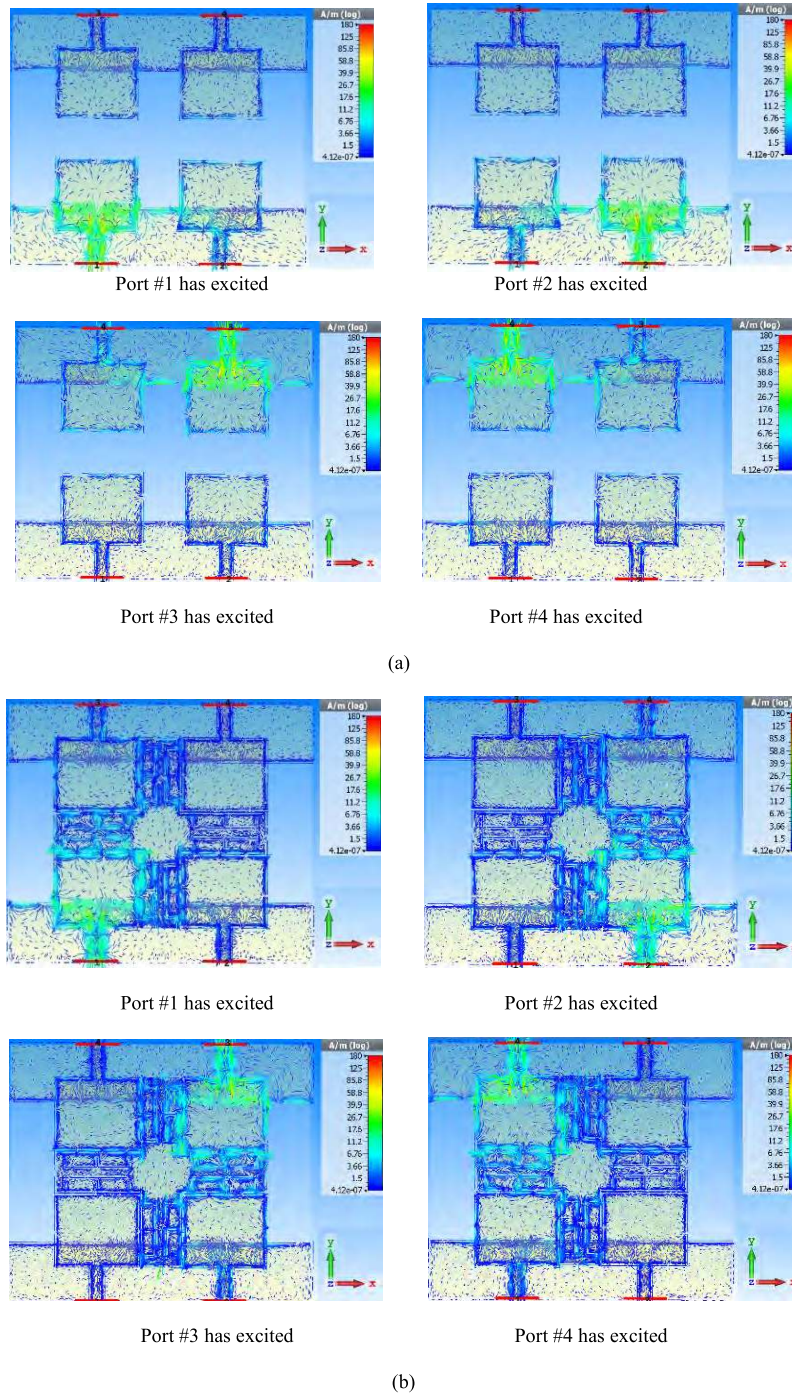


(c)

**FIGURE 13.** Measured S-parameter responses of the proposed array antennas before and after applying MTM-EMBG isolator, (a) between elements #1 & #2, (b) between elements #1 & #3, and (c) between elements #1 & #4.

and the unit-cell ( $K_1$ ) shows little variations to the gap between the slits within the range ( $\lambda_g/16 \sim \lambda_g/12$ ).

Characterisation of the proposed MTM-EMBG decoupling structure can be obtained from simulation of the model in Fig. 9(a). The simulated surface impedance is shown in Fig. 9(b). It can be observed the MTM-EMBG decoupling structure exhibits acceptable impedance over its operational frequency range from 8.8 to 10.5 GHz. The reflection coefficients are shown in Fig. 9(c). The results show the decoupling structure design is optimum at  $\sim 9.85$  GHz.



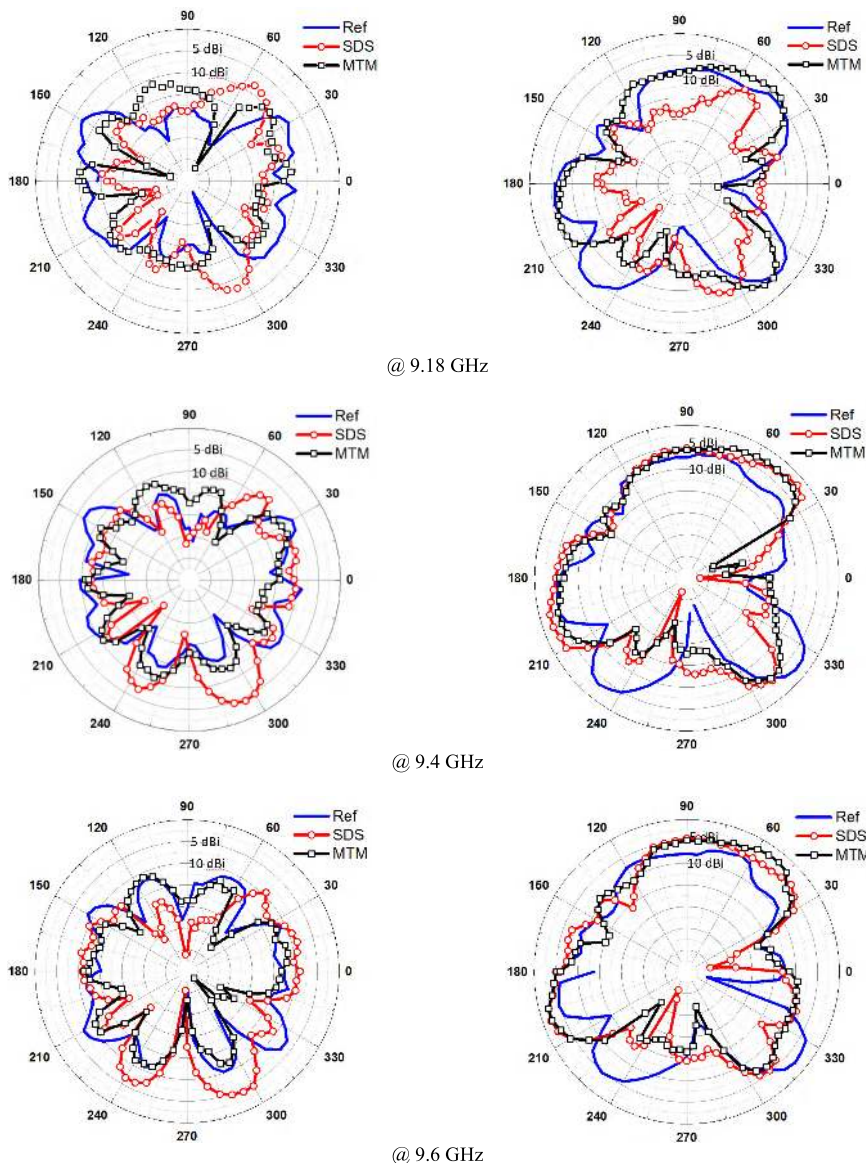
**FIGURE 14.** Current density over the array antenna at 9.6 GHz, (a) with no MTM-EMBG decoupling slab, and (b) with MTM-EMBG decoupling slab.

#### IV. ARRAY ANTENNA WITH MTM-EM BANDGAP ISOLATOR

Functionality of the proposed MTM-EMBG decoupling slab is demonstrated with a four-element antenna array, where the cross shaped decoupling slab is inserted between the patch antenna arrangement, as shown in Fig. 10(a), where Antennas #1 & #2 are used for transmission (TX), and

Antennas #3 & #4 are used for reception (RX) in a RF transceiver. The ground-plane on the back side of the substrate is truncated, as shown in Fig. 10(b). The distance between the adjacent radiating elements ( $d_1$ ) and gap between the elements and the decoupling slab ( $d_2$ ) are 20 mm ( $0.6\lambda_0$ ) and 2 mm ( $0.06\lambda_0$ ), respectively, where  $\lambda_0$  is the free space wavelength at 9.12 GHz.





**FIGURE 15.** Measured radiation patterns of the array antennas, i.e. reference, with SDS, and with MTM-EMBG, at the operational frequencies of 9.18, 9.4, and 9.6 GHz. Please note with reference to Fig. 1(a) the left-hand plots are in the x-y plane and the right-hand plots are in the y-z plane.

The MTM-EMBG decoupling slab was designed for optimum performance at 9.6 GHz. The equivalent circuit model of the vertical unit-cell coupled to patch#1 & #2 is shown in Fig. 10(e). The equivalent circuit of other unit-cells coupled with adjacent patch antennas is similar. Value for RLC parameters are: 5.2 Ω, 11.5 nH, and 7.8 pF, respectively. The decoupling slab has a slot width of  $W_s = 1.5$  mm and slot length of  $L_s = 24$  mm. Dimensions of the array antenna are given in Fig. 11.

The antenna’s S-parameter responses are depicted in Fig. 12. The bandwidth of the array antenna is 840 MHz (9.12 GHz to 9.96 GHz), with a fractional bandwidth of 8.8%. The bandwidth has extended by 360 MHz. Besides the

**TABLE 4.** Isolation between array antenna’s elements.

S-parameters	$S_{12}$	$S_{13}$	$S_{14}$
Minimum	34.2dB @9.48GHz	28.33dB @9.12GHz	27.0dB @9.42GHz
Average	47.0dB	36.12dB	30.0dB
Maximum	60.0dB @9.18GHz	44.3dB @9.72GHz	33dB @9.12GHz

reflection coefficients, the magnitude of the transition coefficients ( $S_{12}$ ,  $S_{13}$ , and  $S_{14}$ ) have substantially dropped. The minimum, average, and maximum magnitudes for  $S_{12}$  are:

TABLE 5. S-Parameter characteristics of the proposed array antenna.

$S_{11}, S_{22}, S_{33}, S_{44} < -10$ dB	Average matching	Max. matching	Bandwidth	Fractional BW
Reference Array	-25dB	-40dB @ 9.36GHz	9.12 – 9.6 GHz	5.13%
With SDS	-17.5dB	-25.76dB @ 9.36GHz	9.12 – 9.84 GHz	7.6%
With MTM-EMBG	-14.5dB	-18.45dB @ 9.72GHz	9.12 – 9.96 GHz	8.80%

$S_{12}$ & $S_{34}$	Min. isolation	Average isolation	Max. isolation
Reference Array	16.95dB @ 9.42GHz	19.5dB	21.85dB @ 9.96GHz
With SDS	22dB @ 9.84 GHz	27dB	32dB @ 9.12GHz
With MTM-EMBG	34.2dB @ 9.48GHz	47dB	60dB @ 9.18GHz

$S_{13}$ & $S_{24}$	Min. isolation	Average isolation	Max. isolation
Reference Array	34dB @ 9.12GHz	35.75dB	37.5dB @ 9.60GHz
With SDS	30.66dB @ 9.12GHz	34.52dB	38.9dB @ 9.54GHz
With MTM-EMBG	28.33dB @ 9.12GHz	36.12dB	44.3dB @ 9.72GHz

$S_{14}$ & $S_{23}$	Min. isolation	Average isolation	Max. isolation
Reference Array	18.0dB @ 9.42GHz	20.0dB	22.0dB @ 9.96GHz
With SDS	19.13dB @ 9.48GHz	24.0dB	27.5 @ 9.84GHz
With MTM-EMBG	27.0dB @ 9.42GHz	30dB	33dB @ 9.12GHz

−34.2 dB, −47 dB, and −60 dB; for  $S_{13}$  they are −28.33 dB, −36.12 dB, and −44.3 dB; and for  $S_{14}$  they are −27 dB, −30 dB, and −33 dB. For clarity these results are given in Table 4. The proposed structure's optimum performance is at 9.6 GHz with impedance matching of −15.0 dB. At this frequency the antenna's isolation between elements #1 & #2, #1 & #3, and #1 & #4 are 38.2 dB, 38.2 dB, and 30.15 dB, respectively. This reveals greater than 10 dB improvement in isolation compared with the reference antenna at 9.6 GHz between the transmit patches (#1 & #2) and receive patches (#3 & #4). Due to symmetrical configuration of the proposed array antenna, the isolation between other adjacent elements is identical.

The measured S-parameter responses without decoupling slab (reference case), with SDS, and with MTM-EMBG decoupling slab are shown in Fig.13. It is evident that with MTM-EMBG, (i) the reflection coefficient is better than −15 dB at around 9.6 GHz; and (ii) improvement in the impedance bandwidth is greater than 350 MHz. It's worth to mention that, the resonance frequencies for the reference antenna without decoupling slab and the antenna with simple decoupling slab are same. However, it has shifted to the high frequency after applying the metamaterial decoupling slab. The reason is that, when we have realized the metamaterial properties by etching the E-shaped slots on the decoupling slab the series left-handed capacitances have generated that enhance the capacitive property of the entire structure, which is caused to shift the resonance frequency to higher frequency.

Surface wave suppression functionality of the MTM-EMBG decoupling slab is evident in the experimental transmission coefficient ( $S_{12}$ ) response between antenna elements #1 & #2, shown in Fig. 13(a). MTM-EMBG decoupling slab has a significant effect on whole of the frequency bandwidth from 9.12 – 9.96 GHz. At 9.18 GHz, the difference in isolation is more than 40 dB and at 9.6 GHz the

isolation deteriorates to more than 20 dB. This is because the MTM-EMBG unit-cell has a finite operational bandwidth. Due to symmetrical configuration of the array antenna the transmission coefficient between elements #3 & #4 is identical to between elements #1 & #2 (i.e.  $S_{34} = S_{12}$ ). The measured transmission coefficient response between elements #1 & #3, and elements #1 & #4 with and without MTM-EMBG are shown in Figs. 13(b) and 13(c), respectively. It is clear from Fig. 13(b) that, the MTM-EMBG decoupling slab has moderate effect at higher frequencies and the isolation tends to converge between 9.4 and 9.6 GHz. The measured transmission coefficient between elements #1 & #4 are shown in Fig. 13(c), which is identical to between elements #2 & #3 ( $S_{23} = S_{14}$ ). At 9.18 GHz, the difference in isolation is 15 dB, and at 9.6 GHz the isolation is 12 dB. These results clearly show the effectiveness of the MTM-EMBG decoupling structure in reducing the mutual coupling between adjacent antennas encountered in array antennas. The results are summarized in the Table 5. It should be noted in the proposed technique no short-circuit grounding using via-holes has been used. Due to the symmetrical configuration of the proposed array antenna, the magnitude of  $S_{11}$  is identical to  $S_{22}$ ,  $S_{33}$ , and  $S_{44}$ . Also,  $S_{12} = S_{34}$ ,  $S_{13} = S_{24}$ , and  $S_{14} = S_{23}$ .

Current density distribution over the array antenna with and without MTM-EMBG decoupling slab is shown in Fig.14. It is evident from these plots the MTM-EMBG decoupling slab soaks up the fringing fields that would otherwise couple with the adjacent radiating elements.

The measured radiation patterns of four-element array antennas under the all three conditions (reference antenna with no loading, SDS and MTM-EMBG loadings) at 9.18 GHz, 9.4 GHz and 9.6 GHz are shown in Fig. 15. It is observed the radiation patterns with MTM-EMBG decoupling slab approximates the original reference antenna, and over certain angular directions can exhibit better

**TABLE 6.** Proposed antenna characteristics compared with recent works.

Refs.	Technique	Max. Isolation Improvement	Number of Elements	Symmetry	Impact on the Size after apply MTM	Changing and Developing (defected ground plane)	Complexity
[17]	UC-EBG	10 dB	2 (1×2)	NO	Yes	Yes	Yes
[41]	Slot in Ground plane	40 dB	2 (1×2)	NO	Yes	Yes	Yes
[42]	EBG	4 dB	2 (1×2)	NO	Yes	Yes	Yes
[43]	Compact EBG	17 dB	2 (1×2)	NO	Yes	Yes	Yes
[44]	DGS	17.43 dB	2 (1×2)	NO	Yes	Yes	Yes
[45]	U-shaped resonator	10 dB	2 (1×2)	NO	Yes	Yes	Yes
[46]	Slotted Meander Line Resonator	16 dB	2 (1×2)	NO	Yes	Yes	Yes
[47]	I-shaped resonator	30 dB	2 (1×2)	NO	Yes	Yes	Yes
[48]	SCSRR	10 dB	2 (1×2)	NO	Yes	Yes	Yes
[49]	SCSSRR	14.6 dB	2 (1×2)	NO	Yes	Yes	Yes
[50]	Waveguide MTM	20 dB	2 (1×2)	NO	Yes	Yes	Yes
[51]	Waveguide MTM	18 dB	2 (1×2)	NO	Yes	Yes	Yes
[52]	Meander line resonator	10 dB	2 (1×2)	NO	Yes	Yes	Yes
[53]	Fractal load with DGS	16 dB	2 (1×2)	NO	Yes	Yes	Yes
[54]	Antenna Interference Cancellation Chip (AICC)	15 dB	2 (1×2)	Yes	No	No	Yes
[55]	3-D Metamaterial Structure (3DMMS)	18 dB	2 (1×2)	Yes	Yes	No	No
<b>This work</b>	<b>Metamaterial</b>	<b>40 dB for <math>S_{12}</math> ~7 dB for <math>S_{13}</math> 11 dB for <math>S_{14}</math></b>	<b>4 (2×2)</b>	<b>Yes</b>	<b>NO</b>	<b>NO</b>	<b>NO</b>

gain performance. The maximum gain of the array antenna with the decoupling slab increased from 3.3 dBi to 5.4 dBi corresponding to 63% improvement.

## V. COMPARISONS WITH OTHER ANTENNAS

The proposed array antenna is compared with the several recent works in Table 6. In the literature, all the proposed designs are constructed with only two radiation elements, since they have not symmetrical configuration that impossible them to realize the arrays with more than two elements. However, in our case due to the symmetrical configuration of the structure we have increased the array elements to four. All papers referenced in Table 6 have defected ground plane to enhance isolation between the two radiating elements, which caused to enhance complexity of the structure and therefore the cost for manufacture procedures has increased. With the proposed technique the size of the array antenna remains unchanged. The maximum isolation improvement between adjacent antennas with the proposed method is 40 dB, which is comparable to [41], however unlike [41] in the proposed technique there is no need to temper with the ground plane, and the MTM-EMBG decoupling structure didn't require short-circuit vias. This resulted in a simple technique which can be retrofitted to existing antenna arrays quickly and at low cost for MIMO systems and SAR applications.

## VI. CONCLUSIONS

A novel technique is demonstrated to suppress mutual coupling between adjacent radiating elements in array antennas. This involves inserting a metamaterial electromagnetic bandgap decoupling structure between the radiating elements. The proposed MTM-EMBG structure, which does

not require any via-holes and defected ground plane structures, can be directly implemented on the surface of the planar array antenna. In addition, the MTM-EMBG structure can also be retrofitted with ease. Experimental results show excellent isolation is achieved with the decoupling slab across 9.12 to 9.96 GHz. The results confirm the proposed technique is suitable in applications such as synthetic aperture radar (SAR) and multiple-input multiple-output (MIMO) systems.

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**MOHAMMAD ALIBAKHSHIKENARI** (S'18) was born in 24. Feb. 1988 in Freydounkenar, Mazandaran, IRAN. He received the B.Sc. (Feb. 2010) and M.Sc. (Feb. 2013) degrees both in Electrical Engineering from the Islamic Azad University, Najafabad Branch of Esfahan, Iran and Shahid Bahonar University of Kerman, Iran, respectively. His research interests include array antennas, synthetic aperture radars (SAR), Multiple Input Multiple Output (MIMO) systems, waveguide slotted antenna arrays, substrate integrated waveguides (SIWs), on-chip antennas, microwave, millimeter-waves and terahertz applications, metamaterials, and electromagnetic-waves applications. The above research lines have produced more than 60 publications on refereed-international journals and presentations within international-conferences.

Mr. M. Alibakhshikeni is Postgraduate Studying as PhD candidate under supervision of Prof. Ernesto Limiti at the Electronic Engineering Department of the University of Rome "Tor Vergata", Rome, ITALY. He is member of the Microwave Engineering Center for Space Applications (M.E.C.S.A.). The head of the EE department and M.E.C.S.A. is Prof. Ernesto Limiti. He was two recipients of the 47th and 48th European Microwave Conference (EuMC) Young Engineer Prize in 2017 and 2018 held in Nuremberg (Germany) and Madrid (Spain), respectively, where he had presented his papers.

From 1st May 2018 to 1st November 2018 he was doing research activities as a PhD visiting researcher in the Antenna System Division, Electrical Engineering Department of the Chalmers University of Technology, Gothenburg, Sweden. As well as, at the same period he was working with the GAPWAVES institute in Gothenburg, Sweden as antenna researcher.



**MOHSEN KHALILY** (M'13–SM'18) is a Lecturer in antenna and propagation at Department of Electrical and Electronic Engineering, Faculty of Engineering and Physical Sciences (FEPS), University of Surrey, U.K. He was with Institute for Communication Systems (ICS), home of the 5G Innovation Centre (5GIC), University of Surrey as a research fellow on antenna and propagation from December 2015 to March 2019. Before joining 5GIC, he worked with Wireless Communication Center (WCC), Universiti Teknologi Malaysia (UTM) as a Senior Lecturer, and as a Postdoctoral Research Fellow, from 2012 to 2015. Dr Khalily is an IEEE Senior Member (SMIEEE), Fellow of UK Higher Education Academy, a Member of IEEE Antennas and Propagation Society, IEEE Communication Society, IEEE Microwave Theory and Techniques Society, an Associate Editor for IEEE Access and has published almost 80 academic papers in international peer-reviewed journals and conference proceedings. His research interests include: dielectric resonator antennas, MIMO antennas, phased array antennas, hybrid beamforming, mmWave body centric communication, and millimetre-wave antennas and propagation.



**BAL SINGH VIRDEE** (SM'08) received the B.Sc. and MPhil degrees in Communications-Engineering from the University of Leeds-UK and his Ph.D. in Electronic-Engineering from the University of London-UK. He has worked in industry for various companies including Philips (UK) as an R&D-engineer and Filtronic-Components Ltd. as a future products developer in the area of RF/microwave communications. He has taught at several academic institutions before joining London Metropolitan University where he is a Professor of Microwave-Communications in the Faculty of Life Sciences&Computing where he Heads the Center for Communications-Technology and is the Director of London Metropolitan-Microwaves. His research, in collaboration with industry and academia, is in the area of microwave wireless communications encompassing mobile-phones to satellite-technology. Prof. Virdee has chaired technical sessions at IEEE international conferences and published numerous research-papers. He is Executive-Member of IET's Technical and Professional Network Committee on RF/Microwave-Technology. He is a Fellow of IET and a Senior-Member of IEEE.



**CHAN HWANG SEE** (M'14–SM'15) received the first class B.Eng. honors degree in electronic, telecommunication, and computer engineering and the Ph.D. degree in computational bioelectromagnetics from the University of Bradford, Bradford, U.K. He is an associate Professor in the School of Engineering and the Built Environment, Edinburgh Napier University. He also is a Visiting Research Fellow in the School of Engineering and Informatics, University of Bradford and School of Engineering, University of Bolton. Previously, he was a Senior Lecturer, in University of Bolton and a Senior Research Fellow in the Antennas and Applied Electromagnetics Research Group within the University of Bradford. His research interests cover wireless sensor network system design, computational electromagnetism, antennas, microwave circuits and acoustic sensor design. He has published more than 200 peer-reviewed journal articles and conference papers. He is a coauthor of one book and five book chapters.

Dr. See received two Young Scientist Awards from the International Union of Radio Science and the Asia-Pacific Radio Science Conference in 2008 and 2010, respectively. He received a certificate of excellence for his successful Knowledge Transfer Partnership with Yorkshire Water on the design and implementation of a wireless sensor system for sewerage infrastructure monitoring in 2009. He is a Chartered Engineer in the U.K., and a Fellow of the Institution of Engineering and Technology, U.K. He is also a Fellow of The Higher Education Academy and an Associate Editor for IEEE Access.



**RAED A. ABD-ALHAMEED** (M'02–SM'13) received the B.Sc. and M.Sc. degrees from Basrah University, Basrah, Iraq, in 1982 and 1985, respectively, and the Ph.D. degree from the University of Bradford, Bradford, U.K., in 1997, all in electrical engineering.

He is a Professor of electromagnetic and radio frequency engineering at the University of Bradford. He has long years' research experience in the areas of radio frequency, signal processing, propagations, antennas, and electromagnetic computational techniques, and has published more than 600 academic journal and conference papers; in addition, he is a coauthor of four books and several book chapters. He is currently the Leader of Radio Frequency, Propagation, Sensor Design, and Signal Processing; in addition to leading the Communications research group for years within the faculty of Engineering and Informatics, Bradford University. He is a Principal Investigator for several funded applications to EPSRCs and leader of several successful Knowledge Transfer Programmes (KTPs) such as with Arris (previously known as Pace plc), Yorkshire Water

plc, Harvard Engineering plc, IETG Ltd., Seven Technologies Group, Emkay Ltd., and Two World Ltd. He has also been a Co-Investigator in several funded research projects including: H2020 MARIE Sklodowska-CURIE ACTIONS: Innovative Training Networks “Secure Network Coding for Next Generation Mobile Small Cells 5G-US,” nonlinear and demodulation mechanisms in biological tissue (Department of Health, Mobile Telecommunications & Health Research Programme, and Assessment of the Potential Direct Effects of Cellular Phones on the Nervous System (EU: collaboration with six other major research organizations across Europe). He received the Business Innovation Award for his successful KTP with Pace and Datong companies on the design and implementation of MIMO sensor systems and antenna array design for service localizations. He is the Chair of several successful workshops on Energy Efficient and Reconfigurable Transceivers: Approach Towards Energy Conservation and CO2 Reduction, that addresses the biggest challenges for future wireless systems. He was also appointed as a Guest Editor for IET Science, Measurements and Technology in 2009 and 2012. He has also been a Research Visitor at Glyndwr University, Wrexham, U.K., since September 2009, covering the wireless and communications research areas. His research interests include computational methods and optimizations, wireless and mobile communications, sensor design, EMC, beam steering antennas, energy-efficient PAs, RF predistorter design applications and 5G front end design.

Prof. Abd-Alhameed is the Fellow of the Institution of Engineering and Technology, U.K., a Fellow of the Higher Education Academy, and a Chartered Engineer in the U.K.



ERNESTO LIMITI (S'87–M'92–SM'17) is a full professor of Electronics in the Engineering Faculty of the University of Roma Tor Vergata since 2002, after being research and teaching assistant (since 1991) and associate professor (since 1998) in the same University. Ernesto Limiti represents University of Roma Tor Vergata in the governing body of the MECSA (Microwave Engineering Center for Space Applications), an inter-university center among several Italian Universities. He has been elected to represent the Industrial Engineering sector in the Academic Senate of the University for the period 2007-2010 and 2010-2013. Ernesto Limiti is actually the president of the Consortium “Advanced research and Engineering for Space”, ARES, formed between the University and two companies.

Further, he is actually the president of the Laurea and Laurea Magistrale degrees in Electronic Engineering of the University of Roma Tor Vergata. The research activity of Ernesto Limiti is focused on three main lines, all of them belonging to the microwave and millimetre-wave electronics research area. The first one is related to characterisation and modelling for active and passive microwave and millimetre-wave devices. Regarding active devices, the research line is oriented to the small-signal, noise and large signal modelling. Regarding passive devices, equivalent-circuit models have been developed for interacting discontinuities in microstrip, for typical MMIC passive components (MIM capacitors) and to waveguide/coplanar waveguide transitions analysis and design. For active devices, new methodologies have been developed for the noise characterisation and the subsequent modelling, and equivalent-circuit modelling strategies have been implemented both for small and large-signal operating regimes for GaAs, GaN, SiC, Si, InP MESFET/HEMT devices. The second line is related to design methodologies and characterisation methods for low noise circuits. The main focus is on cryogenic amplifiers and devices. Collaborations are currently ongoing with the major radioastronomy institutes all around Europe within the frame of FP6 and FP7 programmes (RadioNet). Finally, the third line is in the analysis methods for nonlinear microwave circuits. In this line, novel analysis methods (Spectral Balance) are developed, together with the stability analysis of the solutions making use of traditional (harmonic balance) approaches. The above research lines have produced more than 250 publications on refereed international journals and presentations within international conferences. Ernesto Limiti acts as a referee of international journals of the microwave and millimetre wave electronics sector and is in the steering committee of international conferences and workshops. He is actively involved in research activities with many research groups, both European and Italian, and he is in tight collaborations with high-tech italian (Selex - SI, Thales Alenia Space, Rheinmetall, Elettronica S.p.A., Space Engineering...) and foreign (OMMIC, Siemens, UMS,...) companies. He contributed, as a researcher and/or as unit responsible, to several National (PRIN MIUR, Madess CNR, Agenzia Spaziale Italiana) and international (ESPRIT COSMIC, Manpower, Edge, Special Action MEPI, ESA, EUROPA, Korrgan, RadioNet FP6 and FP7...) projects.

Regarding teaching activities, Ernesto Limiti teaches, over his institutional duties in the frame of the Corso di Laurea Magistrale in Ingegneria Elettronica, “Elettronica per lo Spazio” within the Master Course in Sistemi Avanzati di Comunicazione e Navigazione Satellitare. He is a member of the committee of the PhD program in Telecommunications and Microelectronics at the University of Roma Tor Vergata, tutoring an average of four PhD candidates per year.

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