

OFDR Based Distributed Temperature Sensor Using the Three-Channel Simultaneous Radio-Frequency Lock-In Technique

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Abstract: Weak signal detection for single-mode fiber-optic distributed temperature sensor (DTS) is a key technology to achieve better performance. A hybrid technique combining the incoherent optical frequency domain reflectometry (IOFDR) and the three-channel simultaneous radio-frequency (RF) lock-in amplifier (LIA) is presented to improve the signal-to-noise ratio (SNR) of the measured spontaneous Raman backscattered light. The field programmable gate array (FPGA) based RF-LIA is designed with a novel and simple structure. The measurement frequency range is achieved from 1 kHz to 100 MHz. Experimental results show that the backscattered light signal of picowatt level can be detected with high SNR. With a 2.5 km single-mode fiber, a 1064 nm laser source, and the measurement time of 500 s, this sensing system can reach a spatial resolution of 0.93 m and a temperature resolution of about 0.2 °C.

Keywords: Distributed temperature sensor, incoherent optical frequency domain reflectometry, radio-frequency lock-in amplifier, simultaneous detection

Citation: Ke CHEN, Xinlei ZHOU, Wei PENG, and Qingxu YU, "OFDR Based Distributed Temperature Sensor Using the Three-Channel Simultaneous Radio-Frequency Lock-In Technique," *Photonic Sensors*, 2015, 5(3): 217–223.

1. Introduction

The fiber-optic Raman distributed temperature sensor (DTS) can be realized with two different signal detection mechanisms: optical time domain reflectometry (OTDR) and incoherent optical frequency domain reflectometry (IOFDR) [1–3]. Based on the narrow-band signal detection method and the frequency modulated continued wave (FMCW) technology, the IOFDR method has many technical advantages, such as higher signal-to-noise ratio (SNR), lower sample rate, and longer working life of the light source [4, 5].

The power of the spontaneous Raman scattering from the optical fiber is about six orders of

magnitude weaker than that of the incident light. As a result, low SNR is the main limiting factor for achieving higher spatial resolution, higher temperature resolution, and longer measurement range [6]. This problem is much more serious in the DTS system using single-mode fiber [7, 8]. For an IOFDR-based DTS system, the amplitude of the useful alternating current (AC) signal is dramatically decreased with the modulation frequency increased. The signal power can be attenuated to picowatt level with the modulation frequency up to 50 MHz [8].

By using the electrical heterodyne technique, the received signal can be mixed to a low frequency signal. The digital band-pass filter has been used for

signal processing in IOFDR-based DTS [9], and a temperature resolution of 1.6°C was achieved with 3 m sampling resolution and 13.8 km single-mode fiber. However, due to the central frequency jitter of the digital filter, the additional noise is increased, which limits the improvements of spatial and temperature resolutions. The radio-frequency (RF) lock-in amplifier (LIA) is suitable for measuring the amplitude and phase of the weak AC signal [10, 11]. The phase-locked loop (PLL) technique used in the LIA can effectively eliminate the frequency jitter caused noise. Meanwhile, for an IOFDR-based DTS system, the signal dynamic range of at least 80 dB is required. The digital LIA is able to reach a dynamic range up to 110 dB [12]. By taking advantages of LIA, high SNR improvement and high measurement resolution can possibly be realized.

In this paper, in order to measure the amplitude and the phase shift of the weak Raman backscattered light signal in an IOFDR-based single-mode fiber-optic DTS system, a three-channel simultaneous RF-LIA technique is presented and realized with a novel structure. The SNR improvement of the Raman backscattered light signal is studied by experiments. Furthermore, the spatial and temperature resolutions are measured.

2. Principles

2.1 Principle of the IOFDR-Based DTS

The IOFDR method uses a continuous wave laser source which is sinusoidal intensity modulated by several stepwise increased frequencies. By using electrical heterodyne technique, the backscattered light signal can be mixed to a low-frequency signal. The AC part of the power of the received light can be expressed as [8]:

$$\tilde{P}_i(0, \omega_m, t) = P_0 \cdot m \cdot \Re \left(e^{j\omega_m t} \cdot \int_0^L \chi_R(z) \cdot e^{-(\alpha_i + \alpha_R)z} \cdot e^{-j\Omega z} dz \right) \quad (1)$$

where P_0 is the initial average power of the incident

light, m is the modulation depth, ω_m is the modulation frequency, L is the fiber length, α_i and α_R are the attenuation coefficients of the incident light and the Raman backscattered light, respectively, Ω is the spatial angular frequency, \Re represents the real part inside the parentheses, and $\chi_R(z)$ is the Raman backscattered coefficient at the location of z .

With the modulation frequency increased, the amplitude and the phase are measured to obtain the frequency response of the backscattered light signal. Equation (1) indicates that $\chi_R(z)$ can be obtained by carrying out an inverse Fourier transform on the measured frequency response, and the profile of the power of backscattered light changing with location can be obtained. Therefore, spatial resolution is achieved by the IOFDR technology.

In the Raman based DTS system, the power of the anti-Stokes component is much more sensitive to temperature, as compared to the Stokes component, because of the Boltzmann distribution of the silica molecular energy level. The DTS technology derives temperature information from the ratio between the powers of the anti-Stokes and Stokes backscattered light [13].

2.2 Principle of the three-channel simultaneous RF-LIA

The RF-LIA can be realized by using the electrical heterodyne technique, as shown in Fig. 1. The input RF signal is mixed with a local oscillator (LO) whose frequency is higher than the RF signal frequency. With a low-pass filter (LPF), the input signal is converted to an intermediate frequency (IF) signal which can be expressed as

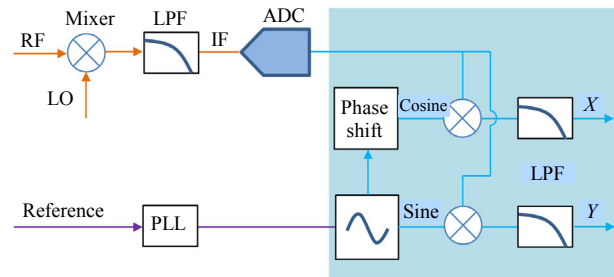


Fig. 1 Schematic diagram of the electrical heterodyne technique based RF lock-in amplifier.

$$U_{\text{IF}} = \frac{1}{2} V_{\text{RF}} V_{\text{LO}} \cos[(\omega_{\text{RF}} - \omega_{\text{LO}})t + (\varphi_{\text{RF}} - \varphi_{\text{LO}})] \quad (2)$$

where V_{RF} and V_{LO} are the amplitudes of the input RF signal and the LO signal, ω_{RF} and ω_{LO} are the frequencies of the RF signal and the LO signal, while φ_{RF} and φ_{LO} are the initial phases of the RF signal and the LO signal.

The frequency of reference signal is equal to the difference frequency between the RF signal and the LO signal, and the reference signal can be expressed as

$$U_{\text{Ref}} = \cos[(\omega_{\text{RF}} - \omega_{\text{LO}})t + \varphi_{\text{Ref}}] \quad (3)$$

where φ_{Ref} is the initial phase of the reference signal.

According to the signal detection theory of an orthogonal lock-in amplifier, the measured amplitude and phase of V_{IF} can be expressed as

$$\frac{1}{2} V_{\text{RF}} V_{\text{LO}} = 2\sqrt{X_s^2 + Y_s^2} \quad (4)$$

$$\varphi_{\text{RF}} - \varphi_{\text{LO}} - \varphi_{\text{Ref}} = \arctan\left(\frac{Y_s}{X_s}\right) \quad (5)$$

where X_s is the ‘‘in-phase’’ component of the output value, and Y_s is the ‘‘quadrature’’ component.

For an IOFDR based DTS, the initial phase is measured by a reference light channel. Therefore, the measured phase can be expressed as

$$\varphi_{\text{RL}} - \varphi_{\text{LO}} - \varphi_{\text{Ref}} = \arctan\left(\frac{Y_r}{X_r}\right) \quad (6)$$

where φ_{RL} is the initial phase of the reference light, X_r is the ‘‘in-phase’’ component of the reference light channel, and Y_r is the ‘‘quadrature’’ component.

From (4), the amplitude of the RF signal can be expressed as

$$V_{\text{RF}} = \frac{4\sqrt{X_s^2 + Y_s^2}}{V_{\text{LO}}} \quad (7)$$

From (5) and (6), the phase shift of the RF signal can be expressed as

$$\Delta\varphi = \varphi_{\text{RF}} - \varphi_{\text{RL}} = \arctan\left(\frac{Y_s}{X_s}\right) - \arctan\left(\frac{Y_r}{X_r}\right) \quad (8)$$

With this method, a multi-channel RF-LIA can be developed with a relatively simple structure and few electronic components, compared with

traditional methods. Moreover, the amplitude and the phase shift of Raman backscattered light can be measured with a high SNR improvement.

3. Experimental setup

3.1 IOFDR-based DTS setup

An IOFDR-based DTS system has been developed for well logging, as shown in Fig. 2. Due to harsh environments in oil well, the problem of hydrogen darkening in fiber is serious [14, 15]. Moreover, the caused differential attenuation between Stokes and anti-Stokes channels in the DTS system can lead to a large measurement error. Previous studies have indicated that hydrogen darkening phenomenon can be weakened by using low germanium doped single-mode fiber [16], and the variation of differential attenuation is much smaller by using a laser source whose wavelength is near 1064 nm [17]. In this scheme, the laser diode, with an emission wavelength of 1064 nm, is modulated by stepwise increased frequencies. A splitter with a coupling ratio of 1:99 splits 1% of the incident light for a reference optical signal which is detected by a photodiode (PD). The laser is launched into the single-mode fiber (SMF) with a length of 2.5 km, and the backscattered lights are detected by an avalanche photodiode (APD) module. Two Raman backscattered lights are filtered out by two wavelength division multiplexers (WDMs). A temperature reference fiber coil with a length of 22 m is used for calibration. A three-channel simultaneous RF-LIA is designed for laser modulation and signal processing.

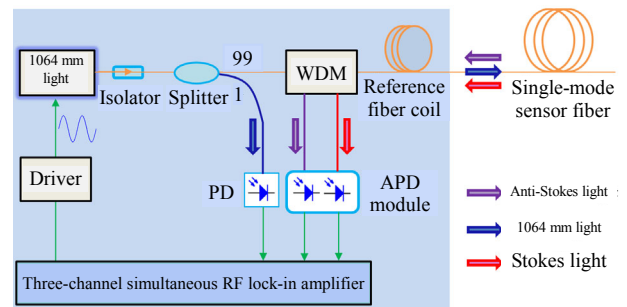


Fig. 2 Setup of the IOFDR-based single-mode fiber-optic DTS system.

3.2 Three-channel simultaneous RF-LIA design

The schematic diagram of the three-channel simultaneous RF-LIA is shown in Fig. 3. The laser modulation signal is supplied by DDS2 which is a direct digital synthesizer (DDS). The laser reference signal, the Stokes signal, and the anti-Stokes signal are mixed with an LO signal whose frequency is 8 kHz higher than the modulation frequency all the time, and the LO signal is supplied by DDS1. The LPF is used to attenuate high frequency component of the output of the mixer. As a result, the three processed signals have the same frequency of 8 kHz. The amplitude and the phase of the three ADC converted signals are calculated by the field programmable gate array (FPGA) based digital LIA. Meanwhile, the reference signal input LIA is supplied by DDS3, and its frequency is also 8 kHz. A PLL locks the reference signal and multiplies its frequency for ADC sampling clock. In order to minimize the measurement error of the phase, three DDSs are used a same crystal oscillator as their main clock. The size of this RF-LIA is 16 cm×12 cm×5 cm.

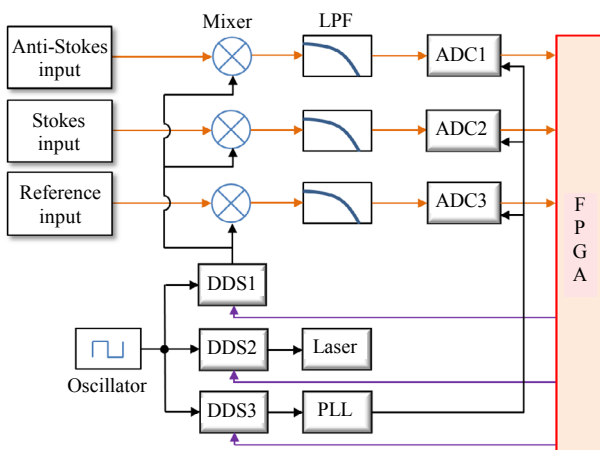


Fig. 3 Schematic diagram of the three-channel simultaneous RF lock-in amplifier.

The sample rate of ADCs is 64 times higher than the reference frequency which is 8 kHz. By using this oversampling method, the dynamic range can reach to 114 dB with a 16-bit ADC. Meanwhile, the trigger signals for sampling are generated by FPGA simultaneously to minimize the error of phase

measurement. With the high-speed DDSs, the modulation frequency can sweep from 1 kHz to 100 MHz.

With the designed RF-LIA, Raman signals can be processed while data acquiring. After modulation of all frequencies, the demodulation for distributed temperature is carried out by FPGA immediately.

4. Experimental results and discussion

4.1 SNR improvement

In order to measure the noise spectrum, the measurement frequency was stepwise increased, and the power of the laser diode was not be modulated. Therefore, the Raman backscattered light was a direct-current (DC) signal, and the LIA measured value was the noise near the frequency equal to the reference signal. When the sensor fiber was put into a temperature-controlled chamber which was set to be 30°C, the average power of the backscattered anti-Stokes light was 24.3 nW. Since the noise was relevant to the input optical power [18], the power of the laser diode has been adjusted without modulation until the output power of the backscattered anti-Stokes light to be 24.3 nW. Additionally, the standard deviation of the noise of the APD module was measured to be 5.83 mV by an oscilloscope. With the three-channel simultaneous RF-LIA based signal processing unit and a measurement time of 500 s, the measured noise of the APD module over the frequency range of 100 MHz is shown in Fig. 4.

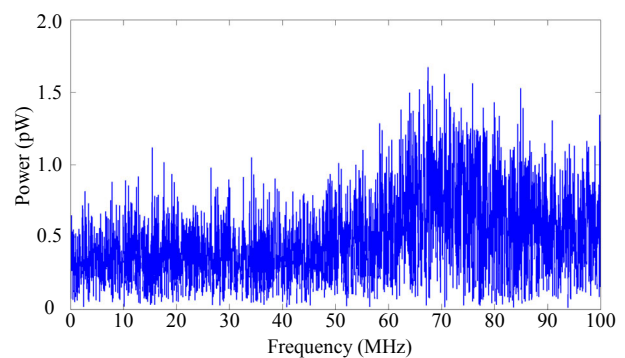


Fig. 4 Measured noise of the APD module over the frequency range of 100 MHz.

Figure 4 shows that the largest noise is near the frequency of 68 MHz. Thus an SNR measurement was taken on condition that the laser was modulated with the frequency of 68 MHz. The measured anti-Stokes signal value with an integral time of 200 ms is shown in Fig. 5.

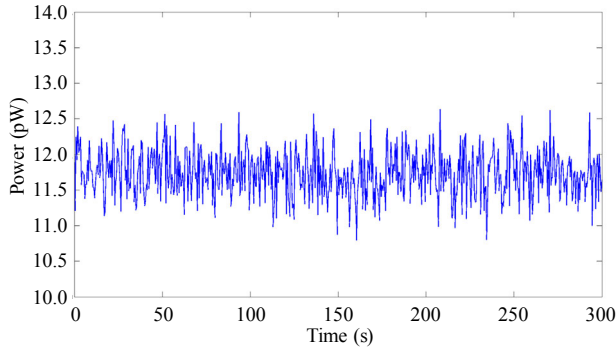


Fig. 5 Measured signal value at the modulation frequency of 68 MHz.

From Fig. 5, the root-mean-square (RMS) of the anti-Stokes signal P_S is calculated to be 11.7 pW, and the standard deviation of the noise σ_N can be calculated to be 0.33 pW. With the responsivity R of the APD module being 1.61×10^6 V/W at 1020 nm, and the gain factor G of the LIA being 11, the SNR of the LIA output SNR_o can be calculated as

$$\text{SNR}_o = 10 \cdot \lg \left(\frac{V_{So}^2}{\sigma_{No}^2} \right) = 10 \cdot \lg \left(\frac{(P_S \cdot R \cdot G)^2}{(\sigma_N \cdot R \cdot G)^2} \right) \quad (9)$$

where V_{So} is the RMS of the output signal of the LIA, and σ_{No} is the RMS of the output noise. Thus the SNR_o is calculated to be 30.9 dB.

The input noise σ_{Ni} from the oscilloscope measured value is 5.83 mV. The SNR of the LIA input SNR_i can be calculated as

$$\text{SNR}_i = 10 \cdot \lg \left(\frac{V_{Si}^2}{\sigma_{Ni}^2} \right) = 10 \cdot \lg \left(\frac{(P_S \cdot R)^2}{\sigma_{Ni}^2} \right) \quad (10)$$

where V_{Si} is the RMS of the input signal of the LIA, and σ_{Ni} is the RMS of the input noise. Thus the SNR_i is calculated to be -49.8 dB. Therefore, with this RF-LIA, the SNR has been improved from -49.8 dB to 30.9 dB. The designed RF-LIA shows a great ability of SNR improvement for weak Raman backscattered signal detection.

4.2 Frequency response measurement

With the modulation by stepwise increased frequencies, the Raman backscattered signals were measured by the RF-LIA. To reach a sampling spatial resolution of 0.5 m and a measurement range of 2.5 km, the maximum modulation frequency was set to be 100 MHz, and the frequency interval was set to be 37 kHz. When the measurement time has been set to be about 500 s, the amplitude of the measured frequency response of the anti-Stokes channel is shown in Fig. 6(a). The phase shift, which is the difference between the phases of the anti-Stokes signal and the optical reference signal, is shown in Fig. 6(b).

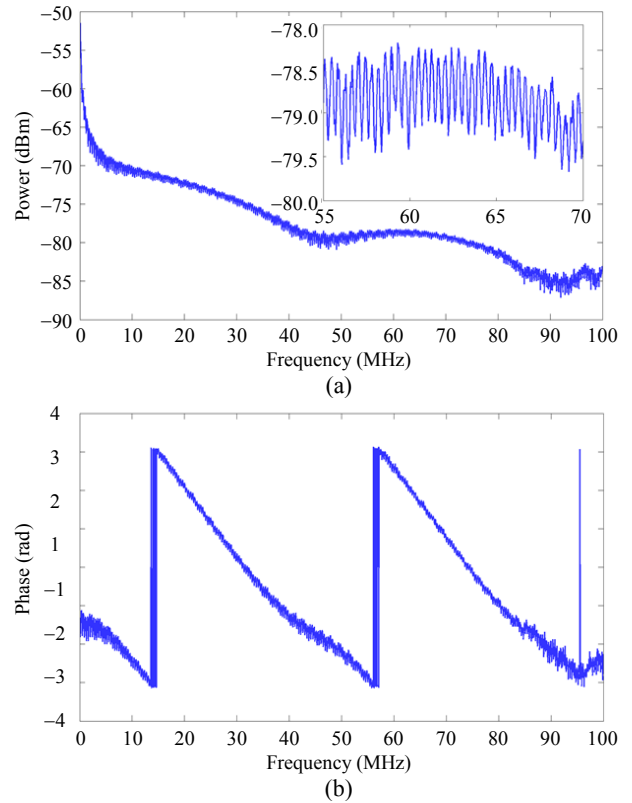


Fig. 6 Amplitude (a) and the phase shift (b) of the measured frequency response of anti-Stokes channel.

Figure 6(a) shows that the amplitude decreases significantly when the modulation frequency increases. With the modulation frequency up to 50 MHz, the power of the AC part of the backscattered light signal could decrease to picowatt level. However, the extremely weak Raman signal

can still be detected with the RF-LIA. The power changes from near -50 dBm to -90 dBm, this requires the dynamic range of the signal processing unit exceeding 80dB. Meanwhile, Fig. 6(b) shows a tendency of decrease in overall, which is caused by a shift of spatial location according to the Fourier transform properties.

4.3 Distributed temperature measurement

In order to measure the spatial resolution, the measurement should be carried out at the end of the sensing length where the SNR is the worst, so that the claimed spatial resolution is effective for the entire sensing length [19]. The temperature profile of the tested fiber with a 14 m fiber coil put into a water bath is shown in Fig. 7. A spatial resolution of 0.93 m was calculated using the 10% to 90% step response corresponding to the rising edge of a temperature change.

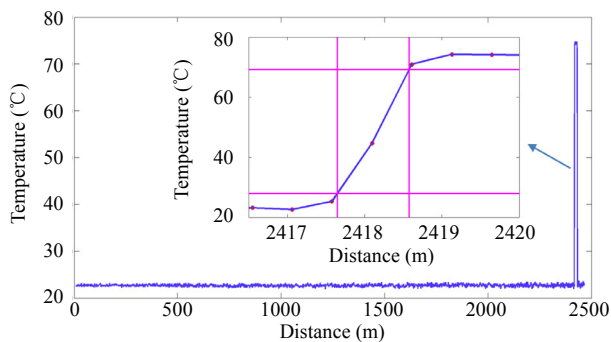


Fig. 7 Measured distributed temperature profile of the 2.5 km single-mode fiber.

20 distributed temperature profiles were measured with the measurement time of 500s. The temperature resolution which has been calculated by standard deviation is shown in Fig. 8. The solid line is an exponential fit to the calculated temperature resolution. The fit curve shows that a temperature resolution of about 0.2°C has been achieved in the entire measurement range. Due to the increasing attenuation of the propagating light along the fiber, the temperature resolution grows accordingly.

Compared with multi-mode fiber-optic DTS, the Raman scattering cross-section is much smaller in single-mode fiber-optic DTS. Additionally, the

responsivity of the detector is much lower near the wavelength of 1064 nm. The SNR is thus reduced with these two factors. Fortunately, the temperature changes slowly in oil well. In order to achieve high temperature resolution for down-hole distributed temperature measurement, long period measurement time is permitted with the single-mode fiber-optic DTS system.

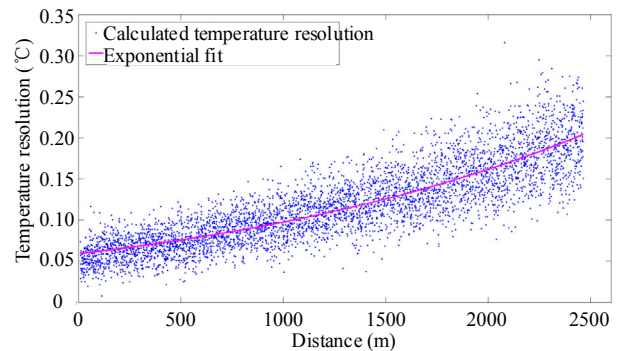


Fig. 8 Temperature resolution along the sensing fiber.

5. Conclusions

In conclusion, we have proposed a three-channel simultaneous RF-LIA based signal detection method for an IOFDR-based DTS system. A single-mode fiber-optic DTS has been designed for well logging. In order to detect weak Raman backscattered light, an FPGA based three-channel simultaneous RF-LIA with a novel and simple structure has been designed. At the modulation frequency of 68 MHz, the SNR of the anti-Stokes signal was improved from -49.8 dB to 30.9 dB. Frequency response of the tested fiber was measured over the frequency range from 36 kHz to 100 MHz, and the ability of high sensitivity and large dynamic range for measuring the Raman backscattered light was demonstrated. High spatial resolution and temperature resolution of the distributed temperature profiles have been achieved with high SNR improvement of Raman signal detection. Therefore, the designed three-channel RF-LIA is suitable for frequency response measurement of Raman backscattered light signal in the IOFDR-based DTS system.

Acknowledgment

The authors would like to acknowledge the financial supports from the National Nature Science Foundation of China (51277021, 61137005, and 61307105).

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