

Stability of Networked Control Systems with Large Delays

M.B.G. Cloosterman, N. van de Wouw, W.P.M.H. Heemels and H. Nijmeijer

Abstract—This paper proposes stability analysis techniques for Networked Control Systems (NCSs) with uncertain, time-varying network-induced delays. A discrete-time model, describing an NCS with delays, that can be both smaller and larger than the sampling interval, is presented. This model includes the effects of message rejection and vacancy sampling. The conditions are kept less conservative by exploiting the real Jordan form of the continuous-time model in the discretization. Based on this discrete-time NCS model sufficient LMI conditions are proposed for the stability analysis.

I. INTRODUCTION

Networked Control Systems (NCSs) are control systems in which (part of) the control loop is closed over a real-time network. The advantages of the use of an NCS are its flexible architecture [1] and a reduction of installation and maintenance costs [2]. The main disadvantages of NCSs are the network effects that influence the control loop, such as delays, variable sampling intervals and packet dropouts. Despite these disadvantages, NCSs are applied in a broad range of systems, e.g. mobile sensor networks, remote surgery, automated highway systems and unmanned aerial vehicles [1], [2]. In this paper the focus will be on the effects of delays on the stability of the control loop, where we restrict ourselves to systems without packet dropouts and with a constant sampling interval.

Most of the NCS literature on stability analysis deals with constant delays or time-varying delays smaller than the sampling interval. Here, we study NCS models including large delays, i.e. delays that can be both smaller and larger than the sampling interval. In [3], [4], a discrete-time NCS model, based on the NCS model of e.g. [5], [6] is proposed, for time-varying delays τ_k that vary solely in the interval $(d-1)h \leq \tau_k \leq dh$, where d is a constant integer, h the sampling interval and τ_k the time-varying delay. As a consequence, time-delays that vary in an interval larger than the sampling interval, i.e. $\tau_k \in [\tau_{min}, \tau_{max}]$, with $\tau_{max} - \tau_{min} > h$ are not considered in [3], [4]. Note that this is a fundamental difference with arbitrary time-varying delays ($\tau_{max} - \tau_{min} > h$), where message rejection can occur.

Discrete-time models that consider arbitrary time-varying delays that take values in an interval larger than the sampling

interval are described in [7] and [8]. The model in [7] is based on [5] and describes the effects of multiple control updates during one sampling interval and vacancy sampling, where no new control input becomes available during the current sampling interval. The effect of message rejection, where more recent control data becomes available before the older data is implemented and therefore the older data is discarded, is, however, not considered in [7]. In [8] another stability analysis approach is described, without an explicit definition of the NCS model for large delays. For the analysis, the uncertain time-varying delays are divided in a constant and a time-varying part, where the time-varying part is allowed to be larger than the sampling interval. This results in a set of constant and uncertain matrices. Based on an overestimation of the uncertain matrices and a Lyapunov-Krasovskii approach for discrete-time systems, sufficient conditions for the stability analysis are proposed.

An alternative modeling approach is based on impulsive delay-differential equations, in which NCSs with variable sampling intervals, time-varying delays and packet dropouts are considered, see [9]. A main advantage of this modeling approach is the possibility to incorporate time-delays larger than the sampling interval without increasing model complexity, as is the case in the discrete-time modeling approach.

In this paper, we extend the model of [7], such that it includes message rejection. Due to this discrete-time representation, it is a different modeling approach than [9], which presents models in terms of continuous-time delay impulsive systems. Compared to the work in [8], we give an explicit definition of the uncertain functions, which depend on the uncertain time-varying delay, instead of an implicit one. We rewrite the proposed large-delay NCS model, using the real Jordan form of the continuous-time system matrices, such that we can separate constant and time-varying parameters, which removes conservativeness from the analysis. Based on this model, we propose LMIs that are sufficient for the stability analysis.

The paper is organized as follows. In Section II, we introduce the discrete-time NCS model for time-variations in the delay that are larger than one sampling interval. Section III discusses the stability analysis. In Section IV, simulation results illustrating the effectiveness of the proposed approach are presented. Finally, Section V gives the conclusions.

Notation: We denote the transpose of a matrix A by A^T and we write $P > 0$ (or $P < 0$) for a positive (or negative) definite matrix. With $*$ we denote the symmetric part of a matrix, with $\dim(J)$ the dimension of the square matrix J and $0_{m,n}$ denotes a matrix of zeros of size $m \times n$.

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II. NCS MODELS FOR LARGE DELAYS

The NCS consists of a continuous-time plant, sampled with a constant sample-rate, and a discrete-time controller as is schematically depicted in Figure 1. In the model, both the computation time and the networked induced delays, i.e. the sensor-to-controller delay τ_{sc} and the controller-to-actuator delay τ_{ca} , are incorporated. Under the assumption that the sensor acts in a time-driven fashion (i.e. sampling at the times kh , $k \in \mathbb{N}$), that the controller and actuator act in an event-driven fashion (i.e. responding instantaneously on newly arrived data) and that the controller is static and time-invariant, all three delays can be combined into one single delay τ_k that delays the control input u_k with respect to the corresponding measurement y_k [10].

The continuous-time model of the NCS is given by:

$$\begin{aligned} \dot{x}(t) &= Ax(t) + Bu^*(t) \\ u^*(t) &= u_k, \text{ for } t \in [kh + \tau_k, (k+1)h + \tau_{k+1}], \end{aligned} \quad (1)$$

with $A \in \mathbb{R}^{n \times n}$, $B \in \mathbb{R}^{n \times m}$, the system matrices, $u^*(t) \in \mathbb{R}^m$ the continuous-time control input if all inputs are implemented to the plant, i.e. all data at both the controller and actuator are received in a sequential order, which means that message rejection can not occur, $x(t) \in \mathbb{R}^n$ the state, kh the sampling instants, h the sampling-interval, $u_k \in \mathbb{R}^m$ the discrete-time control input calculated from the measurements at sampling instant kh and τ_k the time-delay experienced by the output $y(kh) = x(kh)$ at sampling instant kh . At the end of this section, we will adapt the expression for $u^*(t)$, such that the effects of message rejection are included.

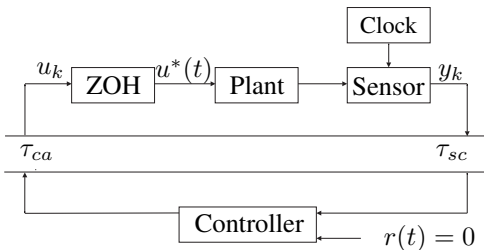


Fig. 1. Schematic overview of the networked control system.

To derive a discrete-time NCS model for time-varying delays that vary in an interval larger than the sampling-interval ($\tau_k \in [\tau_{min}, \tau_{max}]$, with $\tau_{max} - \tau_{min} > h$), including message rejection, we use the standard, discrete-time NCS model for constant large-delays, see e.g. [5]. This model is an exact discretization of (1), given by:

$$x_{k+1} = e^{Ah}x_k + \int_0^{h-\tau_{k-d+1}^*} e^{As}dsBu_{k-d+1} + \int_{h-\tau_{k-d+1}^*}^h e^{As}dsBu_{k-d}, \quad (2)$$

with $d = \lceil \frac{\tau_k}{h} \rceil$, the smallest integer larger than or equal to $\frac{\tau_k}{h}$ and $\tau_k^* = \tau_k - (d-1)h$. This model is limited to constant time-delays or delays that vary at most within one sampling interval (i.e. $[\tau_{min}, \tau_{max}] \subseteq [(d-1)h, dh]$ for some constant integer d). This can be explained using Figure 2. In Figure 2, the delays are allowed to take values in $[0, 2h]$, which shows that the number of active control inputs in one sampling

interval is variable and depends on the previous and current time-delay, which is not handled by (2).

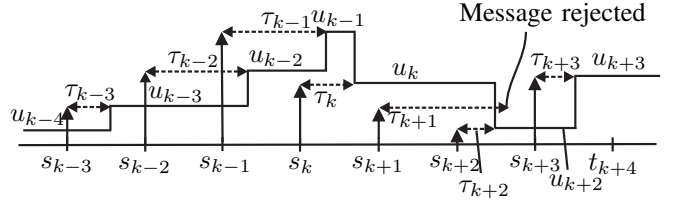


Fig. 2. Influence of time-delays that can be smaller and larger than the sampling interval (with e.g. $s_{k+1} := (k+1)h$ and $\tau_k \in [0, 2h]$).

In the case that $\tau_k \in [0, 2h]$, the model that describes the NCS consists of the following subsystems:

$$x_{k+1} = \begin{cases} e^{Ah}x_k + \int_0^{h-\tau_k} e^{As}dsBu_k + \int_{h-\tau_k}^h e^{As}dsBu_{k-1}, & \text{if } \tau_k \leq h \wedge \tau_{k-1} \leq h \\ e^{Ah}x_k + \int_0^{h-\tau_{k-1}^*} e^{As}dsBu_{k-1} + \int_{h-\tau_{k-1}^*}^h e^{As}dsBu_{k-2}, & \text{if } h \leq \tau_k \leq 2h \wedge h \leq \tau_{k-1} \leq 2h \\ e^{Ah}x_k + \int_0^h e^{As}dsBu_{k-1}, & \text{if } h \leq \tau_k \leq 2h \wedge \tau_{k-1} \leq h \\ e^{Ah}x_k + \int_0^{h-\tau_k} e^{As}dsBu_k + \int_{h-\tau_k}^{h-\tau_{k-1}^*} e^{As}dsBu_{k-1} + \int_{h-\tau_{k-1}^*}^h e^{As}dsBu_{k-2}, & \text{if } \tau_k \leq h \wedge h \leq \tau_{k-1} \leq 2h \wedge \tau_{k-1} - h < \tau_k \\ e^{Ah}x_k + \int_0^{h-\tau_k} e^{As}dsBu_k + \int_{h-\tau_k}^h e^{As}dsBu_{k-2}, & \text{if } \tau_{k-1} - h \geq \tau_k, \end{cases} \quad (3)$$

with $\tau_{k-1}^* = \tau_{k-1} - h$. The last subsystem describes the case where message rejection occurs, which results in loss of some control data (u_{k-1} in this case). Moreover, the second subsystem corresponds to (2) (with $d = 2$). An NCS modeling approach that considers these different subsystems, except message rejection, is given in [7]. We will use their model description, which is based on (2), to develop an NCS model, including message rejection. In our model, during the sampling interval $[kh, kh+h)$, the control $u^*(t)$ takes values from the delayed inputs u_j at the random instants $kh + t_j^k$, with $0 \leq t_j^k \leq h$. The integer j satisfies $k - \bar{d} \leq j \leq k - \underline{d}$, with $\underline{d} = \lfloor \frac{\tau_{min}}{h} \rfloor$, the largest integer smaller than or equal to $\frac{\tau_{min}}{h}$ and $\bar{d} = \lceil \frac{\tau_{max}}{h} \rceil$ the smallest integer larger than or equal to $\frac{\tau_{max}}{h}$. The time $kh + t_j^k$ depends on the time-delays and the values of \underline{d} and \bar{d} , according to:

$$t_j^k = \min\{\max\{0, \tau_j - (k-j)h\}, \max\{0, \tau_{j+1} - (k-j-1)h\}, \dots, \max\{0, \tau_{k-\underline{d}} - \underline{d}h\}, h\} \quad (4)$$

with $j \in \{k - \bar{d}, k - \bar{d} + 1, \dots, k - \underline{d}\}$, the superscript k indicating the sampling interval $[kh, kh+h)$, $t_j^k \leq t_{j+1}^k$ and $0 = t_{k-\bar{d}}^k \leq t_{k-\bar{d}+1}^k \leq \dots \leq t_{k-\underline{d}}^k \leq t_{k-\underline{d}+1}^k := h$.

Then, the NCS model for large delays becomes:

$$x_{k+1} = e^{Ah}x_k + \sum_{j=k-\bar{d}}^{k-\underline{d}} \int_{h-t_{j+1}^k}^{h-t_j^k} e^{As}dsBu_j \quad (5)$$

with $t_{k-d+1}^k := h$, t_j^k defined in (4) for $k - \bar{d} \leq j \leq k - \underline{d}$. This model contains all possible control inputs that can be active during the sampling interval $[kh, kh + h)$. Note that $t_j^k = t_{j+1}^k$ corresponds to the situation that the integral related to u_j in (5) is zero and results in an inactive control input u_j during the sampling interval $[kh, kh + h)$. This corresponds to the case of message rejection, vacancy sampling or a control input that has already been implemented in the previous sampling interval or will be implemented in the next sampling interval, due to the size of the time-delay.

Note that (5) is sufficient to model all the different situations that are given in (3), because each subsystem can be obtained by the definition of t_j^k as in (4).

Remark Equation (5) was also stated in [7], however, without the explicit definition of t_j^k as we presented in (4). Moreover, in [7] it is implicitly assumed that message rejection does not occur, as $t_j^k < t_{j+1}^k$ should hold for all $k - \bar{d} \leq j \leq k - \underline{d}$. Finally, the model proposed here exhibits less uncertain parameters than that in [7], because we consider only t_j^k as uncertain, time-varying parameters, while in [7] additional parameters are introduced that denote if a control input is active in the sampling interval $[kh, kh + h)$.

To make the model of (5) suitable for the stability analysis, we rewrite it in a state-space form with the state-vector $\xi_k = (x_k^T \ u_{k-1}^T \ u_{k-2}^T \ \dots \ u_{k-\bar{d}}^T)^T$. Then, the state-equation of the NCS model is given by:

$$\xi_{k+1} = M(\tau_k)\xi_k + N(\tau_k)u_k, \quad (6)$$

$$\text{with } M(\tau_k) = \begin{pmatrix} e^{Ah} & \tilde{B}_1 & \tilde{B}_2 & \dots & \tilde{B}_{\bar{d}} \\ 0 & 0 & 0 & \dots & 0 \\ 0 & I & 0 & \dots & 0 \\ \vdots & & \ddots & \dots & \\ 0 & \dots & 0 & I & 0 \end{pmatrix},$$

$$N(\tau_k) = (\tilde{B}_0^T \ I \ 0 \ \dots \ 0)^T \text{ and}$$

$$\tilde{B}_\rho(\tau_k) = \int_{h-t_{k-\rho}^k}^{h-t_{k-\rho}^k} e^{As} ds B \quad (7)$$

for $\rho \in \{0, 1, \dots, \bar{d}\}$ and $t_{k-\rho}^k$ defined in (4), with $j = k - \rho$. Note that for $\rho < \underline{d}$, it holds that $\tilde{B}_\rho = 0$.

Based on the insights obtained above, we can also adapt the control $u^*(t)$ in the continuous-time NCS model (1), such that it allows for message rejection of the current input u_k . Let us define $k^*(t) := \max\{k \in \mathbb{N} | kh + \tau_k \leq t\}$, which denotes the most recent control input available at time t . Then it holds for the NCS of (1) that

$$u^*(t) = u_{k^*}(t), \quad (8)$$

with $u^*(t)$ a piecewise constant signal. This is a kind of implicit description of the ZOH-based control signal in the NCS. To follow the common representation of the control signal in the NCS literature, we make this more explicit in the following paragraph.

Let us define the additional integer parameter v_k as the smallest integer, with $v_k \geq 1$, such that u_{k+v_k} is a control

input that is implemented after $kh + h$. In other words, if u_k is implemented, v_k denotes the next input u_{k+v_k} that is implemented after u_k . If u_k is rejected v_k denotes the next input u_{k+v_k} that is implemented after u_{k-1} , and so on if u_{k-1} is rejected as well. The parameter v_k is defined as:

$$v_k = \begin{cases} 1, & \text{if } \tau_{k+1} - h < \tau_{k+2} \wedge \tau_{k+1} - 2h < \tau_{k+3} \wedge \\ & \dots \wedge \tau_{k+1} - \bar{d}h < \tau_{k+\bar{d}+1} \\ 2, & \text{if } \tau_{k+1} - h \geq \tau_{k+2} \wedge \tau_{k+2} - h < \tau_{k+3} \wedge \\ & \dots \wedge \tau_{k+2} - (\bar{d}-1)h < \tau_{k+\bar{d}+1} \\ \vdots \\ \bar{d}, & \text{if } \tau_{k+1} - (\bar{d}-1)h \geq \tau_{k+\bar{d}} \wedge \\ & \tau_{k+2} - (\bar{d}-2)h \geq \tau_{k+\bar{d}} \wedge \dots \wedge \\ & \tau_{k+\bar{d}-1} - h \geq \tau_{k+\bar{d}} \wedge \tau_{k+\bar{d}} - h < \tau_{k+\bar{d}+1} \\ \bar{d} + 1, & \text{if } \tau_{k+1} - \bar{d}h \geq \tau_{k+\bar{d}+1} \wedge \\ & \tau_{k+2} - (\bar{d}-1)h \geq \tau_{k+\bar{d}+1} \wedge \dots \wedge \\ & \tau_{k+\bar{d}-1} - 2h \geq \tau_{k+\bar{d}+1} \wedge \tau_{k+\bar{d}} - h = \tau_{k+\bar{d}+1}. \end{cases} \quad (9)$$

Based on this definition of v_k , the continuous-time NCS model that incorporates delays larger than the sampling interval and message rejection becomes, for known values of v_k :

$$\dot{x}(t) = Ax(t) + Bu^*(t)$$

$$u^*(t) =$$

$$\begin{cases} u_k, & \text{for } t \in [kh + \tau_k, (k + v_k)h + \tau_{k+v_k}] \\ & \wedge \tau_k - v_k h < \tau_{k+v_k} \wedge 1 \leq v_k \leq \bar{d} + 1 \\ u_{k-1}, & \text{for } t \in [(k-1)h + \tau_{k-1}, (k + v_k)h + \tau_{k+v_k}] \\ & \wedge \tau_k - v_k h \geq \tau_{k+v_k} \\ & \wedge \tau_{k-1} - (v_k + 1)h < \tau_{k+v_k} \wedge 1 \leq v_k \leq \bar{d} \\ \vdots \\ u_{k-\bar{d}+1}, & \text{for } t \in [(k-\bar{d}+1)h + \tau_{k-\bar{d}+1}, (k + v_k)h + \tau_{k+v_k}] \\ & \wedge \tau_k - v_k h \geq \tau_{k+v_k} \wedge \\ & \tau_{k-1} - (v_k + 1)h \geq \tau_{k+v_k} \wedge \dots \wedge \\ & \tau_{k-\bar{d}+2} - (v_k + \bar{d} - 2)h \geq \tau_{k+v_k} \wedge \\ & \tau_{k-\bar{d}+1} - (v_k + \bar{d} - 1)h < \tau_{k+v_k} \wedge 1 \leq v_k \leq 2 \\ u_{k-\bar{d}}, & \text{for } t \in [(k-\bar{d})h + \tau_{k-\bar{d}}, (k + v_k)h + \tau_{k+v_k}] \wedge \\ & \tau_k - v_k h \geq \tau_{k+v_k} \wedge \\ & \tau_{k-1} - (v_k + 1)h \geq \tau_{k+v_k} \wedge \dots \wedge \\ & \tau_{k-\bar{d}+1} - (v_k + \bar{d} - 1)h \geq \tau_{k+v_k} \wedge v_k = 1, \end{cases} \quad (10)$$

with $k = \lfloor \frac{t}{h} \rfloor$. Note that in the last subsystem in (10), $\tau_{k-\bar{d}+1} - (v_k + \bar{d} - 1)h > \tau_{k+v_k}$ will never occur, but $\tau_{k-\bar{d}+1} - (v_k + \bar{d} - 1)h = \tau_{k+v_k}$ is still possible if $\tau_{max} = \bar{d}$.

III. STABILITY OF NCSS WITH LARGE DELAYS

In this section, we propose techniques for the stability analysis of the NCS model described in Section II. To do so, we first define a different formulation of the NCS model of (6). To solve the integrals in the matrices \tilde{B}_ρ in (7) in a general way, the real Jordan form [11], [12] of the continuous-time system matrix A is used, which is given by:

$$A = QJQ^{-1}, \quad (11)$$

with J the real Jordan form, representing the eigenvalues and Q a matrix that contains the generalized eigenvectors. Suppose that A has p distinct eigenvalues $\lambda_{\tilde{i}}$, with $J_{\tilde{i}, \tilde{j}}$ the corresponding Jordan blocks for the eigenvalue $\lambda_{\tilde{i}}$ and $\tilde{j} = \{1, 2, \dots, g_{\tilde{i}}\}$, with $g_{\tilde{i}}$ the geometric multiplicity of the

\tilde{i}^{th} eigenvalue, with $\tilde{i} = 1, 2, \dots, p$. Then, it holds, for real eigenvalues $\lambda_{\tilde{i}}$, that:

$$e^{Js} = \sum_{\tilde{i}=1}^p \sum_{j=0}^{a_{\tilde{i}}-1} \frac{s^j}{j!} e^{\lambda_{\tilde{i}}s} S_{\tilde{i},j}, \quad (12)$$

with $S_{\tilde{i},j}$ an appropriate matrix of the same dimension as J , with a one at the matrix entries corresponding to $\frac{s^j}{j!} e^{\lambda_{\tilde{i}}s}$ and a zero at all other matrix entries and $a_{\tilde{i}} \in \mathbb{Z}^+$ the size of the largest Jordan block that corresponds to $\lambda_{\tilde{i}}$, i.e.

$$a_{\tilde{i}} = \max_{j \in \{1, 2, \dots, g_{\tilde{i}}\}} (\dim J_{\tilde{i},j}). \quad (13)$$

Similar expressions can be obtained for complex eigenvalues.

Rewriting (6), (7), using (11) and (12), leads to the following general NCS representation:

$$\xi_{k+1} = \left(F_0 + \sum_{i=1}^{\beta} \alpha_i F_i \right) \xi_k + \left(G_0 + \sum_{i=1}^{\beta} \alpha_i G_i \right) u_k, \quad (14)$$

with F_i and G_i constant matrices that are obtained by solving the integrals in (6), (7) with A replaced by (11) and α_i , $i \in \{1, 2, \dots, \beta\}$, a time-varying parameter that depends on the eigenvalue $\lambda_{\tilde{i}}$, h and one of the time-varying delays introduced through t_j^k in (4). The parameter β denotes the number of time-varying parameters in the sampling interval $[kh, kh + h)$:

$$\beta = (\bar{d} - \underline{d}) \nu, \quad (15)$$

with ν the number of parameters (from (12)) that depend on the eigenvalues of A :

$$\nu = \sum_{\tilde{i}=1}^p a_{\tilde{i}}, \quad (16)$$

with ν always smaller than or equal to n . As an illustration, the matrices F_i and G_i , $i = \{0, 1, \dots, \beta\}$, are given for the case with all eigenvalues equal to zero in Appendix II.

A. Stability Analysis

To derive stability conditions for the discrete-time NCS model (6), we adopt the control law

$$u_k = -K\xi_k \quad (17)$$

with $K \in \mathbb{R}^{m \times (\bar{d}m+n)}$. Note that the state-feedback control law $u_k = -\bar{K}x_k$, is a special case of (17), with $K = (\bar{K} \ 0)$, $\bar{K} \in \mathbb{R}^{m \times n}$ and 0 a matrix with zeros. System (14), with control law (17) contains the uncertain time-varying parameters α_i , which may be nonlinear in the parameter t_j^k . These parameters form, together with the constant matrices F_i and G_i , $i = \{0, 1, \dots, \beta\}$, sets of matrices that describe all possible system equations of (6):

$$\mathcal{F} = \left\{ F_0 + \sum_{i=1}^{\beta} \alpha_i(t_j^k) F_i : t_j^k \in [t_{j,min}^k, t_{j,max}^k] \right\}$$

$$\mathcal{G} = \left\{ G_0 + \sum_{i=1}^{\beta} \alpha_i(t_j^k) G_i : t_j^k \in [t_{j,min}^k, t_{j,max}^k] \right\}. \quad (18)$$

To determine the minimum and maximum values of the uncertain parameters α_i in (18), we define the minimum and

maximum values of t_j^k , dependent of the size of the time-delays. We define the minimum value of t_j^k as:

$$t_{j,min}^k = \begin{cases} \tau_{min} - \underline{d}h & \text{if } j = k - \underline{d} \\ 0 & \text{if } j < k - \underline{d}, \end{cases} \quad (19)$$

and the maximum value of t_j^k as:

$$t_{j,max}^k = \begin{cases} h & \text{if } j > k - \bar{d} + 1 \\ \tau_{max} - (\bar{d} - 1)h & \text{if } j = k - \bar{d} + 1. \end{cases} \quad (20)$$

To guarantee the stability of the equilibrium point $\xi = 0$ of system (14), with the uncertain parameters t_j^k , defined in (4), we will use a common quadratic Lyapunov function $V(\xi_k) = \xi_k^T P \xi_k$. Consequently, the following LMI condition is sufficient:

$$P = P^T > 0$$

$$C(\tau)^T P C(\tau) - P < -\gamma P, \forall \tau \in [\tau_{min}, \tau_{max}], \quad (21)$$

with $C(\tau) = F_0 - G_0 K + \sum_{i=1}^{\beta} \alpha_i (F_i - G_i K)$ and $0 \leq \gamma < 1$. This is, based on the Schur complement, equal to:

$$\begin{pmatrix} (1-\gamma)P & * \\ P(F_0 - G_0 K + \sum_{i=1}^{\beta} \alpha_i (F_i - G_i K)) & P \end{pmatrix} > 0. \quad (22)$$

Obviously, (22) represents an infinite number of LMIs. In Theorem 1, we will propose a stability condition for $\tau_k \in [\tau_{min}, \tau_{max}]$, with $0 \leq \tau_{min} \leq \tau_{max}$, based on a finite number of LMIs.

Theorem 1: Consider the NCS of (6), with a known controller (17) and time-varying delays taken from a bounded set $\tau_k \in [\tau_{min}, \tau_{max}]$, $0 \leq \tau_{min} \leq \tau_{max}$. Define the sets of matrices $\mathcal{H}_{\mathcal{F}}$ and $\mathcal{H}_{\mathcal{G}}$:

$$\mathcal{H}_{\mathcal{F}} = \left\{ \bar{F}_0 + \sum_{i=1}^{\beta} \delta_i \bar{F}_i : \delta_i \in \{0, 1\}, i = \{1, 2, \dots, \beta\} \right\},$$

$$\mathcal{H}_{\mathcal{G}} = \left\{ \bar{G}_0 + \sum_{i=1}^{\beta} \delta_i \bar{G}_i : \delta_i \in \{0, 1\}, i = \{1, 2, \dots, \beta\} \right\}, \quad (23)$$

with $\bar{F}_0 = F_0 + \sum_{i=1}^{\beta} \underline{\alpha}_i F_i$, $\bar{F}_i = (\bar{\alpha}_i - \underline{\alpha}_i) F_i$, $\bar{G}_0 = G_0 + \sum_{i=1}^{\beta} \underline{\alpha}_i G_i$, $\bar{G}_i = (\bar{\alpha}_i - \underline{\alpha}_i) G_i$, and

$$\bar{\alpha}_i = \max_{t_j^k \in [t_{j,min}^k, t_{j,max}^k]} \alpha_i(t_j^k),$$

$$\underline{\alpha}_i = \min_{t_j^k \in [t_{j,min}^k, t_{j,max}^k]} \alpha_i(t_j^k), \quad (24)$$

the maximum and minimum value of α_i , respectively, with $t_{j,min}^k$ and $t_{j,max}^k$ defined in (19) and (20), respectively.

If there exist a matrix $P \in \mathbb{R}^{(n+\bar{d}m) \times (n+\bar{d}m)}$ and a scalar $0 \leq \gamma < 1$, such that the following LMI conditions are satisfied:

$$\begin{pmatrix} (1-\gamma)P & (H_{F,s} - H_{G,s}K)^T P \\ P(H_{F,s} - H_{G,s}K) & P \end{pmatrix} > 0, \quad (25)$$

$$\forall H_{F,s} \in \mathcal{H}_{\mathcal{F}} \text{ and } \forall H_{G,s} \in \mathcal{H}_{\mathcal{G}},$$

and $s = \{1, 2, \dots, 2^{\beta}\}$, then (10), (17) is GAS for any sequence of time-varying delays $\tau \in [\tau_{min}, \tau_{max}]$.

Proof: The proof is given in Appendix I. ■

These LMIs contain only stability analysis results. Note that performance measures can be included in these LMIs as well. In [13], the LMIs are augmented such that a certain ISS bound can be guaranteed in the face of disturbances.

IV. ILLUSTRATIVE EXAMPLE

In this section, we will apply the proposed results to a second-order motion control example, obtained from the document printing domain, as in [14]. We limit ourselves to one single motor driving one roller pair that is used to transport a sheet through part of the printer paperpath. The continuous-time motor-roller model is given by:

$$\begin{aligned} \dot{x} &= Ax + Bu \\ y &= Cx, \end{aligned} \quad (26)$$

with $A = \begin{pmatrix} 0 & 1 \\ 0 & 0 \end{pmatrix}$, $B = \begin{pmatrix} 0 \\ \frac{nr_R}{J_M + n^2 J_R} \end{pmatrix}$, $C = \begin{pmatrix} 1 & 0 \\ 0 & 1 \end{pmatrix}$ and $x = (x_s^T \ \dot{x}_s^T)^T$ the state vector, which contains the sheet position and velocity. Moreover, $J_M = 1.95 \cdot 10^{-5} \text{kgm}^2$ the inertia of the motor, $J_R = 6.5 \cdot 10^{-5} \text{kgm}^2$ the inertia of the roller, $r_R = 14 \cdot 10^{-3} \text{m}$ the radius of the roller, $n = 0.2$ the transmission ratio between motor and roller and u the motor torque. We assume that the sampling interval $h = 1 \text{ms}$ is constant and that the state-feedback controller is given by $u_k = -\bar{K}x_k$, with $\bar{K} = (K_1 \ K_2)$ and a constant position controller gain $K_1 = 50$. We determine the controller gains K_2 that still stabilize the system with time-varying delays $\tau_k \in [0, \tau_{max}]$, with $\tau_{max} \leq 2h$, according to Theorem 1 with $\gamma = 0$. The maximum and minimum allowable controller gains K_2 are given by the solid line in Figure 3. Note that for delays larger than the sampling interval h , the possibility of message rejection is included, as given in (5), (4). Compared to the previously published stability conditions in [14], which are depicted by the dotted line in Figure 3, the results obtained by Theorem 1 are clearly less conservative, due to the usage of the Jordan form representation of (14) of the NCS, which results in a reduction of the number of LMIs and a much tighter overapproximation of F_i and G_i than in [14]. The dashed line in Figure 3 gives the values of a periodic delay sequence with two delays $(\tau_a, \tau_b, \tau_a, \tau_b, \dots)$, with $\tau_a = 0.2 \text{ms}$ and $\tau_b = 0.6 \text{ms}$ ($\bar{K} = [50 \ 11.8]$, $h = 1 \text{ms}$), that yields an unstable closed-loop system. However, for constant delays (i.e. only τ_a or only τ_b) the corresponding system is stable (see for more details [14]). For comparison, the minimum and maximum allowable controller gains for constant time-delays equal to τ_{max} are depicted by the dash-dotted line in Figure 3. Such examples underline the need for stability results for time-varying delays. We remark that the difference between the lines for constant and time-varying delays is similar for other values of K_1 . This difference reveals the fact that the stability bound is hardly conservative.

V. CONCLUSIONS AND FUTURE WORKS

In this paper we extended the NCS model for large delays of [7] to incorporate the effect of message rejection. Moreover, we introduced an explicit definition of this extended discrete-time NCS model. For this NCS model, sufficient LMI conditions for stability analysis are proposed. By using the real Jordan form of the original continuous-time plant, the number of uncertain parameters is much smaller than in

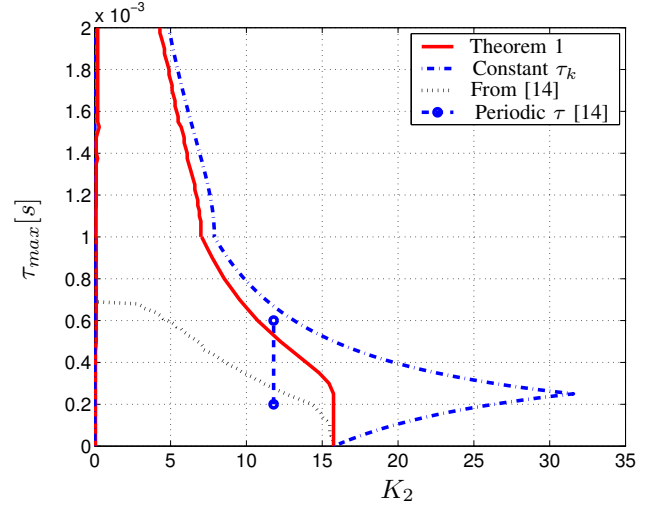


Fig. 3. Minimum and maximum allowable controller gains K_2 , for $h = 1 \text{ms}$, $K_1 = 50$ and time-varying delays in the interval $[0, \tau_{max}]$ for Theorem 1 and based on [14], and for constant delays equal to τ_{max} .

[14], thereby resulting in a reduction of the number of LMIs and the conservatism, as illustrated by the example.

Future work will deal with a model extension including that packet dropouts.

APPENDIX I
PROOF OF THEOREM 1

The proof of Theorem 1 consists of three parts. First, we exploit a convex overapproximation of the sets \mathcal{F} and \mathcal{G} , defined in (18). Second, we prove the stability of the discrete-time NCS model, based on the common quadratic Lyapunov function $V(\xi_k) = \xi_k^T P \xi_k$. Third, we investigate the intersample behavior to prove stability of the continuous-time NCS model (10), (17). For the time-varying parameter α_i , given in (24), we can write any $\alpha_i \in [\underline{\alpha}_i, \bar{\alpha}_i]$ as $\alpha_i = \underline{\alpha}_i + \delta_i(\bar{\alpha}_i - \underline{\alpha}_i)$, for some $\delta_i \in [0, 1]$ and $i = \{1, 2, \dots, \beta\}$. Hence, the sets $\bar{\mathcal{F}}$ and $\bar{\mathcal{G}}$, are defined as:

$$\begin{aligned} \bar{\mathcal{F}} &= \left\{ \bar{F}_0 + \sum_{i=1}^{\beta} \delta_i \bar{F}_i : \delta_i \in [0, 1], i = \{1, 2, \dots, \beta\} \right\}, \\ \bar{\mathcal{G}} &= \left\{ \bar{G}_0 + \sum_{i=1}^{\beta} \delta_i \bar{G}_i : \delta_i \in [0, 1], i = \{1, 2, \dots, \beta\} \right\}, \end{aligned}$$

with $\bar{F}_0 = F_0 + \sum_{i=1}^{\beta} \underline{\alpha}_i F_i$, $\bar{F}_i = (\bar{\alpha}_i - \underline{\alpha}_i) F_i$, $\bar{G}_0 = G_0 + \sum_{i=1}^{\beta} \underline{\alpha}_i G_i$, $\bar{G}_i = (\bar{\alpha}_i - \underline{\alpha}_i) G_i$. This is an overapproximation of the set \mathcal{F} and \mathcal{G} in the sense that $\mathcal{F} \subseteq \bar{\mathcal{F}}$ and $\mathcal{G} \subseteq \bar{\mathcal{G}}$, respectively. Due to the definition of the new uncertainty parameters δ_i , the sets $\bar{\mathcal{F}}$ and $\bar{\mathcal{G}}$ are still infinite. However, each matrix in this set can be written as a convex combination of the generators of this set, which are defined as the set $\mathcal{H}_{\mathcal{F}}$ and $\mathcal{H}_{\mathcal{G}}$ in (23). Note that the set $\mathcal{H}_{\mathcal{F}}$ and $\mathcal{H}_{\mathcal{G}}$ consist of 2^{β} matrices, which we denote individually by $H_{F,s}$, $H_{G,s}$, $s = \{1, 2, \dots, 2^{\beta}\}$. Based on these generators, a convex overapproximation of $\bar{\mathcal{F}}$ and $\bar{\mathcal{G}}$ can be given by:

$$\begin{aligned} \text{co}(\mathcal{H}_{\mathcal{F}}) &= \left\{ \sum_{s=1}^{2^{\beta}} (\mu_s H_{F,s}) : \sum_{s=1}^{2^{\beta}} \mu_s = 1, \mu_s \in [0, 1], \right. \\ &\quad \left. s = \{1, 2, \dots, 2^{\beta}\} \right\}, \\ \text{co}(\mathcal{H}_{\mathcal{G}}) &= \left\{ \sum_{s=1}^{2^{\beta}} (\mu_s H_{G,s}) : \sum_{s=1}^{2^{\beta}} \mu_s = 1, \mu_s \in [0, 1], \right. \\ &\quad \left. s = \{1, 2, \dots, 2^{\beta}\} \right\}, \end{aligned}$$

in the sense that

$$\begin{aligned} \mathcal{F} &\subseteq \bar{\mathcal{F}} \subseteq \text{co}(\mathcal{H}_{\mathcal{F}}), \\ \mathcal{G} &\subseteq \bar{\mathcal{G}} \subseteq \text{co}(\mathcal{H}_{\mathcal{G}}). \end{aligned} \quad (27)$$

Next, we show that indeed (25) is sufficient to guarantee the satisfaction of (22). Since (25) holds for all $H_F \in \mathcal{H}_{\mathcal{F}}$ and $H_G \in \mathcal{H}_{\mathcal{G}}$, for any $\mu_s \geq 0$ and $\sum_{s=1}^{2^\beta} \mu_s = 1$, (23) implies

$$\begin{aligned} 0 &< \sum_{s=1}^{2^\beta} \mu_s \begin{pmatrix} (1-\gamma)P & * \\ P(H_{F,s} - H_{G,s}K) & P \end{pmatrix} \\ &= \begin{pmatrix} (1-\gamma)P & * \\ \sum_{s=1}^{2^\beta} \mu_s P(H_{F,s} - H_{G,s}K) & P \end{pmatrix}. \end{aligned} \quad (28)$$

Consequently, it holds that:

$$\begin{pmatrix} (1-\gamma)P & * \\ P(\bar{H}_{F,s} - \bar{H}_{G,s}K) & P \end{pmatrix} > 0, \quad (29)$$

$\forall \bar{H}_{F,s} \in \text{co}(\mathcal{H}_{\mathcal{F}})$ and $\forall \bar{H}_{G,s} \in \text{co}(\mathcal{H}_{\mathcal{G}})$, $s \in \{1, 2, \dots, 2^\beta\}$. Based on (27), we have that (29) implies (22), which is, based on the Schur complement, equal to (21). This shows that $V(\xi_k) = \xi_k^T P \xi_k$ is a common quadratic Lyapunov function for (14), (17) which proves GAS of the origin $\xi = 0$ of (14), (17) and by equivalence of (6), (17).

With a similar reasoning as in [14], it can be proven that the intersample behavior (and therefore the continuous-time system) is GAS if the NCS model is GAS, i.e. the LMIs (25) are feasible. This proves GAS of $x = 0$ of (10), (17).

APPENDIX II

JORDAN FORMS OF THE LARGE DELAY NCS MODEL

For the case with all eigenvalues equal to zero the parameter α_i in (14) is defined as:

$$\alpha_i = \begin{cases} \frac{(h - t_{k-d}^k)^{\check{j}}}{\check{j}!}, & \text{for } \check{j} = i - 1 \wedge i \in \{1, 2, \dots, \nu\}, \\ \frac{(h - t_{k-d+1}^k)^{\check{j}}}{\check{j}!}, & \text{for } \check{j} = i - \nu - 1 \wedge \\ i \in \{\nu + 1, \nu + 2, \dots, 2\nu\}, \\ \vdots \\ \frac{(h - t_{k-d+1}^k)^{\check{j}}}{\check{j}!}, & \text{for } \check{j} = i - (\beta - \nu + 1) \wedge \\ i \in \{\beta - \nu + 1, \dots, \beta\}. \end{cases}$$

The corresponding matrices are given by:

$$F_0 = \begin{pmatrix} \Theta_1 & 0_{n,m} & 0_{n,m} & \dots & \Theta_2 \\ 0 & 0 & 0 & \dots & 0 \\ 0 & I & 0 & \dots & 0 \\ \vdots & & & \ddots & \vdots \\ 0 & \dots & 0 & I & 0 \end{pmatrix}, F_i = \begin{pmatrix} \Psi_i \\ 0_{\bar{d}m, n+\bar{d}m} \end{pmatrix},$$

with $\Theta_1 = Qe^{Jh}Q^{-1}$, $\Theta_2 = Q \sum_{\check{j}=0}^{\alpha_i-1} \frac{h^{\check{j}+1}}{(\check{j}+1)\check{j}!} S_{i,\check{j}} Q^{-1}B$ and

$$G_0 = \begin{pmatrix} 0_{n,m} \\ I_{m,m} \\ 0_{(\bar{d}-1)m,m} \end{pmatrix}, G_i = \begin{pmatrix} \Xi \\ 0_{\bar{d}m,m} \end{pmatrix}.$$

Before we give Ψ_i and Ξ_i , let us first define $\Upsilon_i = QT_iQ^{-1}B$, $\check{s}_1 = (\bar{d}-\underline{d}-1)m$, $\check{s}_2 = \check{s}_1 - m$ and $\check{s}_3 = \check{s}_2 - m$. Then, it holds that

$$\Xi_i = \begin{cases} \Upsilon_i, & \text{if } i \in \{1, 2, \dots, \nu\} \wedge \underline{d} = 0 \\ 0_{n,m}, & \text{if } i > \nu \wedge \underline{d} = 0 \text{ or } \underline{d} > 0, \end{cases}$$

$$\Psi_i = \begin{cases} \begin{pmatrix} 0_{n,n} & -\Upsilon_i & 0_{n,\check{s}_1} \\ 0_{n,n+\bar{d}m} & \Upsilon_i & -\Upsilon_i & 0_{n,\check{s}_2} \end{pmatrix}, & \text{if } i \in \{1, 2, \dots, \nu\} \wedge \underline{d} = 0, \\ & \text{if } i \in \{\nu + 1, \nu + 2, \dots, 2\nu\} \wedge \underline{d} = 0, \\ & \text{or } i \in \{1, 2, \dots, \nu\} \wedge \underline{d} > 0, \\ \begin{pmatrix} 0_{n,n+(\underline{d}+1)m} & \Upsilon_i & -\Upsilon_i & 0_{n,\check{s}_3} \end{pmatrix}, & \text{if } i \in \{2\nu + 1, 2\nu + 2, \dots, 3\nu\} \wedge \underline{d} = 0 \\ & \text{or } i \in \{\nu + 1, \nu + 2, \dots, 2\nu\} \wedge \underline{d} > 0, \\ \vdots \\ \begin{pmatrix} 0_{n,n+(\bar{d}-2)m} & \Upsilon_i & -\Upsilon_i \end{pmatrix}, & \text{if } i \in \{(\bar{d}-\underline{d}-1)\nu + 1, \dots, \beta\} \end{cases}$$

and for $\underline{d} > 0$ it holds that $\Xi_i = 0_{n,m} \forall i \in \{1, 2, \dots, \beta\}$. Moreover, it holds that:

$$T_i = \begin{cases} S_{1,\check{j}} & \text{for } \check{j} = i - 1 \wedge i \in \{1, 2, \dots, \nu\}, \\ S_{1,\check{j}} & \text{for } \check{j} = i - \nu - 1 \wedge i \in \{\nu + 1, \nu + 2, \dots, 2\nu\}, \\ \vdots \\ S_{1,\check{j}} & \text{for } \check{j} = i - \beta + \nu - 1 \wedge i \in \{\beta - \nu + 1, \dots, \beta\}. \end{cases}$$

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